## ham



## magazine


hro
focus
on
communications
technology
the magic jar: origin of the Hertian antenna $~$ low-cost UHF tower • custom-built trap antenna " "smart" frequency counter - top-band, top-loaded vertical. VHF/UHF power dividers - Yagi algorithms $\bullet L / C$ measurement technigue e quick Smith chart impedance matching

# ICOM IC-27H <br> Ultra Compact 45 Watt, 2-Meter Mobile! 

Now ICOM offers the best choices in compact 2-meter FM mobiles...the IC-27H 45 -watt compact $\left(15 / 6^{\prime \prime} \mathrm{H} \times 512^{\prime \prime} \mathrm{W} \times 9 \% /^{\prime \prime} \mathrm{D}\right)$ and the IC-27A 25 -watt super compact mobile. The IC-27A and IC-27H are the smallest fullfeatured 2 -meter mobile transceivers available, and feature an internal speaker for easy installation. For the ultimate portable station, the IC-37A 220MMz and IC-47A 440 MHz 25 watt compact mobiles are also available.


45 Watts. The IC-27H provides 45 watts of output power, while the IC-27A provides 25 watts of output power.


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See the IC-27A/H compact mobile transceivers at your loca ICOM dealer. For superb perform ance, reliability, and the ultimat in a VHF mobile radio, your only choice is an ICOM.


The IC-25A 2-meter 25 -watt mobile and its 45 -watt companion, the IC-25H. are also available.


## That To ook For In A hone Patch

te best way to decide lat patch is right for you to first decide what a tch should do. A patch ould:

Give complete control to the mobile, allowing full break in operation.

Not interfere with the normal operation of your base station. It should not require you to connect and disconnect cables (or flip switches!) every time you wish to use your radio as a normal base station.

Not depend on volume or squelch settings of your radio. It should work the same regardless of what you do with these controls.

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The patch should have standard features at no extra cost. These should include programmable toll restrict (dip switches), tone or rotary dialing. programmable patch and activity timers, and front panel indicators of channel and patch status.

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## How To Use SMART PATCH

Placing a call is simple. Send your access code from your mobile (example: ${ }^{*} 73$ ). This brings up the Patch and you will hear dial tone transmitted from your base station. Since SMART PATCH is checking about once per second to see if you want to dial, all you have to do is key your transmitter, then dial the phone number. You will now hear the phone ring and sor.eone answer. Since the enhanced control system of SMART PATCH is constantly checking to see if you wish to talk, you need to simply key your trans. mitter and then talk. That's right, you simply key your transmitter to interrupt the phone line. The base station automatically stops transmitting after you key your mic. SMART PATCH does not require any special tone equipment to control your base station. It samples very high frequency noise present at your receivers discriminator to determine if a mobile is present. No words or syllables are ever lost.

## SMART PATCH Is All You Need To Automatically Patch Your Base Station To Your Phone Line.

Use SMART PATCH for:

- Mobile (or remote base) to phone line via Simplex base. (see fig 1.)
- Mobile to Mobile via interconnected base stations for extended range. (see fig. 2.)
- Telephone line to mobile (or remote base).
- SMART PATCH uses SIMPLEX BASE STA. TION EQUIPMENT. Use your ordinary base station. SMART PATCH does this without interfering with the normal use of your radio.


## WARRANTY?

YES, 180 days of warranty protection. You simply can't go wrong.
An FCC type accepted coupler is available for SMART PATCH.

## TRM-201A/TM-401A

## TM-201A/TM-401A "comp-ACT" .. tough act to follow.

The word "compact" best describes the TM-201A VHF (a big 25 watts!) or the TM-401A $70-\mathrm{cm}$ (12 watts) mobiles. Measures $5.6 \mathrm{~W} \times 1.6 \mathrm{H} \times 7.2 \mathrm{D}$ inches (the TM-201A and -TM-401A are the most compact rigs available). Ideal in size,
their performances are superlative. Each features a HI/LO power switch, dual digital VFO's built-in, 5 memories plus a "COM" channel with lithium battery back-up, memory scan, programmable band scan, priority alert scan, and GaAs FET RF (front end) amplifiers. They have a highly visible yellow LED digital display, a repeater offset switch, a reverse switch.
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Other TM-201A/TM-401A Optional Accessories:
TU-3 Programmable twofrequency CTCSS encoder, KPS-7A fixed station power supply, MA-4000 dual-bander mobile antenna with duplexer, SW-100A/B SWR/power meter, MC-55 mobile microphone with time-out timer.


## Optional FC-10 Frequency

 ControllerConnects to the TM-201A or TM-401A. Convenient control keys for frequency UP/DOWN MHz shift, VFO A/B, and MR (memory recall or change memory channel). A green LCD display indicates transmit/ receive frequencies, memory channel number, ALERT, and SCAN (with blinking MHz decimal).

T1 W-4000A

## TW-4000A

## FM "Dual-Bander"

KENWOOD'S TW-4000A FM "Dual-Bander" provides new versatility in VHF and UHF operations, uniquely combining $2-\mathrm{m}$ and $70-\mathrm{cm}$ FM functions in one compact package. It covers the $2-\mathrm{m}$ band ( $142.000-$ 148.995 MHz ), including certain MARS and CAP frequencies. and the $70-\mathrm{cm}$ band ( 440.000 449.995 MHz ), all in a package
only 6-3/8 $\mathrm{W} \times 2-3 / 8 \mathrm{H} \times$ 8-9/16 D inches. RF output power measures 25 watts on either band. The TW-4000A features a large, easy-to-read LCD display, front panel illumination for night operations, 10 memories with OFFSET recall and lithium battery backup. programmable memory scan. band scan in selected $1-\mathrm{MHz}$ segments, priority watch function, common channel scan, dual digital VFO's, repeater reverse switch, GaAs FET front ends, rugged die-cast chassis.
"beeper" through speaker, a mobile mount, and a 16-key autopatch UP/DOWN mic.

The new optional VS-1 voice synthesizer has everyone talking! A voice announces the frequency, band, VFO A or B, repeater offset, and memory channel number when these functions are selected.

## Other TW-4000A

## optional accessories:

VS-1 voice synthesizer, TU-4C programmable two-frequency CTCSS encoder, KPS-7A fixed
station power supply, SP-40 compact mobile speaker, SP-50 compàct mobile speaker. MA-4000 dual-band mobile antenna with duplexor, MC-55 mobile microphone with timeout timer, and a SW-100B SWR/power meter.

More information on the TM-201A/TM-401A and TW-4000A is available from authorized dealers of Trio-Kenwood Communications 1111 West Walnut Street Compton, California 90220.
specifications and prices are subject to change without notice or obligation


## ham radio

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New Features: individually calibrated resistance scale, expanded capacitance range ( t 150 pf ). Built-in range extender for measurements beyond scale readings, $1-100 \mathrm{MHz}$. Comprehensive ${ }^{-}$ manual. Use 9 V battery. $2 \times 4 \times 4$ in.

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Turn your synthesized scanning $\$ 39.95$
2 meter handheld into a hot Police/ $5=\mathrm{MFJ}$ Fire/Weather band scanner! $144-148 \mathrm{MHz}$ handhelds receive Police/Fire on 154 158 MHz with direct frequency readout. Hear NOAA maritime coastal plus more on $160-164 \mathrm{MHz}$. Converter mounts between handheld and rubber ducky. Feedthru allows simultaneous scanning of both 2 meters and Police/Fire bands. No
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Low cost
MFJ-812 \$29.95
VHF SWR/ Wattmeter! Read SWR (14 to 170 MHz ) and forward/ reflected power
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## 1 KW DUMMY LOAD <br> Tune up fast, extend life of finals, reduce QRM! Rated 1 KW CW or 2KW PEP for 10 min utes. Half rating for 20 minutes, continusus at 200 W CW, 400 W PEP VSWR under 1.2 to 30 $\mathrm{MHz}, 1.5$ to 300 MHz . Oil contains no PCB. <br>  50 ohm non-inductive resistor. Safety vent Carrying handle. $71 / 2 \times 63 / 4$ in.

## 24/12 HOUR CLOCK/ID TIMER

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## Switch to 24 <br> hour UTC or

## 12 hour format!

Battery backup
maintains time during power outage. ID timer alerts every 9 minutes after reset. Red LED .6 inch digits. Synchronizable with WWV. Alarm with snooze function. Minute set, hour set switches. Time set switch prevents mis-setting. Power out, alarm on indicators. Gray and black cabinet. $5 \times 2 \times$ 3 inches. $110 \mathrm{VAC}, 60 \mathrm{~Hz}$.

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a) Mostercord

# de W9JUV 

A FROPOSAL TO REALLOCATE 220 MHZ AMATEUR FREQUENCIES TO LAND MOBILE was made in late July by Sideband Technology, Inc., a manufacturer of Amplitude Compandored Sideband (ACSB) equipment. In its Petition for Rule Making, RM-4831, Sideband Technology proposes that the bottom two megacycles of the $220-225 \mathrm{MHz}$ Amateur band plus the adjacent $216-220 \mathrm{MHz}$ Inland Waterways Communications Service band be allocated to ACSB Land Mobile users.

Opposition To The Growing Pressure On 220 has Developed Rapidly, highlighted by a teleconferencing net August 2 that carried the story throughout the country via many VHF and UHF repeaters, plus a few SSB relays to the HF bands. The net, hastily organized and led by 220 Notes publisher K9XI, did an excellent job of reviewing the growing 220 problem and what could be done about it. It was particularly valuable in alerting Amateurs to file Comments on both this petition and the earlier one by the Land Mobile Communications Council (see September Presstop). Comments closed on the LMCC petition in August, but a legal question has delayed the closing date on RM-4831 indefinitely.

A Reallocation of This Importance Is Highly Unlikely without going through a formal Notice of Proposed Rule Making procedure, but rumors of high-1evel FCC support for the change have been circulating. (See this month's Reflections for more on the 220 issue)

AN ELECTION OF UNIONIZING ARRL EMPLOYEES WAS HELD August 23 in Newington, and the union effort lost by a very large margin. Staff dissatisfaction over ARRL's return to the fiveday work week and other work-related matters had triggered the effort to set up a collective bargaining agent at League headquarters, but a very strong, well-organized opposition effort by management defeated the attempt. However, the problems that caused the unionizing effort have still not been resolved. That, coupled with the deterioration in relations between staff and management-and within those groups as well-that developed during the unionizing efforts of the past few months make it likely that morale will continue to be a problem in Vewington for some time to come.

420-450 MHZ USERS IN GEORGIA AND TEXAS FACE POWER RESTRICTIONS following the addition of two new "Military Protected Zones." After September 12, Amateurs within a 124 mile radius of Warner Robbins AFB in Georgia or Goodfellow AFB in Texas who plan to run more than 50 watts ERP will be required to coordinate their operations on the 70 cm band with both the nearest FCC Engineer-In-Charge and the military Area Frequency Coordinator

OSCAR 10'S OPERATING SCHEDULE HAS BEEN CHANGED, due primarily to the onset of an eclipse period which deprives the spacecraft solar panels of sunlight for up to $1 / 2$ hours at a time. The 145.810 General Beacon schedule has also been changed; bulletins now start on the hour and half hour with five minutes of CW, followed by 10 minutes of PSK telemetry, then RTTY bulletins ( 50 baud) for another five minutes. PSK telemetry occupies the final 10 minutes of each half-hour sequence. For schedule updates check the AMSAT nets

The 75 -Meter AMSAT Net Frequencies Have Been Changed to permit General licensees to take part in the Tuesday night nets following the September 1 phone band expansion. At first the $0100 Z$ (Wednesday, GMT) nets moved to 3855 kHz , but problems with an existing operation on that frequency caused a further move. Look for them around $3856-3860 \mathrm{kHz}$

ACSB Experiments Through OSCAR 10 began August 24 in a cooperative AMSAT,
ARRL, and Project OSCAR effort. Expected benefits include improved signal-to-noise ratios (narrower bandwidth) and easier tuning since ACSB receivers lock onto a pilot carrier and thus automatically track doppler shift. ACSB can be received with a normal SSB receiver, despite the 3.1 kHz pilot carrier. Sideband Technology is supplying the ACSB equipment.

AMATEUR ACCESS TO THE NEW 24 MHZ WARC BAND MAY NOT BE TOO FAR OFF. There had even been some thought that the FCC would begin 24 MHz implementation before the Commissioners went on August recess, as there seems to be no problem with current band occupants. On the other hand, the 18 MHz band still supports considerable commercial activity so is not likely to be reallocated very soon.

902-928 MHz's Availability Is Also Likely in the near future, and the ARRL VHF-UHF Advisory Committee has a band plan worked up for i.t. However, before either 18 or 902 MHz becomes available specifics such as modes and subbands must be established through an NPRM.

COMBINING METEOR SCATTER WITH PACKET RADIO could prove a viable mode for Amateur communicat ions, suggests ARRL's QEX. WØR PK is on 50.505 MHz from central Iowa, and KlHTV planned some 145.05 MHz tests during the August Perseids shower. WlaW may also gear up for both 10 and 6 meter meteor scatter packet radio experiments in the near future.

ARRL IS SUPPLYING ANSWERS TO ALL AMATEUR EXAM QUESTIONS in an attempt to establish uniform exams throughout the country. They distributed EIement 3 (Tech/General) questions complete with distractors to other VECs and Amateur Radio publishers in August, and expect to have the Advanced and Extra sets out soon. Whether those VECs who've already invested considerable time and effort in working up their own answer/distractor sets will be willing to change at this time remains to be seen, however.

# the endangered spectrum: 220 MHz under fire 

## I. Who's on 220?

The 1-1/4 meter Amateur band - covering $\mathbf{2 2 0 - 2 2 5} \mathrm{MHz}$ - is in imminent danger of being lost to commerical interests.
So what? Who operates there anyway?
This is the substance of the argument presented by Sideband Technology, Incorporated, in its petition to the FCC (RM-4831). STI, who manufactures amplitude compandored sideband (ACSB) equipment for the land mobile industry, is suggesting that because hams hardly use $220-222 \mathrm{MHz}$, that segment of the band should be reserved for land mobile purposes instead. A second group, the Land Mobile Communications Council (LMCC) has also petitioned the FCC (in RM-4829), suggesting that the entire band should be exclusively reserved for land mobile use.
"T'aint so!" For all practical purposes, the band is divided into two parts. $220-222 \mathrm{MHz}$ is used by Radio Amateurs doing pioneering radio work (EME, propagation beacons, weak-signal communications, packet radio, and experimental and control links, etc. $222-225 \mathrm{MHz}$ is used for $F M$ repeater and general CW/SSB operation.
Just how did the commercial interests get the impression that the lower portion of the band - where the bulk of Amateur experimentation is being carried out - was unoccupied? They conducted an exhaustive study by consulting a repeater directory.
What can you do?

1. Take this threat SERIOUSLY.
2. Read the additional information provided by W9JUV and W1JR on these pages.
3. Weigh the facts - check to see what activity exists in your area - and then . . . be ready to respond rapidly in writing to the FCC if it gets to the NPRM (Notice of Prooosed Rule Making) stage. *
Though the formal comment period for one of the petitions ended as this issue was going to press August 29 , we believe the FCC would still find your comments valuable. If you do respond, be sure to indicate that you wish them to accept this as a late comment, and that your comment is in opposition to a specific petition (either RM-4829 or RM-4831). State your name, call sign, class of license, and the year you were first licensed. Provide as much information about 220 MHz activity in your area - repeaters, control links, weak-signal work, etc. - as possible. Type (double-space) and stick to the facts.

You will have an opportunity to file a formal comment when and if an NPRM on the reallocation of the $220-\mathrm{MHz}$ band is issued by the FCC. If this occurs, a well documented, logical argument will carry the greatest weight.
Ham radio will keep you informed of late-breaking events, as will other news services; follow Westlink Report (via mail or repeater), the W5YI Report, ARRL letter, and ARRL bulletins. Do your homework, be prepared, and respond formally at the appropriate time.

Rich Rosen, K2RR Editor-in-Chief

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## II. How We Got There - A Brief History

The 1-1/4 meter band has survived a number of changes since its establishment just before World War II. Before the war, everything above 110 MHz was designated "Amateur and experimental." During the war, the spectrum from about 200 MHz up was used for the primitive radars of that period, radio altimeters, and radio navigation aids. Shortly afterwards, the U.S. phased out most of its use of the frequencies just above 220 MHz ; Amateurs were temporarily allocated a band at 235 to 240 MHz and then moved to 220 to 225 MHz in the late 1940's. In much of the world, however, military use of the band continued, and Amateurs outside of the Americas never did get a post-war 1-1/4 meter band.
Because the U.S. wanted to keep 220 to 225 - adjacent to its 225 to 400 MHz military aircraft frequencies - available for expansion, it permitted Amateur use of the band on a secondary basis. This became the standard for ITU Region 2, while the rest of the worid continued to use the band for radiolocation and/or land mobile. During the 1960's and 1970's other services cast frequency-hungry eyes on 220 to 225 MHz , but were discouraged by the government's continued intention to hold on to the band, with Amateurs acting in a "caretaker" role.
WARC 79 wrought a change with far-reaching implications for Region 2 Amateurs. The U.S. government relinquished interest in the band, and the Conference reallocated these frequencies to Amateurs and fixed mobile services on a co-equal basis. Thus the die was cast.
In an FCC study conducted several years ago, 220 to 225 MHz was mentioned in passing as a possible source of land mobile frequencies. This past June, the band was again cited by the LMCC in a frequency survey submitted to the Commission. However, the first direct attack on continued Amateur use of the band came in July when S.T.I. filed its petition.
To the horror of both FM equipment manufacturers and FM land mobile users, the FCC has proposed putting ACSB channels between existing land mobile FM channels. Indeed, some 150 MHz equipment has been licensed by the FCC on a temporary basis and is already in operation; ACSB promoters, however, would prefer to see it occupy a place where it could be exercised without interference to or from other communications modes. 220 to 225 MHz seems to be the answer to their prayers.
Can this threat be stopped before it reaches the status of a Notice of Proposed Rule Making? Perhaps not. By rejecting the "no-code" license, we lost our chance to ensure that 220 to 225 MHz would be "off limits for commercial encroachment for years to come; most of the no-code supporters had recommended that at least part of the 220 to 225 MHz range be allocated to no-code license holders. A few voices in the wilderness even pointed out the value of new licensees to frequency preservation of that band. Had no-code been adopted, it is inconceivable that the Commission would have turned its back on the new class of Amateur license it had just created by giving that class's prime frequencies to another service. With that opportunity gone, the industry's conception of the 220 to 225 MHz frequency range is that it is under-utilized, with significant activity only in major urban areas and then on only a few repeater pairs. "Use it or lose it" has never been more true than it is today.

- Joe Schroeder, W9JUV


# two petitions before the FCC <br> threaten yet another Amateur band 

## III. Why Amateur Radio Needs $220 \mathbf{M H z}$

Despite the lack of commercially available equipment and worldwide participation, 220 has seen continued growth over the years. This growth has taken two directions - weak signal operation in the lower segment and FM operation in the upper portions of the band. The latter is understandable in terms of severe crowding in the 2 meter and $70 \mathrm{~cm}(440-450 \mathrm{MHz})$ bands - and because foliage attenuation decreases the lower you go in frequency, $135 \mathrm{~cm}(220 \mathrm{MHz})$ is preferred to 70 cm in suburban areas.
The 220 band plan written by the ARRL VUAC (VHF/UHF Advisory Committee) in 1978 (table 1) designated 222-225 MHz for the use of FM repeaters. This has been widely accepted. $220-222 \mathrm{MHz}$ was divided up into two portions: weak-signal on 220-220.5 and FM repeater links, remote bases and control links on 220.5-222 MHz. Information on the latter stations is rarely published in order to prevent unauthorized control of the repeaters. (If STI and the LMCC had done their homework, they would have been aware of this. - Ed.)
The lower portion has been extensively used by weak-signal operators for the exploration of new propagation modes. Despite the band's claimed similarities to 2 meters, there are important differences between the two. For example, in meteor burst communication cutoff frequency is often just below or slightly above the 220 band. (It wasn't until 1968 that a 220 meteor scatter QSO was completed.) To this day, weak-signal operators are experimenting to find the cutoff frequency for the slower speed meteor showers. Further research is essential. For EME communication, 220 is a practical frequency because the antenna size required and the sky noise present is just about 50 percent of that at 2 meters. Auroral propagation, seldom seen at the higher frequencies such as 70 cm , is often possible.*
It was the 220 band that accounted for the 2500 -mile DX contact between California (W6NLZ) and Hawaii (KH6UK) in the late 1950's via a tropo-ducting mode. More recently, in 1983, the trans-equatorial path was finally conquered when KP4EOR worked LU7DJZ over a 3670 mile ( 5906 km ) path. Still to be explored are the FAI (Field Aligned Irregularities) and mid-latitude sporadic-E modes, which while theoretically possible have not yet been successfully used to establish two-way contact. This unique frequency range should be left intact for Radio Amateurs to further the state-of-the-art in radio wave propagation.
(Why wasn't all this activity obvious to those conducting a study on band occupancy? Perhaps the survey was performed during the regular work-week, while weak signal operators were busy working at their regular jobs, and not on the air. Also, weak-signal operators employ highly directional antennas, and would not be detected unless those conducting the survey were directly between the sending and receiving antennas.)
Nationwide activity on this band is apparent by the achievement of the WAS ( 50 states) award last year by a number of Amateurs. It's also easy to check the number of entries in the various VHF/UHF contests, 220 standings of active stations listed in QST's "The Worid Above 50 MHz " or correspondence in the dedicated newsletter: 220 Notes. That weak-signal interest and activity exists is obvious, even though it may be most evident during special propagation openings, contests, and net nights. Haphazard monitoring of the band results in inaccurate
data. To obtain a valid indication of 220 activity, monitoring would have to be done nationwide, and over a longer period of time; one would assume the land-mobile industry would have done so before making rash (and incorrect) statements claiming that the lower portion of the 220 band is not well used.
Only a year ago Amateurs received FCC permission to experiment with Packet Radio on the VHF FM bands. The overcrowding of 2 meters and the requirements for additional bandwidth to support 9600 baud and higher data rates make 220 a natural. (Part 97 of the FCC regulations prohibits high baud rates below 220.5 MHz . - Ed.) In the New England area, several stations using Packet Radio in the 221-222 MHz region have just become active.
This frequency range is not without problems. Amateurs in the vicinity of TV channel 13 experience video beats across the weak-signal portion of the 220 band. This is further complicated by radiation from TV set local oscillators, which often radiate into the lower portion of the 220 band when tuned to TV channel 7. No fixed commercial service would care to operate in the vicinity of these interfering sources. (Amateurs, on the other hand, are frequency-agile and can attempt to minimize these effects. In addition, radiation from the second harmonic of the local oscillator of the ubiquitous frequency scanners can fall within the 220 band, affecting any and all services. - Ed.)
Where can the land-mobile interests go? Considering how outdated the present FCC allocation of TV channels is, a better idea might be to go entirely to the UHF spectrum and make the VHF spectrum (land mobile allocated frequencies) available for point-to-point and mobile-to-base station use. The FCC could probably allocate more spectrum by taking advantage of the unused TV channels in the UHF spectrum, eliminating all channels below channel 25 . (The LMCC petition, in fact,
(continued on page 119)

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## $2 w^{2}$

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FSK Output - Open Collector +40 VDC Max. Polarity can be reversed.
Scope Output - 10 K ohm output impedance.

PTT Output - Open Collector +40 VDC Max.
Computer Connection - TTL Compatible. Inputs also RS232 level compatible.
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## a six-output power supply

## Build a low-cost lab-quality voltage source

This power supply construction project will provide a valuable addition to the workbench of most Amateurs. The unit includes three positive and three corresponding negative outputs consisting of a dualtracking pair, a positive and negative independently adjustable pair, and a positive and negative programmable voltage standard pair. A detailed set of drawings for construction is provided. The total cost of completing the project is surprisingly low, mainly because the unit is built around nine op amps that cost approximately fifty cents each.

## independently adjustable supply

Any voltage regulator or voltage regulated power supply must have five parts: a voltage reference, an
error amplifier, a feedback mechanism, a series-pass transistor or means of current-buffering and, usually, an optional current-limiting or self-protection circuit. This power supply includes all five of these elements. In circuit B (CKTB) of fig. 1, diode D5,* a 1N754 6.8 -volt zener, provides a 6.8 -volt input to the noninverting $(+)$ input of op amp $\cup 1$. The $(-)$ or inverting input will consequently also have +6.8 volts on it through normal op amp action (feedback). The voltage reference provided by op amp U 1 is impressed across pot R6, a 10 K pot. This variable voltage of from 0 to +6.8 volts is again applied to the noninverting ( + ) input of op amp U2, a 741 or LM101 type bipolar amplifier. Gain is determined by:

$$
E_{\text {out }}=E_{\text {in }} \frac{(R 10+R 11)+R 12}{R 12}
$$

$E_{\text {in }}=6.8$ volt reference voltage and is derived by pot R6 from 0 to 6.8 volts.

If you work through the numbers, you will derive an output of from approximately 0 to 16.5 volts with output adjust trimmer pot, R11, set halfway at 2500 ohms.

The op amps themselves have internal current

[^2]By Vaughn D. Martin, 114 Lost Meadows, Cibolo, Texas 78108, and Dean Davis, WB5ZKU, 6206 Ridge Oak, San Antonio, Texas 78250


fig. 2. Front panel controls and indicators.

fig. 3. A typical application of a precision Weston electrochemical voltage standard cell.
limiting, and with the output series-pass transistors Q1 and O 2 , providing the needed current drive, all five previously listed requirements of a voltage regulator are satisfied.

## negative independently adjustable supply

The complementary negative portion of circuit $B$ (CKTB) is composed of op amps U3 and U4 and associated circuitry. The reference voltage from the 6.8 volt zener diode D5 provides the input to an inverting amplifier (U3) with a gain of 1 . The ratio of the input resistor (R13) divided by the feedback resistor (R14) establishes the gain, and since they are equal, the gain is 1 . Therefore, amplifier U3 has a -6.8 volt output, which like its positive counterpart, is applied to front panel control pot R15 ( - supply); refer to fig. 2. This negative input voltage is fed to the noninverting amplifier, U4, and amplified for a gain of from zero to approximately 2.5 as a result of the feedback resistor ratio from R19 to R20. The transistors Q3 and Q4 provide current buffering only - no voltage gain.

## dual tracking power supply

This circuit, CKTC, is a composite and slight variation of previously developed and discussed circuits.

Amplifier U5 has a +6.8 volt voltage reference in the form of zener diode D6 applied to the noninverting ( + ) input pin 3. This voltage is applied across front panel control pot $\left( \pm \mathrm{V}_{\mathrm{T}}\right)$ R24. This 0 to +6.8 volts is then applied to noninverting amplifier U6, as described above. Amplifier U7 and transistors Q7 and Q8 form a negative regulator that is slaved to and therefore "tracks" the positive portion of this circuit, but naturally has an output equal in magnitude but opposite in polarity.

## programmable power supplies

These two positive and negative power supplies are precision voltage sources and do not deliver power. They can deliver only approximately 4 mA of current, the capacity of an op amp itself. They are used primarily as precision stable voltage sources. Those readers old enough to remember the Weston cell that characterized most instrument labs some 20 years ago or more will recall that these were electrochemical voltage standards intended for use with very high resistance pots. They were typically employed with

fig. 4. Mounting and functions of a multi-turn pot and matching turns counting dial.

fig. 5. Rear view of case shows easy access to PC board trimmers.
galvanometers in "balancing schemes" to indirectly determine to several significant figures the accuracy of an unknown voltage source (see fig. 3). Today we have $61 / 2$-digit DVMs that will do this with equal or better accuracy and with much more convenience than that cumbersome hookup configuration. The Weston standard cells nonetheless developed an opencircuit voltage of 1.0183 volts as a result of the precise predictable nature of the electrochemical reactions within. But they could never be used to operate even a small lamp or similar low current demand device because irreparable damage would result, and their accuracy and repeatability could never again be trusted. However, these two precision low current circuits, using LM101 op amps, are nearly short-circuit proof.

The positive and negative programmable power supplies are simple (see fig. 1, CKTA). Both use complementary pair transistors to form an accurate current source that can provide 1 mA of current. This current, run through a 25 -kilohm pot, generates a +25 volt fullscale output (positive power supply).

The pot, R51, is a 10 -turn pot with a 10 -revolution turns counting dial, (see fig. 4). For each revolution, up to and including the tenth turn, the pot will have 2.5 kilohms of resistance. Therefore, if you were to turn the pot to 4 , you would have 4 turns at 2.5 kilohms each for 10 kilohms of resistance with 1 mA of current flowing through it for 10 volts DC of positive very precise voltage generated. You will note that this very precise positive voltage source goes to the input of U9 which is an op amp used as a voltage follower. More specifically, it is just an amplifier with a gain of +1 with a bit of current buffering. The noninverting input denoted by a $(+)$ sign on U9 has an input impedance of at least 10 megohms, so very little, if any, voltage division occurs at this point.

The negative programmable power supply is the mirror image of its positive complementary counterpart. The +12 volt zener establishes bias on the bases of a complementary pair of transistors, Q 9 and Q 10 ,

fig. 6. Six-output power supply.

fig. 7. Interior view of power supply.
which produce a constant 1 mA current. This current is adjusted by a multi-turn PC mountable pot placed at the rear of the PC board (see fig. 5). Adjust R43 until four turns of the pot (10K) produce exactly 10 volts. A DVM can be used to check this. Make sure you do not load down this output. Op amp U8, like all nine op amps used with this project, is an LM101. If you have the TO-100 version, use it; its pin configurations is identical (pin 8 is the pin underneath the tab).

## construction

The Bud box selected and specified in the parts list is ideal for this application in terms of cost and shape. The top of the enclosure slides down over the metal frame in a clamshell fashion. Fig. 6 illustrates the finished product with the top in place. Fig. 7 shows the project with the lid removed.

The actual detailed dimension of the box and the holes are provided in fig. 8. It should be noted that the two holes holding the shafts of the multi-turn pots can be either $1 / 8$ or $1 / 4$ inch, depending on the pot shaft diameter and corresponding turns counting dial

fig. 8. Drawing illustrates case drilling pattern.


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IC-PS30 base station supply. IC-PS 15, and the internal IC-PS35.


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Also available to complete your VHF/UHF base station, are its 2-meter companions, the 100 -watt IC-271H and 25 -watt IC-271A.

See the IC-471H and other ICOM equipment at your local authorized ICOM dealer.

selected. Also, the cutout in the back, made with a Greenlee 5/8-inch square punch accommodates a rather fancy fuseholder. You may have greater luck finding a round standard MIL-M-14 type CFG fuseholder with a 0.440 -inch diameter round hole. The 1:1 scale foil pattern are shown in fig. 9. Note that the side with far fewer runs (lands) is the component side. Kits are available (see fig. 10) for lifting a pattern directly from a magazine page such as this one. The drill diameter schedule shown in fig. 11 is a must for this method; even if you purchase the pre-drilled board, you will nonetheless still need this drawing as a component placement guide.
When mounting the parts on the PC board, be sure to observe the polarity of all the diodes and polarized electrolytic capacitors. Also, be sure to note that the op amps have pin 1 indicated by a dimple adjacent to the notch. The PC board has a small dot above pin 1 on the foil side of the board. Failure to observe these guidelines will result in destruction of the op amps. The smaller TO-100 type of transistors that do not go on the rear panel in the heatsinks can be properly oriented onto the PC board by a "tick" mark denoting where the alignment of the case's tab should be. Diode symbols are on the board; there are also ( + ) signs for proper placement of electrolytics.
The meter circuit is optional because only one supply at a time can be used when the current meter is in use.

## turns-counting dials

Refer to fig. $\mathbf{4}$ when placing the turns counting dial and multi-turn pot on the front panel. Select a dial that matches the pot's shaft diameter; the two most common shaft diameters are $1 / 4$ and $1 / 8$ inch. The turns counting dial that matches it will probably have its inner scale marked in gradients of hundredths of a turn. The outer scale counts the number of turns (usually up to 15) completed.
To mount the pots and dials, refer to fig. 4 again and follow the procedure described below, prepared originally for the Helipot ${ }^{\text {TM }}$ Duodial ${ }^{\text {TM }}$ series of pots and multiple turns counting dials:*

- Locate positions for holes " $A$ " and " $B$ " on panel. " $B$ " for lug on locating washer is $9 / 32$ inch below center of hole " $A$ ".
- Drill $9 / 32$ inch hole " $A$ " in panel for pot bushing.
- Drill $5 / 64$ inch hole " $B$ " in panel for lug on locating washer.
- Turn potentiometer shaft against its counterclockwise stop. Insert shaft into center hole " $A$ " in panel.

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fig. 9. Double-sided PC board artwork.


- Slip locating washer over shaft and seat lug on locating washer in hole " $B$ ".
- With a wrench, firmly tighten mounting nut onto potentiometer bushing. Note that the nut supplied is reversible. For thick panels, use as shown in drawing. For thin panels, reverse the nut. If the Duodial is used with a device other than a Helipot potentiometer, an appropriate mounting nut may have to be obtained. This must fit within the $3 / 8$-inch diameter $13 / 64$-inch deep recess in model 2601 DUODIAL.
- With locking lever in OFF (UP) position, slip dial assembly over potentiometer shaft. Be sure lug at top of locating washer seats in slot in back of dial, and that the whole dial assembly sets lightly against the panel.
- Turn dial knob counter-clockwise until the zero of the outer scale is in the center of the window. Now turn slowly until the scale reads between 10 and 20 at the index line. Tighten the set screw until a very slight drag on the shaft is felt. Turn knob very slowly until both zeros line up with the index line. Tighten the set screw firmly.


## parts - and where to get them

Components. This design purposely uses components that are easy to obtain. Several suggested sources are listed at the end of this article.

fig. 10. Typical kits available today to nonphotographically "lift" a PC board from magazine pages.

Zener diodes. Four are used in the input power conditioning circuit off the transformer. The two 20 -volt zeners are 1 N4747As, available from Digi-Key. The 40 -volt zeners must be obtained elsewhere. However, two 20 -volt zeners may be connected in series to achieve the same result. The other six low-power zener diodes consist of: two 2.7 -volt zeners, two 6.8 -volt zeners, and two 12 -volt zeners. If the 2.7 -volt zeners are hard to find, 1 N5226B 3.3 -volt zeners may be used in their place. If this substitution produces more than a 1 mA output from the constant current sources, then trim pots R43 and R50 can be adjusted accordingly for a 1 mA output. The two 12 -volt zeners can

fig. 11. A combination drill pattern/component placement drawing.
be 1 N963, 1 N 5242 B , or 1 N 4742 As . The 6.8 -volt zeners establishing reference input voltages, namely D5 and D6, can be either 1 N957B, 1 N5235B, or 1 N4736As.

Rectifier diodes. The rectifier diodes are 1 N 4001 s . You may also use any of the 1 N 4000 series up to and including 1N4007, 1000 PIV diodes.

Capacitors. All capacitors that are polarized aluminum electrolytics are radial rather than axial lead devices, which are designed to lie flat on the PC board.

Meters. Edgewise meters have been selected to minimize the amount of front panel space required and to avoid a cluttered look.

- Trim pots. All five cermet trimming pots are $3 / 4$-inch rectangular ones with three staggered pins coming out their underside. All five are available from Digi-Key for $\$ 1.20$ each. The three 5 K pots are part No. 01B53 and the two 1 K pots are No. 01B13.
Op amps. It is the nine LM101 or 107-type bipolar operational amplifiers that give this project its appeal in the form of some exceptional performance parameters.

National Semiconductor, the leader in op amp and linear IC manufacturing, has adopted a parts numbering convention now almost universally accepted throughout the industry, with variations occurring only in prefixes to denote the different styles of case available. " $L$ " in the prefix "LM" stands for "linear," the " M " stands for "monolithic," (as opposed to " H ", which stands for "hybrid"). The first digit - a 1, 2, or 3 - signifies whether the part is military, industrial, or commercial grade. A " 3 ", or commercial grade product, is sufficient for this project and is less expensive than a grade 1 or 2 part.

Transformer. The Triad F-91X specified will adequately power this project and its $\pm 100 \mathrm{~mA}$ outputs. However, if 2 amp outputs are required, you must increase the transformer's capacity along with the output power transistors' drive capability into 12 amp Darlington or single-cased direct-coupled transistor pairs. The two NPN transistors, which are now 2N3766's must then be 2N6057's or equivalents. The two PNP transistors, which are now 2N3740's, must then be 2N6050's or PNP Darlington pairs. Housed in TO-3 cases, both require heatsinking. Detailed thermal design information is available in references 1 and 2.

## references

1. Vaughn D. Martin, "Cooling Semiconductors: Part One," ham radio, July, 1984, page 33.
2. Vaughn D. Martin, "Cooling Semiconductors: Part Two,": ham radio, August, 1984, page 52.

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# Leyden's magic jar: the derivation of the Hertzian and Marconi antennas 

# From "electrical fire" to today's "rubber duckie" 

In 1745, Ewald Jurgen von Kleist literally held in his hand the ancestor of most radio antennas in use today. Von Kleist was not a radio engineer; radio wasn't even discovered until 43 years later. Dean of the Cathedral of Kamin in Pomerania, Kleist enjoyed investigating the strange phenomenon of "electrical fire" in his spare time. Realize, now, that this was long before there was an electric light bulb, electro-magnet, or even a battery with which to power them. Von Kleist was not seeking to discover anything about antennas - he'd never even heard of them. He was just enjoying himself, as many experimenters do, by playing with

fig. 1. (A) An example of a capacitor such as von Kleist discovered; (B) A Leyden jar loccasionally called a "Kleistian jar).
and studying electricity. In doing so, he unwittingly discovered the world's first electrical "condenser" or capacitor. And believe it or not, this discovery led to antennas as we know them today.

As you know, a capacitor consists of two conductors called "plates" which are separated by an insulator called a "dielectric." Such a device can accept and store an electrical charge. First Kleist filled a glass flask with water. Then, holding the flask in one hand, he inserted a wire into the water in the flask and charged the wire with sparks of static electricity. As shown in fig. 1A, the water in the flask formed the inside plate of the world's first capacitor. The glass of the flask formed the dielectric, and von Kleist's hand served as the other plate of the capacitor! Touching the wire, von Kleist literally got the "shock of his life." He told others who played with electricity about his "shocking" discovery; one of them, a man named Graylath, succeeded in replicating the effect. According to Heilbron, ${ }^{1}$ Graylath reported that his device for storing "electrical fire" could knock children of 8 or 9 "off their feet. ${ }^{" 1}$ Such was the remarkable beginning of what we commonly refer to as the "Leyden jar." The term "Leyden" derives from the town of Leyden in the Netherlands, where in 1746, Pieter van Musschenbroek and his student Cuneaus further developed the early capacitor while trying to replicate and improve upon von Kleist's work. Obviously, one could not continue to use one's own hand as one plate of this potentially dangerous device. In the Leyden jar, the experimenter's hand on the outside of the flask was replaced with a coating of metal foil. The water on the inside of the flask - the inner plate of the capacitor - was

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replaced by a second piece of foil. These two foil plates were separated by the glass wall of the Leyden jar, just as the glass of the flask had separated the water and von Kleist's hand in the original device. Fig. 1B shows the Leyden jar invented by Musschenbroek.
As the early physicists continued to pursue the elusive electrical phenomena of the day, more discoveries were uncovered. Ruhmkorff developed the induction coil or transformer. Induction coils equipped with the battery, invented by Volta, were capable of producing very high voltages continuously and giving impressive sparks across gaps in conductors. It was also found that the induction coil would give a much more powerful spark at a spark-gap if a Leyden jar or two were connected across the gap. Another finding quite important to the discovery of radio was that the discharge of a Leyden jar across a spark-gap was actually an oscillating current rather than just one pulse of current as it appears to the eye. Then along came Heinrich Hertz, bringing these discoveries together to confirm Maxwell's predictions of the possibility of radiating electromagnetic waves through space. As part of the apparatus used in demonstrating this remarkable phenomenon, he employed an induction coil and spark-gap to create a transmitter similar to that of fig. 2.
Aitken has noted that the metal plates on the ends of Hertz's dipole antenna (fig. 2) were essentially Hertz's way of "unrolling" the foils of the Leyden jar and thereby increasing the capacitance across the spark-gap of his transmitter. ${ }^{2}$ Hertz, of course, knew that a Leyden jar discharging through a spark-gap produced an oscillating electric current. What he had to do was to somehow "open up" that circuit so that it could produce the suspected radiation of electromagnetic waves that Maxwell had predicted. In discussing the evolution from Leyden jar-plus-wire-loop oscillator to wire-plus-metal-plate antenna, Aitken says, "The two foil surfaces of the Leyden jar, opened outward and transformed, became Hertz's radiating dipole antenna. ${ }^{\prime \prime 2}$ Hertz at times dispensed with the foils, and used as his antenna only the rods to which the foils were attached. (In some instances he selected dipole lengths that put his electromagnetic radiations near the 2-meter Amateur band of today!! Thus did the Leyden jar evolve into the dipole or doublet antenna as we now know it.
Subsequently, Guglielmo Marconi, while vacationing in the Italian Alps, read an announcement of the death of Hertz. The same article recounted Hertz's astounding achievements in demonstrating the possibility of transmitting electromagnetic waves through space. Marconi was struck with the potential such a discovery might hold for the communication of information across more than just the few feet of laboratory space which Hertz had done. He cut short his vaca-

fig. 2. An example of a spark-gap transmitter with dipole antenna and capacitance plates.

fig. 3. A Marconi antenna connected to a spark-gap transmitter. The left side of the spark-gap is connected to the earth.
tion and returned home to begin work on what was to become the wireless telegraph, or what we now call radio. Marconi soon began experimenting with antenna placement and eventually came to connect one side of the spark-gap in his transmitter to a vertical antenna (see fig. 3) and the other side of the gap to the earth or ground.

Hertz had found that he had to make the length of his dipole equal to one-half the wavelength of the frequency which he desired to radiate. Marconi, on the other hand, found that with the earth substituting as half the dipole, he could use one-fourth of the wavelength as the length of his vertical radiator. With this configuration was born the grounded vertical antenna, ancestor to the common quarter-wave vertical ground-plane antenna as well as AM broadcast towers and many other vertical antennas. Although antennas didn't look much like a capacitor or a Leyden jar by Marconi's time, the idea of the antenna as a capacitor did not die with Hertz's opened-out Leyden jar. Early technical books on radio routinely discussed antennas as being large capacitors and explained their functioning in those terms. For instance, in a 1922 revision of the U.S. Army Signal Corps radio handbook, ${ }^{3}$ we find the following: "There are two general types of anten-

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nas, those which act primarily as electrical condensers and those which act primarily as electrical inductances. The first type is usually referred to simply as an 'antenna.' The second type is usually referred to as a 'coil antenna,' 'coil aerial,' 'loop,' or when used for a particular purpose, as a 'direction finder.' " Of course today we realize that an antenna has capacitance (as well as inductance and resistance), but are more likely to conceptualize an antenna as a resonant circuit than as a capacitor.

## terminology

Notice that in fig. 2, Hertz's antenna is oriented with its radiating conductor in the horizontal plane. Thus the electron flow on the radiator, and the electrical wave radiated into space, would naturally be horizontal. For this reason, Hertz's antenna is described as a horizontally polarized antenna. Terms still in use for common horizontally polarized antennas, in particular the $1 / 2 \lambda$ dipole or doublet, are "Hertz" or "Hertzian" antennas. On the other hand, in Marconi's $1 / 4 \lambda$ antenna, note the vertical orientation of the antenna's wire radiator. Here the current flow on the radiator, and the electrical wave radiated into space, are vertically oriented. It's not hard to see why, even today, vertically polarized antennas worked against a groundplane are sometimes referred to as Marconi antennas. For example, in the 1982 edition of the RSGB's HF Antennas, Moxon refers to " . . . the Marconi antenna . . . which can be regarded as one-half of a dipole, the other half being the image in the ground. "/4 Shrader, in Electronic Communication, ${ }^{5}$ wrote, "Any antenna complete in itself and capable of self-oscillation, such as a half or full wavelength, is known as a Hertz antenna. When an antenna utilizes the ground (earth) as part of its resonant circuit, it is a Marconi antenna." To me, it seems fitting that the two most common antenna configurations we have today still bear the names of their illustrious discoverers.
The next time you whip the ol' rubber duckie past your ear as you put your HT on the air, give a little thought to the debt we owe those old-timers for the pleasures we enjoy today. If the thought makes the hair on the back of your neck stand up a little, it might just be that the spirit of old von Kleist is back there with a charged flask, still playing with his "electrical fire."

## references

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## low-cost UHF antenna tower

## Chimney-mounted perforated tubing provides accessible 57-foot skyhook

This article describes a design for a UHF antenna tower that can be constructed very simply and at a price most hams should be able to afford - less than $\$ 200.00$. This type of tower is ideal for Amateur Fast Scan Television applications, among others.

Before the design was begun, several ground rules were established:

- The tower should be attached to the chimney of the house. (The advantage is obvious; the chimney would serve as the base for the tower and also provide extra height.)

fig. 1. Tower and antenna assembly measures 57.5 feet (17.5 meters) from ground.
- For aesthetic reasons, no guy wires were to be included. This meant that the tower had to be strong enough to withstand 80 -mile per hour ( 128 km per hour) winds with an antenna area of $2 \mathrm{ft}^{2}\left(0.19 \mathrm{~m}^{2}\right)$, which is sufficient for two or more UHF-type antennas.
- For ease of maintenance, the tower must be a tiltover.
- The tower sections had to be light enough to allow construction and assembly to be carried out without the need for a crane.


## the chimney must take the load

The first order of business was the necessity of establishing the strength factor of the chimney for a given side load. This is very important; not all chimneys are strong enough to support a mast. At this site, the chimney is constructed from an inner column of tube segments surrounded with a brick-cemented outer shell. The space between the brick shell and the tube segments is filled with concrete reinforced with four $1 / 2$-inch $(1.27-\mathrm{cm})$ steel rods. This is common practice in Southern California. A check with the county masonry society revealed that this type of chimney should be capable of sustaining a side load of 1000 pounds ( 454 kg ).

The next step requires calculating the strength specifications for the tower itself. Because no guy wires were planned to supporthe tower above the chimney, the combined strength of the tower, the rotator mounted on top, and the antennas above the rotator must be sufficient to sustain violent winds up to 80 miles per hour, or 128 km per hour. (A detailed analysis is included at the end of this article.)

The tower and antenna assembly consists of a set of chimney mounting brackets; three lengths of square tubing sections, each successively smaller in diameter and fitting inside the previous tube; a rotator; and a

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fig. 2. Right angle bolts connect tubing sections.

9 -foot ( 2.74 meters) long, 16 -gauge ( 2 mm ) galvanized steel $1-5 / 8$ inch ( $4.1-\mathrm{cm}$ ) I.D. tube with two DX-420 Cushcraft antennas mounted to it. The total height, measured to the tip of the antenna mounting tube is 57.5 feet ( 17.5 meters) above the ground. This includes the 23 -foot ( 7 -meter) high chimney. (See fig. 1 .

## construction details of tower and chimney mounts

The tower was assembled from three lengths of Telespar perforated tubing. This type of tubing was designed for sign posts, storage racks, and benches. Of the many unique properties of the tubing, its modularity makes it most useful for antenna mounting. Each segment of tubing was designed to fit into the next larger tube diameter. Right angle bolts provided by the supplier fasten the sections of tubes together. (See fig. 2). An overlap of 1-1/2 feet ( 46 cm ) should be maintained to allow for sufficient strength. Since cost and simplicity were of primary concern, no elaborate motor driven or other type of mechanism to lower or raise the tower was included. Access to the antennas was achieved by making it a tiltover assembly with a hinge.

The brackets are of an all-welded construction. A detailed drawing (fig. 3) outlines the construction features of the front bracket which supports the tower.
The rear bracket is almost the same as the front bracket, with the exception that no tower brackets are included. The author chose to make the bracket longer, reaching further down the chimney for added strength and to provide a better stress distribution in the chimney. Each chimney width will be different; thus the inside bracket dimension will be unique for each installation. The $4.5-\mathrm{foot}(137-\mathrm{cm})$ bracket height should be maintained in order to provide adequate base support. Remember, the tower, rotator, boom, and antennas weigh approximately 150 pounds ( 68 kg ). The front bracket weighs approximately 80 to 100 pounds ( 36 to 46 kg ) and the rear bracket approximately 70 to 90 pounds ( 32 to 41 kg ).

fig. 3. Construction details of front bracket assembly.

fig. 4. Hinge assembly, consisting of a front and rear bracket, is fastened with two 2-foot long threaded bolts.

After the brackets are completed, apply rust preventing paint and measure the width of the chimney accurately; the welded bracket assembly cannot be readjusted to fit the chimney. (A bolted construction may work loose or cause twisting in heavy winds.)
The sandwich mounting of the front and rear brackets, using $1 / 2$-inch $(12.7-\mathrm{mm})$ bolts, serves two purposes: first, it eliminates the need for drilling into masonry and mounting of lag bolts, which are unreliable in this application; second, it helps prevent the failure of masonry between the bricks. If the chimney is not straight you may have to insert shims between the brackets and the chimney for stability.

fig. 5. Remove upper mast bolt to lower tower to roof.

fig. 6. To reach antennas, simply remove bolts joining sections, sliding one section inside the other.

fig. A1. Tower/antenna configuration.

Designed to be part of a welded bracket straddled around the chimney, the hinge is fastened together with $1 / 2$-inch ( $12.7-\mathrm{mm}$ ) two-foot long threaded bolts available at most hardware stores. (See fig. 4.) Fig. 5 illustrates how the tower can be lowered to the roof by removing the upper mast bolt.

If you have a pitched roof, how do you reach the antennas after the mast is hinged down? The mast is 39.5-feet (12-meters) long, measured from the hinge point. It overhangs the rooftop by 27 feet ( 8.2 meters). Therefore, the design includes the sectional feature shown in fig. 6. Since three square tubes slide together, merely removing the two sets of bolts that hold the sections together allow shortening the mast
to the point where the antennas can be easily reached.
In terms of the rotator, antennas, and tubes supporting these antennas, each individual must consider the options available and choose the most appropriate configuration. The tower constructed by the author was tested involuntarily when seven major storms swept through the Los Angeles area with wind velocities up to 100 miles per hour ( 160 km ) during the winter of 1982-1983. The tower, brackets, and antenna sustained no damage; the tower is still perfectly vertical, and no stress cracks or other minor damage has been observed on the brackets or tower.

## acknowledgement

My sincere thanks to Bob Provost for providing the mechanical analysis for the tower design.

## appendix

## antenna tower stress analysis

The following is a stress analysis of an antenna tower attached to a chimney. This analysis may be used as a guideline for any tower configuration. The simplified approach assumes a cantilever beam with a projected antenna surface area of 2 feet $^{2}\left(0.19\right.$ meter $\left.^{2}\right)$. The object of the analysis is to determine the wind velocity a given tower/antenna configuration can endure without damage.

The configuration of the tower/antenna model is shown in fig. A1.

First, one needs to determine the moment of inertia ( $I_{S Q}$ ) of sections " $A$ " through " $F$," using equation:

$$
\begin{equation*}
I_{S Q}=1 / 12\left(O . D . .^{4}-I . D .{ }^{4}\right) \tag{A1}
\end{equation*}
$$

$$
I_{A}=I / 12\left[(2.50)^{4}-(2.29)^{4}\right]=0.9635 \text { in. }^{4}
$$

Next, the bending stress ( $\sigma$ ) as a function of wind force $(P)$ needs to be determined.

$$
\begin{equation*}
0=\frac{M C}{I} \tag{A2}
\end{equation*}
$$

where $M=$ moment (arm)
$C=$ distance to neutral axis of cross section
$I=$ moment of inertia
For section " $A$ " the bending stress is:

$$
\begin{aligned}
& \sigma_{A}=\frac{(32.5 \mathrm{ft})(P \mathrm{lb})[(\mathrm{I} / 2 \cdot 2.50 \mathrm{in})](12 \mathrm{in} / \mathrm{ft})}{0.9635 \mathrm{in}^{4}} \\
& \sigma_{A}=506.0(\mathrm{P}) \mathrm{lb} / \mathrm{in}^{2}
\end{aligned}
$$

The following table summarizes the results:

| section | CG <br> distance | tower <br> cross section <br> (inches) | wall thick <br> (inches) | I | PSI |
| :---: | :---: | :---: | :---: | :---: | :---: |
| F | - | - | - | - | - |
| E | 7.0 | $1.5 / 8 \times 1-5 / 8$ | $1 / 16$ | 0.1592 | 428.7 P |
| D | 8.5 | - | - | - | - |
| C | 17.0 | $2 \times 2$ | 0.105 | 0.4778 | 426.9 P |
| B | 25.5 | $2-1 / 4 \times 2.1 / 4$ | 0.105 | 0.6925 | 497.1 P |
| A | 32.5 | $2-1 / 2 \times 2-1 / 2$ | 0.105 | 0.9635 | 506.0 P |

*Extra strong section used, calculation not necessary
As can be seen from the table, Section $A$ experiences the largest stress for a given wind force (Section C, the least). (in other words, Section $A$ would be the first section to break.) The maximum wind force a section can withstand is based on the strength of the material. The yield strength of the tower material is o yield $=33 \mathrm{ksi}(33,000$ $\mathrm{lb} / \mathrm{in}^{2}$ ). Any bending stress less than 33 ksi applied to the cross section will not permanently deform the tower section.

The ultimate strength of the tower material is o ultimate $=52$ $\mathrm{klb} / \mathrm{in}^{2}$. Any bending stresses from 33 to $52 \mathrm{klb} / \mathrm{in}^{2}$ applied to the cross section may result in permanent deformation. Stresses above $52 \mathrm{klb} / \mathrm{in}^{2}$ will cause the tower section to break.

Solving for the unknown wind force yields:

$$
\begin{aligned}
506.0 P & =33 \mathrm{klb} / \mathrm{in}^{2} \\
P & =65.22 \mathrm{lbs}
\end{aligned}
$$

Wind force is related to wind velocity as follows:

$$
\begin{equation*}
P=\frac{A_{\varrho} V^{2}}{g} \tag{A3}
\end{equation*}
$$

where $A=$ antenna area
$\varrho=$ density of air $\left(0.076 \mathrm{lbm} / \mathrm{ft}^{3}\right.$ at $66^{\circ} \mathrm{F}$ )
$V=$ wind velocity
$g=$ gravitational acceleration
$P=\frac{\left(2 f t^{2}\right)\left(0.076\left(\mathrm{lbm} / f t^{3}\right)\left[(\mathrm{V} \text { miles } / \mathrm{hr}) \frac{\mathrm{l}}{\left.\frac{\mathrm{l}}{} \mathrm{hb00} \frac{\mathrm{hr}}{\mathrm{sec}}(5280 \mathrm{ft} / \mathrm{mile})\right]^{2}}\right.\right.}{32.186\left[f t / \mathrm{sec}^{2}(\mathrm{lbm} / \mathrm{lbf})\right]}$
$P=0.01016 V^{2}$ lbs or $V=\sqrt{\frac{P}{0.0 \overline{1016}}}$

Therefore, the maximum wind velocity cross section " $A$ " can withstand is:
$V_{y i e l d}=\sqrt{\frac{65.22}{0.01016}}=80 \mathrm{mph}$
and
$V_{\text {ultimate }}=\sqrt{\frac{103.64}{0.01016}}=101 \mathrm{mph}$
Although the simplified calculations show a $V_{\text {yield }}$ of 80 mph , winds up to and over 100 mph have not resulted in tower material yield at this location. It appears that using the equations outlined above should provide a conservative means of calculating the strength of a tower.
(The same analysis in metric units is available. Send an SASE . Editor.)

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## Johnu flarghall Harrle, WB5IIR

The Amateur Radio community was recently saddened to learn of the untimely death of John Haerle, WB5IIR, in an automobile accident August 1.

A popular author and lecturer active on 160 meters, John had been affiliated with Gates Radio as chief engineer for sales, and later with Collins Radio, where he served as director of advertising and public relations and also headed that organization's broadcast division.

Surviving are his wife, Rose; a son, Dan; and a granddaughter.

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| Less Case \$39 | $144-146$ | 28-30 |
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|  | 144-144.4 | $27-27.4$ |
|  | $146 \cdot 148$ | 28.30 |
|  | 144-148 | 50-54 |
|  | 220-222 | 28-30 |
|  | 220-224 | 144-148 |
|  | 222-226 | 144-148 |
|  | 220-224 | 50.54 |
|  | 222-224 | 28-30 |
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Sends short beep through your audio as any key is depressed.
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hh:mm:ss
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E. EDIT
M. MOVE
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X. SET XMT BUFFER SIZE
C. SET COLOR
T. SET TIME

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# design your own trap antenna 

## Operate wherever you want with this efficient antenna

Even though the trap antenna seems to be simple, designing one - on paper or by cut-and-try can be tedious. It's possible, however, to take the tedium out of the process by using a home computer or a programmable calculator. The antenna described in this article should perform acceptably on first use, and should be easy to adjust.

The basic concept underlying the trap vertical, dipole, or beam antenna is simple: the bottom (or half center) section is simply $1 / 4$ wavelength long at the highest frequency. A parallel-resonant trap tuned to this operating frequency effectively isolates the rest of the antenna. On the next lower band, the bottom section will be less than $1 / 4$ wavelength long (physical(y). This length is electrically extended by the loading coil effect of the below resonance trap (looks like an inductance), and the combination must be brought to 90 degrees effective (electrical) length by a second section of tubing. A trap resonant at this lower frequency can now be added if more bands are needed, or the antenna simply "stopped." Each additional band requires a trap, plus an extended metal section. At low

fig. 1. Organized approach to trap antenna design.
frequencies, a loading coil can also be added to reduce section length.

The challenge of trap antenna design lies in the fact that conversion from the physical length of sections to electrical length depends on the ratio of section diameter to wave length, so that the values must be recalculated for each band. Also, the trap-to-loading coil effect must be redone for each band, with conversion from reactance to effective length also considered. Unless an organized approach is used, it's easy to get lost.

For Amateur Radio purposes, the key to this organized approach is a series of articles by Boyer, W6UIH. The following summarizes the calculation steps involved and the equations used. (For explanations of the individual steps, refer to the Boyer series.)

INPUT the design parameters:
Number of bands
Operating frequencies, $f_{n}$, (highest first, in order)
Section diameters, $D_{n}$
Trap capacity or inductance, $C_{n}$ or $L_{n}$
CALCULATE for specified frequencies:
Trap inductance or capacitance, and reactance, $X_{n}$
Section characteristic impedance, $Z_{0}$
CALCULATE by looping:
Set first section length $h$ to 90 degrees
Loop for each band and for each trap
Calculate the wave length $=11808 / \mathrm{f}$ inches
Calculate the section impedance
$Z_{n}=60\left(L_{n} \cdot \lambda_{n} / D_{n}-1\right)$
Calculate the ratio of trap frequency to operating frequency $f_{n} / f_{n}^{\prime}=m$
Calculate effective section length $h^{\prime}=m h$
Calculate normalized trap reactance $X_{L}=X_{L}(1 / m$ $-m) / Z_{n}$
Add reactances $X^{\prime}=X_{L}+X$
Convert to length $h=\tan ^{-1} X^{\prime}$
Determine section length when all traps and sections have been considered.
$S=90^{\circ}-h$
By R.P. Haviland, W4MB, 1035 Green Acres Circle, N., Daytona Beach, Florida 32019

| $\begin{aligned} & 10 \\ & 20 \\ & 30 \end{aligned}$ | ```REM TRAP ANTENNA FAST FRINT "ENTER NLIMEER BANL,``` |
| :---: | :---: |
| 5＂ |  |
| 40 | INPUT |
| 50 | DIM F（ ${ }^{(1)}$ |
| 50 | OIM Did） |
| 70 | OIM L（U） |
| 80 | DIM C Cu） |
| 92 | DIM T（a） |
| 100 | OIM H（S） |
| 110 |  |
| 200 | PRINT＂ENTER TRAP KMCHA |
| $\begin{aligned} & \text { DR T IF COAX } \\ & \text { SIO INPUT K } \\ & \text { SOG QRINT "STARTINE HITH HIEHES } \end{aligned}$ |  |
|  |  |
| T BAND，IN $N=1$ TOROER，ENTER＂ |  |
| 204 | PRINT AT E，E；＂FAER＂；幽， |
| 250 | INPUT F（N） |
| 260 | PRINT F（N），＂SECTIEM SEA＂； |
| 270 INPUT D（N） <br> 2BD PRINT D（N）＂TRAF＂；$\because$ ；＂L－UH <br> ，COPF＂＂OR Q FAK EAAK＂， <br> SgO INPUT TEMP |  |
|  |  |
|  |  |
|  |  |
|  |  |
| 310 IF K象＝＂C＂THEN LET E\N！＝TEH |  |
|  |  |
|  |  |
| 330 PRINT TEM |  |
| 335 | SCROL |
| 336 SCROLL |  |
| $337 \text { SC }$ |  |
|  |  |
| 339 Sc |  |
|  |  |
|  |  |
|  |  |
|  |  |
|  |  |
|  |  |
| 4 4D INPUT TRP <br> $4 \bar{Z} F \bar{F} \quad$ N $=1$ TO v－1 |  |
|  |  |
| 450 |  |
| 440 IF TRP＝7，8 THEW LET T TNT $=13$ |  |
| 450 IF TRP＝1， 4 THEN LET T \｛ V＝＝ER |  |
|  |  |
|  |  |
|  |  |
|  |  |
|  |  |
| 480 | NEXT N |
| 6OO REM DO |  |
| 610 FOR $N=1$ |  |
|  | IFK事三＂L＂OR K |
|  |  |
|  |  |
|  |  |
|  |  |
|  |  |
| $\{2 * P I * F$（N） |  |
| 60 | NEXT N |
| OQQ REM DO SEETI |  |
| 810 FOR $N=1$ |  |
|  |  |
|  |  |
| 840 NEXT N |  |
| 1000 REM MAIN LD |  |
| 10QS LET DEG＝0 |  |
| 1010 LET Hi1） |  |
| 1020 FOR $N=R$ TO |  |
| 1030 FOR $P=1$ TQ N－1 |  |
| 1040 LET M＝F M M M MP， |  |
|  |  |
|  |  |
| 1－M－M）${ }^{\text {® }}$（N）（N） |  |
|  |  |
|  |  |
| 1080 LET DE | NEXT P |
|  |  |
| 1110 LET DEC |  |
| L123 NEXT N |  |
| 2QQQ REM QUTPLT |  |
| 3010 CLS |  |
| 三®EQ PRINT＂FREO［IA LUH CPF HBE |  |
|  |  |
|  |  |


fig．2．Trap antenna program for 2X－81．（For copy of program written for Commodore 64，send SASE to ham radio．l

## coax can be used for traps

There is a special feature used in the program．This is a routine to calculate the number of turns of RG－58U coaxial cable required to resonate as a trap，as de－ scribed by Johns，W3JIP，${ }^{2}$ and to calculate the induc－ tance．If other coil diameters are needed，some expe－ rimental coils should be constructed and their frequen－ cy measured．The number of turns required：

$$
\begin{aligned}
& N=135.7 f^{-0.91} \text { on } 7 / 8 \text { inch form } \\
& N=68.86 f^{-0.86} \text { on } 1.5 \text { inch form }
\end{aligned}
$$

The inductance is calculated from Wheeler＇s formula，

$$
L=\frac{(D+0.2)^{2} N^{2}}{18(D+0.2)+8 N}
$$

where the 0.2 is the diameter of RG－58．These rela－ tions must all be changed if coax of another diameter and capacity per foot is used．

The final step in the program is conversion of the dimensions and printing the results．The sketch of fig． 1 should aid in keeping the quantities organized．In the above equations，a prime is equivalent to chang－ ing a subscript）．

## program listing

The BASIC program for the calculation is given in fig．2．Each section is set off by an REM statement to correspond to the program outline．The program is in Sinclair BASIC，but should run on any common home computer with minor changes．（A version for the Commodore 64 is available from ham radio；send SASE．）

fig. 3. Sample run of $\mathrm{ZX}-81$ program for five-band trap antenna using $7 / 8$ inch coax coils.

Fig. 3 shows a sample run. A five-band version using only one-inch tubing would be difficult to build, mechanically, but could be done by using glass-fiber lines for support. A three-band version using two traps is very practical. The writer, as experimental station KK2XJM, uses a six-band version covering $10,12,15$, 18,20 , and 30 meters.

The main calculation routine is also available for use on the HP 67/97/41 series of calculators. ${ }^{3}$

## construction hints

Note that these programs can be used for dipoles by entering wire diameter and by considering that the base section is measured from the center of the dipole to the first trap. When designing antennas using these programs, it is usually best to set the capacitance, since it is most difficult to change. Typical values for dipoles would be $25,35,50$, and 100 pF for the 10-40 meter traps.
The ARRL Antenna Handbook has some hints on construction, and there have been many articles on construction of both integral traps for beams and discrete ones for dipoles. Lately, the author has used only the coaxial trap design for HF. Trap tuning in all cases is by changing coil turn spacing. Sections should be built to allow some length adjustment - about four inches. If necessary, sections can be cut shorter, but the need for this should be rare.
To avoid making up new sections if they must be lengthened, a form of "capacity hat" may be used. This can be two lengths of small tubing clamped to the section to be lengthened at 90 degrees to each other. Tuning is accomplished by moving the "hat" toward or away from the top end of the section. The total length of each added section of tubing should be about twice the added length of section needed.

If the section lengths are excessive, the required lengths can be reduced by using the "capacity hat," a loading coil, or both. To calculate the effect of a loading coil, introduce a dummy frequency, a few percent lower than the value of the next higher band frequency, and use a trap inductance equal to the value of the loading coil contemplated. It will probably be necessary to make several trials to arrive at reasonable values (see sidebar).
Note that these programs are also usable for reso-
nant single-band antennas because the length of these is equivalent to the length of the first section of the trap antenna. Boyer's articles provide information that allows calculating the SWR versus frequency for these trap antennas.

## operate both phone/CW

Most trap verticals commercially available require separate settings in order to operate the phone or CW segments of the 40 and 80 -meter bands. The following design provides a low VSWR at both sections of each band. Overall length is just under 50 feet.

| FREQ | DIA | L-UH | C-PF | H-DEG | H-IN |
| :--- | :--- | :--- | :--- | :--- | :--- |
| 7.2 | 1.5 | 6.5 | 75 | 89.9 | 376 |
| 7.025 | 1.5 | 6.8 | 75 | 1.3 | 5 |
| 3.795 | 1.5 | 17.5 | 100 | 23.9 | 191 |
| 3.525 | 1.5 | 0 | 0 | 2.9 | 25 |

A more manageable height ( 38.8 feet) is achieved by using a loading coil for the 3.5 MHz portion:

| FREQ | DIA | L-UH | C-PF | H-DEG | H-IN |
| :--- | :--- | :--- | :--- | :--- | :--- |
| 7.2 | 1.5 | 6.5 | 75 | 89.9 | 376 |
| 7.025 | 1.5 | 6.8 | 75 | 1.3 | 5 |
| 6.75 | 1.5 | 55.5 | 10 | 1.5 | 7 |
| 3.795 | 1.5 | 17.5 | 100 | 7.8 | 62 |
| 3.525 | 1.5 | 0 | 0 | 1.4 | 12 |

A small further reduction in height can be obtained by changing the section above the last trap to a top hat: the diameter should be about one-half the length of the section. If still further reduction in height is needed, another loading coil could be placed near the top of the 40 -meter section.

The trap quality in these designs must be very good. The coil should be about twice the diameter of the section, made of large wire or small tubing, and spaced to give a length about equal to the diameter. The 7.025 MHz trap and the loading coil can be wound as one coil, tapped for the capacitor connection.

These designs have not been tested. Because of the closeness of trap frequencies, expect to do some adjustment after construction.

## references

[^4]ham radio

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fig. 1. Flowchart for basic frequency counter.

## Build a versatile test instrument with digital display and microprocessor control - for less than \$50

Digital displays for radios have been around for several years, and most people have grown quite used to their appearance and operation. After purchasing an inexpensive HF transceiver without a digital display, I actually felt a little lost because I had been used to seeing the digits flicker as I tuned across the band. So I decided to add a digital display to my unit that would also function as a normal frequency counter.

This article describes not only how to build a gen-eral-purpose microprocessor-controlled frequency counter, but also provides some routines that will allow the counter to be used as a digital display for a radio. In production quantities, this frequency counter could be built for about $\$ 10.00$ or $\$ 15.00$. In single quantities, a price of less than $\$ 40.00$ to $\$ 50.00$ would be more realistic. A parts list at the end of the article provides prices and quantities required.

In trying to determine the actual operating frequency of a radio, several problems can arise. Depending on the type of radio (single conversion, dual conversion, direct conversion, etc.), different counting methods must be used to determine operating frequency.
It's easiest to provide a digital display for a direct conversion type because the actual VFO frequency is the operating frequency. In fact, any frequency counter may be used to measure the operating frequency.

On single conversion radios, the frequency to be counted is either the sum or difference of the VFO and HFO. In this configuration, several things must be considered: if selectable sideband operation is required,

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fig. 2. Basic frequency counter schematic.
some provision must be incorporated to allow shifting of the displayed frequency. Generally, this is an additional wafer on the mode switch. Also, in counting the frequency, the MHz may or may not be valid (with respect to the operating frequency), but the 100 kHz (and down) digits would be correct. To provide a correct MHz reading, an additional wafer on the bandswitch is required. One alternative is to read the HFO, read the BFO, and either add or subtract the two, depending upon which is necessary.

On double conversion types of radios, the counter must be preset to get the correct frequency, and the mode taken into account. On both the single and double conversion radios, it is obvious that some necessary "smarts" must be incorporated by the counter
to make it display the proper frequency. A normal frequency counter could not easily be modified to provide these features; instead, a microprocessor would be an ideal choice for this function.

## description

The heart of the counter is the MC68705P3 microprocessor, an EPROM, which means that a user can erase the internal program using ultraviolet light, and reprogram it many times. (In a production-type environment, a mask-programmed part would be used. Mask programming is done as a one-time shot at the factory, and is much less expensive than the EPROM part.)
Programming the EPROM is a simple task that may

fig. 3. The serial display can be separated from the microprocessor.
be done by anyone; Motorola's Application Note $A N-587$ and the accompanying data sheet contain instructions.

## operation

Most frequency counters use a high frequency time base, divide it down, and use it to allow a certain number of input pulses to go into some BCD counters. These counters then feed the normal latches and BCD to 7 -segment decoder drivers for the display. In the MCU (microcomputer unit) version of the frequency counter, the MCU controls the actual time base generation, latching of data, and driving of an external display. A basic block diagram of the system is shown in fig. 1.

The inputted analog signal is conditioned and amplified, which means it's turned into a digital signal that the computer system can use. A two-input NAND gate is fed by both this signal and another generated by the computer. The computer-generated signal actually inhibits the input signal from propagating through the counters. Only by having the capability of turning off the frequency source can an accurate count be made. The output of the gate (NAND) is fed into the BCD counters, which do the actual counting. These counters have a "clear" input on them which allows them to start at a count of 0000 . This signal is, of course, controlled by the MCU. After being cleared, the

LS390s count until the 10 millisecond period (generated by the MCU) has been completed. At this time, the MCU disables the gate, reads the data in the counters, and sends that information serially to the display drivers.

The most critical component of any frequency counter is the time base, and this device is no different. A 4 MHz crystal is used as the clock for the MCU, which in turn controls the actual 10 millisecond gate period. To adjust the counter, the highest frequency to be counted should be measured by an external frequency counter, and the trimmer capacitor on the crystal should be adjusted to give an identical reading. For further stability, an external temperature compensated oscillator may be used. Do not try to count the time base by measuring one of the crystal pins. Even an extra load of 5 pF is sufficient to shift the time base frequency and degrade the accuracy of the counter.

The basic frequency counter schematic (fig. 2) can be easily added to a radio such as the Ten-Tec Argosy. Note that while the MHz display option may be incorporated through the addition of a bandswitch, further cost reductions may be realized by only having four digits displayed, with the MHz being read off the band switch.

## reducing computer-generated noise

In any system that uses a computer, some noise is

fig. 4. Basic frequency counter block diagram.
generated. Even with an MCU, which has most of the noisy circuitry inside the ceramic package, fast transitions of the I/O lines will cause some RFI. I recommend that any computer used in a radio environment be shielded. This may be done in several ways. One method employs thin PC board or copper flashing to make a box that totally shields the MCU. This cuts down on most noise that may be generated from the computer. This is especially necessary when the computer is of the "wire-wrap" or hand-wire construction.

## expandability in a single chip MCU

With the advent of single-chip microcomputers, many new "peripheral" parts (those which do some function external to that of the main computer chip) are being designed to "talk" serially. By sending the data down lines in a serial bit stream, many extra I/O pins may be saved for other functions. That is the name of the game in an MCU environment, because once all I/O lines have been used, sometimes a total re-design of the system is required to get "just one more." A good example of this concept of serial peripherals is shown in the schematic of fig. 2.

The display device used, the MC14499, is of this
serial variety (saving I/O pins). Each device is capable of driving a total of four seven-segment LEDs, but the first counter example requires only one. In more sophisticated systems, two 499s could be used to provide a total of six digits. The MC14499 is a simple part to use, and the only external components required are eight current limiting resistors (seven for the segments, and one for the decimal point), four transistors, and a small capacitor. This makes for an easy layout, and since the data is sent serially, the display can be remote from the actual MCU. Fig. 3 shows the display schematic and required hardware.

To re-emphasize the importance of serial-type peripheral devices, consider the number of $I / O$ lines which are required to drive four digits of LEDs. To do this directly, at least sixteen lines are required. This would really be a waste! By using the serial format (data, clock, and enable), only three lines are needed for the first display driver. To add additional drivers, add only one more enable line for each device. The data and clock lines are common.

## alternate displays

If an LCD type of display is desired, an MC145000


| 100 | 0008 $20 \mathrm{F4}$ |  | BRA | CLOCK2 | GO CLOCK IT |
| :---: | :---: | :---: | :---: | :---: | :---: |
| 101 |  | * |  |  |  |
| 102 |  | RESTART VECTORS |  |  |  |
| 103 |  | * |  |  |  |
| 104 | 07F8 |  | ORG | \$7F8 |  |
| 105 |  | * |  |  |  |
| 106 | 07F8 0080 | TIMER | FD8 | START |  |
| 107 | 07FA D0 80 | EXTINT | FDB | START |  |
| 118 | 07FC 0080 | SWIINT | FDB | START |  |
| 119 | O7FE 0080 | RESET | FDB | StART |  |
| 120 |  | * |  |  |  |
| 121 |  |  | END |  |  |

fig. 5. Software for the MC68705P3.
may be used to drive a six-digit multiplexed LCD. The data format is a bit different than that of the 14499, but it is also a serial device and quite easy to use.

Several other serial parts - and microcomputers to talk to them - are becoming available. The MC144110 is a 6-bit D to A converter; the MC144102 is a $16 \times$ 16 bit RAM; and the MC145157,58, and 59 are seriallycontrolled PLLs. Look for more functions to be available in the future which use this type of data transfer.
The ability to use these serial devices is greatly enhanced by the instruction set of the M6805 family of processors. Through the use of the "Bit Set/Bit Clear" instructions, any $1 / \mathrm{O}$ pin or RAM bit may be set or cleared with a single instruction. (This is in contrast to other, generally older, microprocessors that need to get the entire 8 -bit port into a single register, and then do an appropriate Boolean instruction to set or clear the bit - AND, OR, XOR, etc. The entire word then had to be stored back to that port. This required several instructions and a lot of time to implement.) With true bit-manipulation, any type of serial data transfer is easy; several other instructions also simplify work in a controller environment. The "Branch if bit Set/Branch if bit clear" instruction uses this bit manipulation architecture in a branching situation to do things that depend on what an individual bit's state is.

## software

A flow chart of the "simple" 4 -digit counter is shown in fig. 4, and the actual software for the MC68705P3 is shown in fig. 5.

## future developments

From the discussion above, it can be seen that increasing the range of the counter is quite simple. Additional counters, prescalers, or other range-extending devices may be implemented. By placing these prescalers in front of the 74LS000 gate, frequencies greater than 1500 MHz may be counted. Or how about a full-function DVM \& frequency counter all in one small package? By using the MC68705R3, which also incorporates an 8 -bit A to D system on chip, a complete DVM could be implemented with appropriate scaling resistors.
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## SUCCESS



## SPECIFICATIONS AND FEATURES

## 4248:

$424-435 \mathrm{MHz}, 7.6 \lambda$, gain * maximized, F/B ratio 'excellent, bearnwidth $19^{*}$, length 17.42 ft .5 .2 m . 410B:
$424-435 \mathrm{MHz}, 2.2 \lambda$, gain *maximized, F/B ratio 'excellent, beamwidth $33^{\circ}$, length 6 ft .1 .83 m . 416 TB :
428.438 MHz , Circular Polarization $2.2 \lambda$ gain *maximized, F/B 'excellent, beamwidth $34^{*}$, length 6.7 ft .2 .03 m .

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| 32.19 | 144.146 MHz | 19 elements |
| :--- | :--- | ---: |
| 214 B | 144.146 MHz | 14 elements |
| 214 FB | $145.5 \cdot 148 \mathrm{MHz}$ | 14 elements |
| 228 FB | $145.5 \cdot 148 \mathrm{MHz}$ | 28 elements |
| 220 E | 220.223 MHz | 22 elements |
| 617.6 B | 50.51 MHz | 6 elements |

[^5]

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## 80-meter half-wave sloper uses reflector

This antenna was the result of a desire to work 80-meter DX running low power. Many excellent reports have been received, including long path to $V K, Z L$, and JA.

The antenna, basically a doglegged, 1/2-wave sloper, uses a fulllength reflector (fig. 1). The reflector is the tower plus enough wire hooked to the base and extended out under the sloper to give a full-length ( $1 / 2$ plus 10 percent) reflector. The driven element is a folded dipole which can be fed with 300 -ohm feedline or used 50 -ohm line when a $4: 1$ balun is inserted (I used the 300 -onm feedline). Because the amount of doglegging affects the feed impedance, it should be adjusted for minimum SWR. (The closer the antenna is to the tower, the lower the impedance). I used 18 gauge 300-ohm ribbon for QRP; later, when I ran 800 watts, no heating was noted. 18 gauge can easily handle 2 amperes, or 1200 watts at 300 ohms; open wire 300 -ohm line is a better choice if available. The dog-legging causes the pattern to "squint" in the direction of the dipole. I estimate the gain (over a dipole) to be 4 to 6 dB . The angle is low enough to produce good long path results. (The author has been able to consistently contact VK6LK-Robin almost throughout the entire year Ed.)

Use very good end insulators for the driven element to prevent arc-over or leakage. Plexiglas (1/4-inch thick) works very well and is easy to obtain as scraps from manufacturers or others working with it. With the feedline connected to the physical center of the antenna, the portion of the dipole toward the tower may have to be shortened 6 to 15 inches in order to
maintain electrical symmetry. The end of the folded dipole is connected to a single wire to facilitate tuning (see fig. 2). Last but not least, use a rope and pulley to connect it to the top of your tower unless you really like to climb.

Bruce Clark, KO1F

## Argonaut 509 conversion for 30 meters

As declining HF propagation renders the 10-meter band less of a dependable mainstay for the QRP operator, the new"allocation at 10 MHz is coming into its own for this mode of activity. The operating restrictions imposed upon 30 meters actually help rather than hinder QRP operation.

fig. 1. Modification of the Argonaut Model 509 transmitter section only requires adding two capacitors to the T7 tuned circuit on the 80262 board.

The Ten-Tec Argonaut 509 may easily be modified to cover 30 meters with the same performance found on its five bands. All that is required for the modification is five minutes of time, four components, and a jumper wire.

Ten-Tec uses a $9-\mathrm{MHz}$ IF with appropriate VFO frequencies. On 10 meters, the VFO ranges from 19 to 21 MHz . If we use the difference mixer product, rather than the sum, as in the original design, output occurs on 10 MHz rather than 28 MHz . Since the 509's transmitter stages are broadband amplifiers, the only changes required for 10 MHz transmit are to re-resonate the appropriate bandpass filter, composed of 77 and capacitors C17 and C18 on the 80262 front-end board (see fig. 1). Shunt C17 and C18 each with an additional 91 pF of capacitance. De-

fig. 2. Modification of the receiver section of the Argonaut 509 requires minor additions to components switched by S3B and S3D.
pending upon component tolerances, retweaking 77 cores may be necessary for adequate output. The addition of the two $91-\mathrm{pF}$ capacitors completes transmitter modification.

The receiver will function with much reduced performance without modification by turning the receive preselector completely counterclockwise, as mentioned in the 509 manual for WWV reception. To improve 10 MHz performance the receiver front end needs additional capacitance.

C1, on the main schematic, is switched across T1 to resonate at the desired band. For our purposes, C1 needs to be shunted with another capacitor, again of 91 pF , as seen in fig. 2. T2, on the other end of the RF amplifier front end, must also be resonated at 10 MHz . Shorting C7 with a piece of tinned bus wire and parallelling variable C8 with an additional 47 pF completes our modification.
The modification is simple and quick. Lifting one end of each added component easily restores 10 -meter operation when the sunspot activity increases.

Modification of the newer Model 515 is identical. The rig that began it all, the 505 , is not broadbanded on transmit.

Raymond Henry, AA4LL

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[^6]
## audio oscillator to pulse generator conversion

Here is a quick, simple method for converting an audio oscillator into a pulse generator that has served well on bench digital projects. (See fig. 1.)

To cover the full range from 10 Hz to $1 \mathrm{MHz}, \mathrm{C} 1$ and R1 may be either fixed in values with C 1 from 0.1 to $0.001 \mu \mathrm{~F}$ and R1 from 10 k to 1 megohm, or C 1 fixed at 0.1 and a 1 megohm pot used for R1. The drive input from the oscillator should be 1.5 to 3.5 -volts rms if Q 1 is a 2 N 2222 and a 0.75 -volt rms if Q 1 is an MPF6515.

The pulse width is directly related to the oscillator frequency, with the narrowest being $0.6 \mu \mathrm{~s}$. For applications requiring fast pulse triggers, the similar circuit using 02 and the unused two sections of IC1 will provide a fine $1 \mu \mathrm{~s}$

fig. 1. Audio oscillator conversion schematic.
pulse with polarity selected from the IC1 outputs as shown.

Assembly can be accomplished on
a piece of perf board with direct pin wiring in about 30 minutes.

Gene Shapiro, W0DLQ


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## VHFIUHF WORLD

## VHF/UHF frequency calibration

Have you ever wondered whether you're really on frequency - especially when you don't hear the station you're scheduling? This is a constant problem for the VHF/UHFer, especially during meteor scatter or EME schedules. Because the focus of this issue is on test equipment, I thought it would be a good time to discuss frequency accuracy and offer some advice on accurately determining frequency. Then I'll describe a secondary frequency standard or calibrator you can build to sat-
isfy most of the needs and pretty much guarantee that you're at least on the frequency you think you're on!

## frequency determination

There are several ways to determine frequency. You can:

- read the frequency indicator on the gear in use;
- trust the frequency of the crystal in your up or down converter;
- have a reliable friend measure your transmitted frequency;
- buy or build a good frequency counter; or
- build or buy a good secondary frequency reference standard.

fig. 1. Typical frequency drift versus temperature for a $\mathbf{4 8}-\mathrm{MHz}$ overtone oscillator.

All of the above methods have advantages and disadvantages. While you may laugh at the thought of just reading your dial or frequency indicator, some modern commercial gear transmits CW at an offset frequency that may not be directly indicated.

Recently I tested one of the latest state-of-the-art VHF/UHF multi-mode transceivers complete with a built-in digital frequency readout. To my amazement, the frequency indicated was off by almost 1 kHz in the first 15 minutes; even after an hour the frequency indicated on UHF was off by over 0.5 kHz - admittedly not a serious problem, but one worth examining if frequency accuracy would affect the success of a OSO or the accuracy of measuring someone else's transmitted frequency.

## crystal oscillators are used everywhere

All modern converters or transverters use crystal oscillators in one form or other. However, if 1.0 kHz accuracy is required at UHF, the cost of a crystal is prohibitive. Furthermore, the accuracy of the oscillator is also a function of the oscillator circuit and the temperature of the crystal. Some designs use small trimmers to tweak the frequency to the marking on the crystal, but this can have disastrous effects on phase noise, not to mention decreased temperature stability or drift. ${ }^{1}$

All crystals, regardless of price, suffer from a problem called "aging." This means that a crystal will always be drifting slightly away from its marked frequency even after it has been burned in for a predetermined time. (The typical commercial standard is full power for 30 days.)

Suppose a friend measured your
transmitted frequency. D:d he or she tune you in properly on SSB? on CW? Was he or she at true zero-beat? Even if the measurement is accurate, how do you account for local ambient temperature changes, aging or drift and component changes in your own gear
at a later time and date? How long does it take to properly warm up your gear?

Frequency counters are great, but until recently they were beyond the reach of most Amateurs. Several are now available, but suitable ones use a

fig. 2. Typical frequency drift versus temperature for a 1.000 MHz secondary frequency standard.

fig. 3. Typical impedance versus frequency variation for a quartz crystal operating in the fundamental mode. " $\mathrm{f}_{s}$ " is the series resonant frequency and " $f_{p}$ " is the parallel or antiresonant frequency. The typical bandwidth is $5-10 \mathrm{kHz}$ at 4.000 MHz . The parallel resonant frequency can be varied by the use of an external capacitor in series or parallel with the crystal.
reference standard and a proportional control oven that takes time to stabilize - perhaps 15-30 minutes - and usually cost about as much as a typical multi-mode transceiver! Furthermore, frequency counters that read higher than 600 MHz are even more expensive.

## there is another way

A good method that seems to have been almost forgotten by the users of modern rigs is the secondary frequency standard or crystal calibrator. If one is available with a comb generator (a device which generates many harmonics of the input frequency), it can be used up through UHF with surprising accuracy. ${ }^{2}$
After evaluating all these alternatives to accurate frequency determination at VHF/UHF frequencies, 1 decided many years ago that the least expensive and most accurate way to measure my frequency was to build a secondary frequency standard. Before designing one, I listed the features I wanted to include:

- convenient marker frequency in each VHF/UHF band above 6 meters
- good short and long-term stability, 1 to 2 parts per hundred million (0.01-0.02 ppm)
- easy adjustability to the correct frequency
- high harmonic output through 2304 MHz
- battery operation
- fast warmup
- reasonable size, including built-in antenna
- easy construction
- low cost

This is indeed quite a "wish list!" However, after some trial-and-error (over a period of 15 years) such a unit has evolved.
The most important consideration for a secondary standard is crystal stability. First, 1 tried a third-overtone $48-\mathrm{MHz}$ crystal oscillator. Harmonics were no problem, but stability, the very property I wanted to measure,
was no better than the local oscillators in my receiver or transmitter - about 3 to 4 parts in 10 million per degree Centigrade (fig. 1). Also, the only usable harmonics were on 144, 432, and 1296 MHz .

Next, a $1.000-\mathrm{MHz}$ calibrator was tried, but proved quite unsatisfactory for several reasons. ${ }^{2}$ First, it is difficult to produce sufficient harmonics to reach the lower UHF bands. After all, for $70 \mathrm{~cm}(432 \mathrm{MHz})$, that is the 432 nd harmonic! Second, and more important, the frequency stability of a good $1-\mathrm{MHz}$ crystal versus temperature is quite poor. I measured such a unit at typically 500 to 600 parts per million per degree Centigrade (see fig. 2).

After discussing this with crystal manufacturers 1 discovered that reasonably priced, stable crystals and oscillators can be designed and built without an oven if you choose an "AT" cut fundamental crystal in the 3 to 10 MHz region (more on this later). 4 MHz was chosen because harmonics would be present on all of the VHF bands above 6 meters, lending itself to easy calibration with WWV on a $20-\mathrm{MHz} \mathrm{HF}$ receiver. Later I built a $5-\mathrm{MHz}$ unit to be used on 6 meters and other multiples of 5 MHz .

## the circuit you choose is important

Crystals are usually classified as either fundamental or overtone. Because of cost and stability constraints, fundamental crystals are usually used below and overtones above 22 MHz . Each fundamental crystal has two basic resonances, a series and a parallel or anti-resonance. The series resonant frequency is typically a few kHz below the parallel resonant frequency and is very difficult to externally move or adjust. However, the parallel mode resonant frequency can be easily adjusted by placing a capacitor either in parallel or series with the crystal. These characteristics are shown in fig. 3. A parallel mode oscillator was chosen for this reason. The Pierce oscillator circuit was first used because it is reputed to be the most stable, but the parasitics of the active device in the oscillator

fig. 4. Typical frequency drift versus temperature for an "AT' cut high-accuracy crystal at 4.000 MHz .

fig. 5. Frequency versus temperature variation of the 4.000 MHz calibrator in fig. 6. For various amounts of temperature compensation " $A$ " is undercompensated while " $B$ " and " $C$ " are optimum versus desired temperature range, toward either cold or hat.
are prominent. Therefore, a modified Colpitts oscillator circuit was later chosen because it was only slightly less stable than the Pierce oscillator, but more easily adjustable, and uses swamping capacitors to minimize the parasitics of the active device.
" $A T$ " cut crystals have a known frequency versus temperature characteristic that is " S " shaped (fig. 4). Hoff has pointed out that if you want to operate only over a small temperature range such as experienced in most ham shacks, the frequency change is

fig. 6. Schematic diagram for a $\mathbf{4 . 0 0 0} \mathbf{M H z}$ secondary frequency standard.
quite linear and can be decreased over a small temperature range (perhaps 10 to 40 degrees Centigrade) by simply placing a temperature compensating capacitor in series or parallel with the crystal. ${ }^{3}$

Indeed, this is what I did. First an NPO (which has close to zero temperature drift) temperature compensating ceramic disc capacitor (in parallel with a tweaking capacitor) was placed in series with the crystal in an oscillator. Then the frequency versus temperature was measured in a laboratory oven in 5 -degree Centigrade steps and the frequency was remotely measured with a good frequency counter having a proportional control oven. The NPO capacitor was then replaced with various combinations of 10 pF N750 type temperature compensating ceramic disc capacitors and data taken again. It soon became obvious that the temperature drift could be minimized by the right choice of temperature compensation. This is illustrated in fig. 5 for a typical $4.000-\mathrm{MHz}$ crystal oscillator.

## now for those harmonics

Now that I had the oscillator working, I tried various schemes to generate a comb of harmonics. Integrated circuits were discarded because they required considerable current and did not extend high enough in frequency. Tunnel diodes were also tried but did not meet the UHF harmonic requirements. ${ }^{2}$

SRDs (step recovery diodes), properly chosen, fit the desired requirements. Furthermore, if used in the proper circuit, they required low RF drive and could generate power through 2304 MHz . Oscillator-multiplier isolation is required so that frequency stability or calibration is not affected by the multiplier or output circuitry. This was accomplished by using a separate amplifier or buffer stage between the oscillator and multiplier.

## values are now chosen

Several solid-state devices and circuit configurations were tried. JFETs and MOSFETs were eventually dis-
carded in favor of bipolar transistors since the variation from unit to unit necessitated additional tweaking for proper bias and compensation. An os-cillator-amplifier approach was used in the first few calibrators but eventually replaced by a cascade bipolar transistor circuit that provided the required oscillator to multiplier isolation with low power consumption and could be powered by a 9 -volt transistor radio type battery.
A schematic of the final circuit is shown in fig. 6. The modified Colpitts oscillator uses a bipolar transistor, Q1. The trimmer, C1, should be a high quality air dielectric variable with a multi-turn fine adjustment screw. C2 and C3 are the temperature compensating disc ceramic capacitors. The typical oscillator required 20 pF N750 capacitors and in the extreme case required 20 pF N1500 compensation. The feedback capacitors, C 4 and C5, should be NPO-type ceramic disc capacitors. Do not use silver mica capacitors here; they have a positive temperature coefficient that will increase the drift!

Crystal specification is most important. Beware of bargain basement or computer-type crystals. They may be specified for series resonance or have a poor temperature coefficient, which will make it nearly impossible to tune or compensate the calibrator at the desired frequency. International Crystals* sells a "HA" (high accuracy) crystal that should meet the requirements. The price may be higher than you're used to paying for a crystal, but because you'll probably use this secondary reference standard for many years the crystal will pay for itself many times over. Remember to specify the crystal as parallel resonant with 20 pF of capacitance. The temperature tolerance should be $\pm 0.0005$ percent from -30 to 60 degrees Centigrade. The calibration tolerance can be $\pm 0.0025$ percent. Over-specifying the actual calibration frequency is a waste of money because the trimmer will adjust you precisely to zero-beat.

[^7]
## reducing supply voltage dependency

A recent addition to the circuit was a zener diode in the amplifier stage. This provides a good reference voltage to the oscillator over a wide battery voltage range with very little extra power consumption. A standard 9 -volt transistor radio type of battery, preferably the longer life type, is all that is required because the current drain is typically 4 to 5 milliamperes. Another recent innovation is the LED llight emitting diode) in series with the battery. This provides a low-power indicator to remind you to turn off the calibrator when not in use. A battery test point is also provided so that you won't have to open the box to measure the battery voltage.

The multiplier circuit also evolved over the years. A simple pi-network matches the amplifier output to the SRD. The SRD chosen should be of the long lifetime type, typically 100 nanoseconds minimum, since 4 MHz is a very low input frequency for many SRD's. Other types of diodes will probably not work well. C6 peaks the circuit, which matches the amplifier to the SRD. The output of the SRD passes through a 15 MHz high-pass filter, suppressing the fundamental frequency of the comb output. Therefore a calibrator output circuit was added in case you desire to measure frequency directly (such as with a frequency counter) at 4.000 MHz . The typical comb generator output power versus frequency curve is shown in fig. 7.

## construction

The entire circuit including battery can be built on the cover of a Pomona model 2901 or equivalent cast box. First a double-clad printed circuit board about $1-7 / 8 \times 3$ inches ( $48 \times 76 \mathrm{~mm}$ ) is attached to the cover of the box and held in place by the output connectors, switch, trimming capacitor, and LED. A suitable battery clip is mounted on the remaining available space on the box cover. Two insulated standoff terminals are used to hold the crystal

fig. 7. Typical output power versus frequency from a secondary frequency standard comb generator.
leads and associated temperature compensation capacitors. The wiring is done point-to-point in space, as suggested in previous articles.'

## initial testing and calibration

If you don't want to go through the temperature calibration procedure described, just use 10 pF N750 capacitors for C2 and C3 and you should be very close. A small 2-meter quarter-wave pull-up type whip makes a suitable radiating antenna for the entire spectrum of interest. The calibrator is now ready for testing. This can be easily done by listening for the 7th harmonic on a $28-\mathrm{MHz} \mathrm{HF}$ receiver (the signal may not be strong at this frequency) or the 36 th harmonic at 144 MHz on a 2 meter receiver. First peak C 6 for maximum output on a 2 -meter or higher receiver. Next, vary the calibration trimmer, C 1 , and check that the frequency varies a few hundred Hertz and that it is approximately correct. If the frequency is too low, either C2 or C3 will have to be decreased by perhaps 5 pF .
To verify adequate temperature compensation, you'll have to measure the output, preferably with an accurate frequency counter, or zero-beat it with WWV at 20 MHz using a suitable HF receiver. The entire circuit can then be placed in a refrigerator, Itypically about

41 degrees Fahrenheit or 5 degrees Centigrade). Measure the frequency after it's been in the refrigerator for 15 to 30 minutes. Compare the reading to the one made earlier at room temperature. After a few tries, you will see if the calibration is adequate. If the temerature drift when the calibrator is cold causes the frequency to go below the room reference frequency, too much compensation is being used, and vice versa. (See fig. 5 for further information.) Also, whenever you change a capacitor, allow at least 15 minutes for its temperature to stabilize before taking data.

Zero-beating to WWV can be tricky. It's best to move the calibrator around the room until the proper amount of injection is experienced. Also try to zero-beat during the interval when the tones are not present (usually the last 15 seconds of each minute). Watching the " $S$ " meter can be quite helpful. When close to zero-beat, the meter will waiver noticeably and the beat will sound like a chirping canary. When the meter moves once per second, you are within 1 Hertz of the correct frequency. One beat every 15 to 30 seconds is very satisfactory. Be aware that because of atmospheric effects the accuracy of WWV on the HF spectrum is good only to about 1 part per hundred million. However, this should be


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## short circuit

## VHF/UHF World

A chart in fig. 9 (page 88) of W1JR's "VHF/UHF World" column in April, 1984, made reference to "Note 1." Unfortunately, Note 1 was not included at the bottom of the figure, as the author intended. Note 1 should read, "Not used on this frequency."
more than sufficient for Amateur work.

## using the calibrator

At first, it will be worthwhile to test the accuracy of the calibrator several times during the first few months of operation because some aging will inevitably occur. This will also let you develop confidence in its use. After initial burn-in, I usually test calibration against WWV about once a year. One caution is advised: Do not place the calibrator where it will be subjected to temperature variations such as on top of another piece of electronic gear. I usually place mine on a table or desk one or two meters away from the receiver in use. This yields more than adequate injection even at 2304 MHz . Typical warmup is 15 seconds. To conserve battery life, don't forget to turn the calibrator off when not in use!

## summary

Even though the state-of-the-art in accurate frequency determination has advanced significantly in recent years, a secondary frequency standard is still useful for verification of true frequency. The calibrator just described is easy to construct and adjust, relatively inexpensive, very stable, and portable. I now have six of these units operating on different frequencies and always carry one along on expeditions. Once you have one, you'll never want to be without it.

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## VHF/UHF coming events

October 6: Mid-Atlantic States VHF Conference, Warrington, Pennsylvania. IContact W3CCX for information.)
October 6-7: International Region I UHF/SHF Contest. (Contact RSGB for information.)
October 20 and 21: ARRL International EME Contest (second weekend).
October 20: Predicted peak of Orionids Meteor Shower at 0515 UTC
October 24: EME Perigee
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# a high-efficiency top-loaded vertical 

# You don't need traps, coils, or vast acreage to get good performance on 160, 80 , or 40 meters 

The efficient, easy-to-build antenna described in this article requires no radials, traps, or loading coils. The reader with an appetite for low-band DX should be able to duplicate or better my results on 160 meters and, by appropriate scaling, on 80 and 40 meters as well.

Like any serious low-band DXer, I wanted to join the "big boys" using a vertically polarized signal because it has long been demonstrated that horizontals, unless raised to astronomical heights, are unable to do much more than take up space at the bottom of the pile-ups. ${ }^{1}$ The customary current-fed, $1 / 8$ - or $1 / 4$-wave type verticals require an immense radial ground system to be efficient and competitive - yet my terrain consists of deep ravines, gullies, and cliffs that make the installation of radials, or even elevated counterpoise systems, virtually impossible. To add to the misery, the soil at my OTH is almost 100 percent hard sandstone and as such approaches pure silicon in conductivity. Obviously a "non-standard" approach to an antenna was necessary. After reviewing many texts and articles I decided that some form of "ground independent" antenna would be required, particularly one that had its feed point at ground level. The "Bobtail Curtain" ${ }^{2,3}$ version of ground-independent systems met the basic requirements, but for 160 or even 80 meters the dimensions become truly heroic; in addition, my requirement was for unidirectional transmission. My first step was to contact my old friend Woody Smith, W6BCX, who had fathered the fabulous Bobtail, in order to get firsthand information on the "care and feeding" of this type of system.

My call to Woody obviously struck a responsive chord and after a few thousand well-chosen words and equations, we agreed upon the novel form of vertical that this article describes. Sparing you the background - which covered inverted ground planes, slopers, center-fed loaded dipoles, and of course the Bobtail itself - the general parameters decided upon were that the new vertical design should require supports no higher than 70 feet ( 21.34 meters) for the 160 meter version or 35 feet ( 10.67 meters) on 80 ; should not need more than 95 feet ( 28.96 meters) spacing between supports on 160 and half that on 80 ; should be highly efficient in power transfer; should exhibit a high impedance feed point at the bottom of the vertical radiator and should be relatively easy to construct

fig. 1. Efficient top-loaded vertical dimensioned for 160-meter operation.

By Howard F. Shepherd, W6US, c/o Hypercom, P.O. Box 768, Del Mar, California 92014

fig. 2. Plot of resistive and reactive component of 160 -meter top-loaded vertical versus frequency.

## item description

L1 40 turns No. 10 AWG spaced 0.2 inch per turn, 4 inch diameter
L2 7 turns No. 10 AWG spaced 0.2 inch per turn, 5-1/4 inch diameter
C1 two $500 \mathrm{pF}, 2000$ volt variable capacitors in parallel
C2 $500 \mathrm{pF}, 500$ volt variable capacitor with $0.002 \mu$ F mica in parallel
C3 100 pF, 20 kilovolt fixed vacuum capacitor
Note: For upper portion of 160 meter band, L1 is tapped down 8 turns by HV relay and $0.002 \mu \mathrm{~F}$ mica is disconnected from C2 by another relay.
and test using easily obtained materials. How did it work out? If you're not one of the fortunate few who already have a full $1 / 2$-wave vertical on 160 complete with at least 120 radials or a solid silver-plated copper ground sheet of comparable size, read on!

Fig. 1 shows the physical layout of the W6US 160 -meter vertical. No. 14 AWG copper wire is used throughout. The vertical radiator uses three wires spaced 1 foot ( 30.48 centimeters) apart by $3 / 8$-inch $(0.95 \mathrm{~cm})$ diameter wooden dowels. Because the wires are at the same potential, no special treatment is required for the dowels electrically, but a coat of varnish or wax enhances their weatherability. The use
of a four- or six- wire cage feet ( 1.22 meters) in diameter would be helpful as far as increased bandwidth is concerned; however, unless the effective conductor diameter of the diamond-shaped single-turn top loop is also increased by paralleling wires, don't expect to greatly widen the frequency response. ${ }^{4}$ it should be noted that if the vertical radiator is so increased in electrical length, the physical length of the kop will have to be decreased, and provision made for the increased weight of the cage system.

## how does it work?

The general theory of operation presents little mystery, but despite the W6US system's resemblance to the usual "top-loaded" short vertical, the reader will note that in essence the feedpoint is at the end of an electrical $1 / 2$-wave of conductor and represents a point of high radiation resistance and impedance. This becomes paramount when the efficiency of this antenna is compared to that of the usual top- or bottomloaded systems. ${ }^{5}$
antenna efficiency $=\begin{aligned} & R_{\text {rad }} \times 100 \\ & R_{\text {rad }}+\text { all circuit resistance }\end{aligned}$
where $R_{\text {rad }}=$ the radiation resistance of the antenna and "all circuit resistance" represents the resistance of the ground system, the loading inductors, wire resistance and any other resistances present which dissipate power as heat.
A resonant $1 / 4$-wave vertical exhibits a $R_{\text {rad }}$ of about 36 ohms with 10 ohms representing the total resistance of the ground system, coupling circuit, and other loss elements. Inserting these two numbers in eq. 1 produces an efficiency of 78.26 percent. On 160 that $1 / 4$-wave vertical would be about 130 feet ( 36.92 meters) tall. If instead a 60 -foot vertical ( $1 / 8$-wavelength high) is used, the $R_{r a d}$ drops to around 4 ohms and the efficiency diminishes to 28.57 percent $!^{6}$ For 100 watts transmitter output, only 28.57 watts would be radiated - about one-third of the radiation from the full size $1 / 4$-wave vertical, assuming the losses were identical (which is really not the case because the shortened vertical would require more coupling inductance and consequently more power would be consumed in the coupling circuit instead of reaching the antenna).
This is where the W6US ground independent system enters the race with a big lead. From fig. 2, which depicts the variation in measured antenna resistance and reactance of the system shown in fig. 1 note that at resonance - i.e., zero reactance - the resistance is close to 5000 ohms. Applying this number in eq. 1 and assuming for the moment that the "all circuit resistance" figure stays at 10 ohms, the efficiency is 99.8 percent - almost four times the indicated

fig. 3. Coupler houses high voltage matching circuit components.
efficiency of the usual 60-foot vertical radiator! This type of effect is exactly what makes the Bobtail and its other cousins such real winners. Best of all, this is achieved without an extensive ground radial system. In this case a $10 \times 10$ foot ( $3.05 \times 3.05$ meter) square of galvanized poultry wire is all that is necessary. A $1 / 2$-inch ( 1.3 cm ) 8-foot ( 2.43 meter) copper pipe is driven into the ground at the center of the wire screen for lightning protection. The small "coupler house" is placed on this screen as shown in fig. 3 with the ground portions of the coupling circuit strapped to the pipe, which in turn is bonded to the poultry wire.

The resistance/reactance graph shown in fig. 2 illustrates that these curves are steep with respect to frequency. Obviously, this antenna is very high " $Q$ " and the bandwidth of antenna plus coupler is 6.7 kHz on 160 between the 1.2:1 VSWR points. Because of the narrow bandwidth, I provided for remote adjustment of the tuning capacitor in the coupling network with a 90 -volt $60-\mathrm{Hz}$ selsyn pair. The complete coupler circuitry, a parallel tank circuit consisting of L1 and C1 in series with C3 which resonates at the desired frequency, is shown in fig. 4. The tank is inductively coupled to the series circuit L2 and C2 into which the 50 -ohm coax feedline terminates. ${ }^{7}$ Not shown in fig. 4 is a relay switching arrangement whereby L1 is tapped down and the value of C 2 is decreased to provide for a wider total tuning range on 160 . The interior view of the coupler housing in fig. 5 shows the location of all the components. Remote adjustment of the coupler is obtained by having a selsyn drive the capacitor C1 via a reduction ratio chain drive which allows the use of a ten turn dial on the selsyn in the shack. The dial includes a sma!l chart that provides a quick dial versus frequency reference for setting.

The use of the C1-C3 series combination in the

fig. 4. Coupler provides match between high impedance seen at antenna terminals and 50 -ohm coax line.

fig. 5. The interior view of the coupler housing illustrates the precautions taken with component placement as a result of high voltages present.
coupler was dictated by the very high voltage developed at the base of the antenna at full legal power input. C3 is a $100 \mathrm{pF}, 20,000$-volt fixed vacuum capacitor that receives most of the voltage across the tank because C1 is varied from its full capacity of 1000 pF to about 300 pF to cover the tuning range. This combination also provides some degree of bandspread, helpful in view of the sharpness of tuning. I would suggest that you use high quality insulation, and plenty of it, both at the coupler and diamond loop ends of the antenna. With the impedance ranges involved, the voltages are awesome at all but the lowest power input.

## adjusting loop to resonance

Once you've assembled the antenna and set it in place, the next step is the adjustment of the length of the diamond loop to achieve resonance. It is assum-
ed that you will have set the overall length to a halfwave according to the usual equation; $468 / \mathrm{f}_{\mathrm{MHz}}$. For 1850 kHz this figures out to 252.97 feet ( 77.11 meters). There are a variety of ways to determine whether resonance has been achieved, ranging from loosely coupling a grid dip oscillator to the bottom of the vertical radiator to using an accurate RF impedance bridge, which was the method I used (see fig. 6). Another method that is quite easy to use is to resonate the tank circuit in the coupler using a GDO to your desired frequency without having it connected to the antenna. Then attach the antenna temporarily about halfway up the tank inductor from ground. If the antenna is resonant at that frequency, the tank circuit will still resonate with the GDO at the same setting. If not, as almost always is the case, you will have to adjust the GDO to find the dip again. Then try a different diamond loop length and go through the process once more. By noting the movement of the dip, you can easily tell if the antenna length adjustment was made in the right direction. By successive tries you'll find a length for the diamond loop that will closely approximate resonance. The antenna is then connected to the hot end of the tank circuit for adjustment of the VSWR and operation.

It is well to note that the above antenna pruning method can also be used to determine the harmonic resonance by setting up a temporary parallel tuned circuit that will resonate on the harmonic. If this antenna is to be used on both 160 and 80 , or 80 and 40 , you may wish to choose resonant frequencies that cover the band segments of interest. As shown in fig. 2, my antenna has its primary resonance at about 1854

fig. 6. W6US determines the verticals resistive and reactive components with a General Radio GR1606A RF bridge.
kHz . Testing has shown its second harmonic to be close to 3949 kHz .

If you are seriously interested in this type of groundindependent antenna, I would suggest some reading in books and articles that deal with VLF antenna systems. ${ }^{8}$ Some of the earlier systems closely parallel the dimensions of the antenna described here. I would also be interested to learn of your experiences with the W6US antenna on other bands - for example, on 10 meters, where the vertical radiator would be a magnificent 4.32 feet ( 1.32 meters) high and the total span about 11.88 feet ( 3.62 meters)! Also left to your experimentation is the question of whether the addition of a conventional radial system might enhance this antenna for DX.

The sticky point in this investigation is probably whether the raising of the current maximum by the ground independent approach lessens the need for radials to lower the angle of radiation. The Bobtail does not seem to profit by them, but here the vertical radiator is only half as long. At least it seems well established that the increased efficiency goes a long way toward successful long-haul DX.

## testimonial

No antenna article is complete without a relatively rosy exposition of the superlative reports received and the choice DX worked. To maintain tradition, I will therefore note that compared with a great variety of 160-meter systems previously used, this W6US ground independent system has been a real winner for me. A substantial number of solid QSOs have been logged with stations 500 miles or more distant while running just 10 watts transmitter output on SSB. Believing that more of a good thing is even better, I am presently working on a second version of this antenna. I sincerely hope that those who try this approach will provide still more data to benefit us all.

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 Wide Range of Transmitting and Receiving: Morse Code transmitting speed can be set from
the keyboard at any rate between $5-100$ WPM (every word per munute). AUTOTRACK on receive. For communication in Baudot and ASCII Codes, rate is variable by a keyboard instruction between 12-300 Baud when using RTTY Modem and between 12-600 Baud when using TTL level. The variable speed feature makes the unit ideal for amateur, business and commercial use.
Pre-load Function: The buffer memory can store the messages written from the keyboard instead of sending them immediately. The stored messages can be sent with a keyboard command.
"RUB-OUT" Function: You can correct mistakes while writing messages in the buffer memory. Misspellings can also be erased while the information is still in the buffer memory.
Automatic CR/LF: While transmitting, CR/LF automatically sent every 64,72 or 80 characters.
WORD MODE operation: Characters can be transmitted by word groupings, not every character, from the buffer memory with keyboard instruction.
LINE MODE operation: Characters can be transmitted by line groupings from the buffer memory.
WORD-WRAP-AROUND operation: In receive mode, WORD-WRAP-AROUND prevents the last word of the line from splitting in two and makes the screen easily read.
"ECHO" Function: With a keyboard instruction, received data can be read and sent out at the same time. This function enables a cassette tape recorder to be used as a back-up memory, and a system can be created just like telex which uses paper tape.
Cursor Control Function: Full cursor control (up/down, left/right) is available from the keyboard. Test Message Function: "RY" and
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MARK-AND-BREAK (SPACE-AND-BREAK) System: Either mark or space tone can be used to copy RTTY.
Variable CW weights: For CW transmission, weights (ratio of dot to dash) can be changed within the limits of 1:3-1:6.
Audio Monitor Circuit: A built-in audio monitor circuit with an automatic transmit/receive switch enables checking of the transmitting and receiving state. In receive mode, it is possible to check the output of the mark filter, the space filter and AGC amplifier prior to the filters. CW Practice Function: The unit reads data from the hand key and displays the characters on the screen. CW keying output circuit works according to the key operation. CW Random Generator: Output of CW random signal can be used as CW reading practice. Bargraph LED Meter for Tuning: Tuning of CW and RTTY is very easy with the bargraph LED meter. In addition, provision has been made for attachment of an oscilloscope to aid tuning. Built-in AC/DC: Power supply is switchable as required; $100-120 \mathrm{VAC}$;
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# xtended/expanded power dividers 

> Try copper water pipe, hobby-shop brass tubing for quality RF components

In weak signal VHF/UHF work (EME and various scatter modes)* nothing can be more frustrating than the inability to read faint signals you know are present but are largely obscured by noise. $\dagger$ The problem is often solved by increasing the size and/or number of antennas; when properly combined in a low loss system, doubling the number of antennas will yield very close to the theoretical 3 dB gain. But there is little to be gained in capturing a weak signal unless it is nurtured with great care on its way to the preamplifier. To do this, one should use the best quality feedline, cut as short as possible, to the power dividers. Ideally, the power dividers should be constructed to facilitate the use of short lines; unfortunately, most are either $1 / 4$ or $1 / 2$ wavelength long, as illustrated in fig. 1. With stacking distances between antennas as great as two wavelengths, these dividers do not permit the use of short feedlines.

## theory

While most readers are probably familiar with the power divider basics, this section has been included for the benefit of those who may not be, and for the further purpose of showing the evolution of extended power dividers.

Power dividers use the " $Q$ " section used as a means of matching the load of more than one antenna to the

[^8]feedline. A quarter wavelength of feedline will match the impedance of feedlines of the same type (coaxial or parallel) but having different impedances when the impedance of the matching section is: $Z=\sqrt{Z_{1} Z_{2}}$ and is known as a " $Q$ " section. (This discussion is limited to coaxial feedlines; all loads are assumed to be equal.)

When two or more loads, in the form of antennas or other power dividers, are fed from one transmission line, they appear to be in parallel. Four 50 -ohm loads represent a combined load of 12.5 ohms. In order to arrive at the impedance of the matching section we divide the impedance of one load by the number of loads, and this becomes Z 1 . Z 2 will be the impedance of the input feedline. If the matching section is to be divided into two or more branches, as shown in fig. 1B, then its impedance should be multiplied by the number of branches so that the combined value is the originally calculated impedance.

## design

The power divider shown in fig. 2 is a combination of the two types of dividers shown in fig. 1. The center portion of fig. 2, section $A$, is a $1 / 2$-wave power divider or matching section that matches the input impedance to the impedance of the two B sections. In theory, section B could be any impedance that would fit into the overall design, but as a practical matter it should be close in value to the output impedance. The two $C$ sections at each end are $1 / 4$ wave dividers that match section B to the two output ports at each end. I am presently using two of these in my 144 MHz EME array and have been more than satisfied with their performance.
A different method of accomplishing the same thing is shown in the power divider illustrated in fig. 3. Simpler in design, and easier to construct, this one

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fig. 1. Forms of conventional power dividers. (A) $1 / 4$ wave power divider, and (B) 1/2 wave power divider.
should perform equally as well as the others. At each end of a $1 / 2$ wave four-way power divider, the impedance is one-half the impedance of each output port. This will be 25 ohms for 50 ohm feedline or 37.5 ohms for 75 ohms feedline. We simply extend the matching section, at each end equally, to the desired length, at the impedance of $Z_{O U T} / 2$. (I will be using this design in my 432 MHz EME array now under construction.)

## common materials are all that's needed

I use copper water pipe, straight and hard drawn, for the outer conductor of my power dividers. It is available in three wall thicknesses for each nominal diameter: type K, thick wall: L, medium wall; and M, thinwall. Table 1 shows the nominal size, O.D., and I.D. of copper pipe in sizes from $1 / 2$ inch ( 12.7 mm ) through 1-1/2 inch ( 38.1 mm ). For the center conductor, I use brass tubing, available in hobby shops, in diameter increments of $1 / 32$ inch ( 0.8 mm ) from 1/16 inch ( 1.6 mm ) through $21 / 32$ inch ( 17 mm ), having a wall thickness of 0.014 inch ( 0.36 mm ) and sold in lengths of 1 foot ( 30 cm ) or 3 feet ( 91 cm ). It is easily spliced by soldering a short section of the next smaller diameter as an internal sleeve.

Square aluminum tubing is also good for the outer conductor, but I haven't been able to find it in lengths greater than 8 feet ( 2.4 meters), which isn't long enough for widely spaced 2-meter arrays, though it is easy to work with. Coaxial cable connectors can be held in place with small sheet metal screws, or the tubing may be drilled and tapped.

fig. A2. The "One Hundred OHM" 4-way 50 -ohm power divider.

## good performance requires careful construction

In layout, measurement and assembly, accuracy and uniformity are essential. After first determining the desired overall length, find and mark the exact center of the outer conductor, making a very light cut around the circumference with a tubing cutter. At points equidistant from the center, and $3 / 4$ inch ( 19 mm ) from each end, make a similar mark. These are the points at which the connectors or sleeves will be located, as well as the center and each end of the center conductor. Drill holes 180 degrees apart, on opposite sides of each end of the outer conductor, and one at the center, to accept the coaxial cable, connectors or sleeves. The center hole should be either in line with two end holes on one side, or at 90 degrees, depending on the orientation of your feedline. A 3/8 inch $(9.5 \mathrm{~mm})$ hole is drilled to one side of the center hole, just close enough that it will not run out and overlap the center hole. This is for the purpose of being able to have access for soldering the center conductor to the coaxial connector.

In preparing the different sections of the center conductor, the smaller diameter piece should be long enough for about a 3 inch ( 76.2 mm ) overlap into the larger size tubing to which it is to be joined. A reducing sleeve is made by telescoping together short sections of brass tubing, about 3 inches ( 76.2 mm ) long, so as to fill the space between the smaller and larger pieces
to be joined, and to keep them straight and concentric. If the center conductor is to be made in one piece, insulating spacer washers should be put in place before the sections are soldered together.

I use teflon spacer washers* to prevent sag in the center conductor and to maintain concentricity. These are placed on the smaller diameter portion at each point of change in diameter, at the center and on each end. The spacers should fit tightly on the center conductor and loosely in the outer conductor. My center conductors were assembled in two pieces divided at the center. This permits setting the spacers in place on the smaller diameter portions after the soldering is done. They are joined in the center with an internal sleeve after being inserted in the outer conductor. The center conductor should be cleaned and polished after assembly and handled with paper towels or tissue during insertion in the outer conductor. If the inside of the outer conductor is not bright and shiny it should likewise be polished. A small notch or "Vee" should be cut out of each teflon spacer, at the perimeter, to permit the flow of air through the power divider; this is important to prevent the accumulation of moisture.

After inserting the center conductor into the outer conductor, the coaxial connectors are ready to be installed. I recommend the use of UG-58/U connectors with teflon insulators. (Other types of insulation will not withstand the heat generated during the soldering process.) The flange of the UG-58/U should be removed - with a lathe, grinder, or otherwise - to facilitate soldering. A 7/16 inch hole in the outer conductor will provide a neat fit for the portion of the UG-58/U below the flange.

I use coaxial connectors only at the center or input port. At the output ports, I use copper sleeve couplers sized to fit $3 / 8$-inch ( 9.5 mm ) copper pipe. They are about 0.502 inch ( 12.75 mm ) I.D. and provide a very good fit for the shield of the RG-331 hardline leads to the antennas. The sleeves are tinned on the inside. A small stainless steel wormscrew hose clamp is put around the sleeve after the hardline is installed.

After all soldering, assembly, and installation have
table 1. Nominal size, O.D. and I.D. of different grades of copper water pipe.

| nominal <br> size | O.D. <br> (inches) <br> (inches) | K <br> (inches) | I.D. type <br> (inches) | $\mathbf{M}$ <br> (inches) |
| :---: | :---: | :---: | :---: | :---: |
| $1 / 2$ | 0.625 | 0.527 | 0.545 | 0.569 |
| $5 / 8$ | 0.750 | 0.652 | 0.666 | 0.690 |
| $3 / 4$ | 0.875 | 0.745 | 0.785 | 0.811 |
| 1 | 1.125 | 0.995 | 1.025 | 1.055 |
| $1-1 / 4$ | 1.375 | 1.245 | 1.265 | 1.291 |
| $1-1 / 2$ | 1.625 | 1.481 | 1.505 | 1.527 |

[^9]
fig. 2. Long power divider.

fig. 3. Another form of long power divider.
been done, the ends and the center access hole should be sealed. It is not necessary to solder the coverings in place, but they should be held in place with a good sealant and wrapped tightly with stretch tape. All points of possible moisture entry - even the solder joints - should likewise be sealed.

The dimensions given in fig. 2 will yield impedances very close to the calculated ideal. Preliminary calculations indicate that $3 / 4$ inch ( 19 mm ) type $M$ tubing would be a better choice for outer conductor in the fig. 3 design, using brass tubing for the center conductor.

## what to expect

It is said that 1 dB is the least amount of change in sound that can be detected by the human ear. In a noise-free environment, this is probably correct. But in EME work, I question its accuracy. Often we can detect a change in the pitch of the "white noise" as we tune our receivers across a given frequency. Even though there's a signal present, the dits cannot be distinguished from the dahs. Perhaps if this were 0.9 dB , the signal would jump right out of the noise and be readable if we could supply the additional 0.1 dB ? The low-loss feed system described herein may make such a thing possible.

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appendix
other designs for power dividers
In each of the power dividers previously described, a "Q" section is employed at the input port. This is not necessary in all cases. The input may be split into two branches, each of which is twice the impedance of the input feedline, with no resulting mismatch. The " $Q$ " sections may be placed at each end, in either $1 / 4$ or $1 / 2$ wave form.
Figures A1 and A2 illustrate this design in each of these forms. I have designated the first device as a "splitter" to distinguish it from the one in fig. 3. This design is not suitable for a 75 -ohm feed system, which would require splitting into 150 -ohm branches. The $\mathrm{D} / \mathrm{d}$ ratio for 150 ohms would be 12.2, resulting in a center conductor much too small to be practical.
The "hundred OHM" (fig. A2) divider is particularly appealing to me, because it involves no change in diameter of the center conductor. The idea for this one occurred to me about a month ago, and I hastily assembled two of them for my 2 -meter EME antenna ( $8 \times 2.2$ wavelength NBS Yagis). Initial results are very encouraging: SWR is very good, and my own SSB echoes from the moon were readable with a sky temperature of about 400 degrees K . (Below 300 degrees $K$ is considered "quiet sky.")

## construction details for the

"hundred OHM" divider
Outer conductor: $3 / 4$ inch ( 19 mm ) copper pipe, type D, 0.833 inch ( 21.2 mm ) I.D., if available. Type $\mathrm{M}, 0.811$ inch $(21.2 \mathrm{~mm})$ I.D., is satisfactory substitute.
Inner conductor: $5 / 32$ inch ( 4 mm ) brazing rod or brass tubing. Tubing is preferred because of its usefulness as internal coupling sleeves.
Center and end Tee's: $3 / 4$ inch ( 19 mm ) copper plumbing Tee's.
Center conductor splices: $5 / 32$ inch ( 4 mm ) I.D. brass tube. Miniature Tee's fabricated from same material at each end. Il used brazing rod center conductor.)
Coax connectors: UG-58 with tefion insulation, flanges turned to fit pipe, soldered.
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## the weekender

simple, compact QRP keyer

I recently built a QRP CW transceiver and decided to use one small cabinet to house the radio, rechargeable batteries, and a keyer. After completing the transceiver and squeezing in the batteries I found I had left myself less than two square inches of board space for the keyer circuitry.
Because contemporary electronic keyers use one or more ICs and quite a few additional components, I needed to find a simpler, more compact approach. I also wanted self-completing characters and very low battery drain. Dot and/or word memory and digital precision were features I could do without in this application.

The circuit that evolved, shown in fig. 1, does the job very nicely, fits easily on 1.5 square inches of board space, and consumes less than 4 mA , key-down, at 12 VDC.

In lieu of the usual digital clock, this keyer uses one of the unijunction family of devices as the basic timing device. Unijunction devices (UJTs), which have been around almost as long as the basic transistor, have several unique characteristics that make them quite different from those of the conventional twojunction transistor. These features include stable triggering voltage, very low value of firing current, high pulse current capability, and low cost.
The circuit (fig. 1) uses these characteristics of the UJT to generate a precisely timed sawtooth waveform. This is formed by the exponential voltage build-up across capacitor C 1 , and the abrupt discharge of this voltage when the UJT "fires," or triggers. Dashes and dots are self-completing because the UJT has no effect on the capacitor charge until the triggering point is reached. Potentiometer R2 controls the rate of charge of Cl - hence the keying speed. R1 sets the ratio for the generation of dots.
The sawtooth waveform is applied to a PNP transistor, Q2, where it is shaped and amplified. The output

By Jack Najork, W5FG, 3728 East 85th Place, Tulsa, Oklahoma 74136

fig. 1. Simple QRP keyer uses unijunction transistor for timing.
of $Q 2$ is direct-coupled to $Q 3$, the switching or keying transistor. R3, the "weight" potentiometer in the emitter of O2, controls the switching threshold (the onoff periods) of Q2 and Q3.

I use the collector of Q3 (which goes to ground when the key is down) to key the emitter of the transmitter driver transistor that draws about 20 mA . You can, of course, key any circuit that requires ground to transmit provided you stay within the current and voltage capabilities of Q3.

A relay with a DC coil resistance of 500 to 3000 ohms can be used in the collector of 03. The relay coil is connected between the collector of O and +12 VDC as shown in fig. 2. This arrangement will increase the current drawn by the keyer another 5 to 25 mA , depending on the relay coil DC resistance. Reed relays are recommended and work well for keying small, noninductive current loads. An inductive load such as an iron-core choke in series with the keying lead will generate an inductive charge. If not damped, this charge will quickly weld together the contacts of the reed relay.

## limitations

The limitations of simple circuits such as this are often overlooked or glossed over by enthusiastic authors, with resultant heavy mail and telephone traffic to the publication and/or author. To minimize such communication, let me say that this simple keyer will work very well if the following precautions are taken.

First and most importantly, the DC supply voltage must be constant (either through regulation or a stable source) because the timing of the sawtooth generator as well as the switching thresholds of Q 2 and Q 3 are a direct function of the supply voltage. Poor voltage

fig. 2. Reed relay can be driven by $\mathbf{Q} 3$ for keying circuit isolation.

fig. 3. Decoupler circuit helps to reduce AC power supply ripple from DC line.
regulation will cause erratic characters. Long-term changes in supply voltage from, for example, 12 volts to 10 volts, will drastically affect the weight of the characters, and to a lesser extent, the speed. The keyer will work well with supply voltages of 9 to 15 volts. Once the operating voltage is selected it must remain at that value; if it does not, all controls will require re-adjustment.

I use heavy duty batteries to avoid these problems. If an AC supply is used, the simple regulator-decoupler shown in fig. 3 does a good job of cleaning up the supply voltage source.

With the possible exception of C1 and 02 , component tolerances are not critical. C1 must be 2.2 microfarads. $(1 \mu \mathrm{~F}$ is too small and $3.3 \mu \mathrm{~F}$ is too large.) Q 2 should have a fairly high beta - at least 60 or 70 so either avoid the unknown junk-box types entirely or use a socket and make sure your choice works properly. The 2N6027s appear to be non-critical. All six of mine, from two different manufacturers, worked well with no noticeable variation in the characteristics needed for this application.

Finally, if a relay is used, try to use a reed type or one with a short, snappy armature throw. The keying waveform coming out of Q 3 is more triangular than rectangular. A sloppy relay will generate satisfactory dashes but skimpy dots, and you won't be able to compensate for this with the "weight" or "ratio" controls.
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# applied Yagi antenna design part 6: 

 the model and a special teaching tool
## Understanding and using the FORTRAN

## program

In this concluding article, the FORTRAN code used in the model is discussed on terms of its organization and logic flow, and an interesting teaching example also presented.

A copy of the program is available from ham radio (send an SASE with 37¢ postage). Please note that the program, designed to run on a mainframe computer, requires a FORTRAN 77 compiler or its equivalent. While a knowledgeable programmer can convert this program to BASIC, an understanding of the "architectural" differences between FORTRAN and BASIC is essential, as is familiarity with the use of both radians and degrees, as well as the rules of complex (vector quantity) arithmetic. A careful rereading of the first two articles in Lawson's series ${ }^{1,2}$ is also recommended.

## FORTRAN program structure

The program consists of seven logical parts, as depicted in fig. 1. The Driver contains array definitions, constant declarations, and the control logic for the five main subroutines. Each subroutine's name is an accurate description of what it does. The mathematics library contains the functions used in computing impedance components. The model's code has been carefully written to minimize execution time.

[^11]This is especially true for the reactance calculations because they can be executed tens of thousands of times in a single session of Yagi iterations.

The Driver contains the Poynting vectors necessary for pattern calculations. These vectors are listed as constants in an extended DATA statement. As the vector values for the second 90 degrees follow from those of the first 90 degrees, a DO loop makes this assignment. This same loop adjusts the vector values slightly so a dipole has a calculated gain of 2.14 dBi . Further manipulation of the 0.997 multiplier leads to degraded pattern calculations. This is followed by calculation of the dipole pattern constants for each of 180 degrees. All of the Driver code to this point is executed only once - at the start of the initial run. Now the five subroutines can be called to calculate Yagi performance parameters. If a series of iterations similar to those in the first five parts of this series is desired, the nested DO loops begin at this point.
For those articles a primary loop was used to iterate reflector length. A secondary loop iterated director length within each discrete reflector measurement. For tapered directors a tertiary loop was used to apply the tapering constant to the second and subsequent directors. By definition, the first director cannot be tapered. If spacing is to be iterated, the loops for spacing can also be placed here, either in place of the length loops, or within them. When a frequency scan of a specific Yagi design is desired, element length, spacing and diameter are set as constants, and a frequency DO loop is coded. Element diameter (ELDIAM) is usually a constant, but this parameter can also be iterated.

GETDATA originally served to prompt for and accept the individual Yagi design approach parameters. After obtaining calculations for the Yagis in use at WB3BGU, the decision was made to write this six-part

fig. 1. Internal organization of the Yagi analysis program.

fig. 2. E-plane plot of the NBS 4.2 wavelength Yagi.
series of articles. Hence the need arose for either massive amounts of data input or the nested DO loops described above. This routine then became the place where ELDIAM, frequency (FREQ), and element spacing (ELSPACE) from the reflector were defined at each run's start. In the version provided, this routine sets the design parameters for the NBS family of Yagis. Experience indicates that most of the errors leading to erroneous output from the iterations can be traced to typos made in this routine. The importance of "sanity checks" on how a Yagi's design approach is described to the model cannot be overstated. Until ex-
perience is gained in working with the model, the user should consider printing the design parameters before the iterations begin.

IMPEDANCE calculates the self and mutual impedances among the Yagi's elements. The self-resistance of all elements is assumed to be 73 ohms, and the selfreactances are calculated from Lawson's approximations. The self-impedance of the driven element needs to be $73+j 0$ for best results. While the third article in this series was being prepared, it became obvious that this constant could be assigned to the driven element, eliminating the need for calculating its zero reactance length to 0.000001 inch. Hence the second element's self-impedance is set to $73+j 0$ ohms. If another element is to serve as the driven element, the user has to change the test made on index J. Mutual impedances are calculated in the manner stated by Lawson, using the Kraus formulas. ${ }^{3}$ Instead of Kraus' power series or Lawson's less-than accurate approximations, the Sine and Cosine integral routines from the IONCAP program are used. They are also three orders of magnitude faster than either of the other methods. IMPEDANCE also makes good use of the fact that the mutual impedance between elements i and $j$ is the same as between elements $j$ and $i$, and calculates this value only once while storing it in both matrix locations. DO loop indices $I$ and $J$ have an unusual implicit relationship that allows for reducing the number of calculations in a manner proportional to the number of Yagi elements.

SOLVE provides the complex current solutions for each Yagi element. It is basically a routine that solves simultaneous linear equations. An array with one more column than number of rows is necessary because this extra column contains the solved complex current values. The second element is assumed to be the driven element and is driven with $10+i 0$ volts. If as was described before, a different element is to be the driven element (or in the case of multiple driven elements), the user has to make the appropriate modifications. It is also possible to obtain exactly the same gain and F/B results with any other driven element voltage value, provided that zero phase is used. Because a digital computer is being used, an assumption has to be made for the value of "digital zero;" this is the value used to test the complex matrix members for being equal to zero. This routine uses 0.00001 for this value. Smaller values may increase the number of iterations necessary for solving the matrix and not add anything measurable to the calculated gain and F/B. Up to this point the FORTRAN routines can be assumed to execute instantaneously. This was found to be true for Yagis with up to 20 elements. The two subroutines that follow consume the vast majority of the time necessary for a given Yagi's iterations.

fig. 3. E-plane plot of the NBS 4.2 wavelength Yagi with an additional 0.424 wavelength-long director spaced 0.37 wavelengths from the reflector.

They contain multiple sets of nested loops that iterate each of 180 degrees within each Yagi element, or vice versa.

GAIN converts the complex current solutions in the matrix to complex voltages whose phase is in radians. A test is made for elements with zero current because they cause ATAN2 to fail. They also represent Yagis whose performance levels are undesirable. These Yagis are labelled as such and no further processing takes place. Yagi gain is calculated as a summation of each element's contribution in the forward (zero degree) direction as well as through the Poynting vectors. These values are saved for use during pattern generation and F/B calculation.

CARTPLOT calculates the F/B and either the E-plane or H-plane pattern. These patterns are then printed as normalized Cartesian plots. While coded to print only the E-plane pattern, the H-plane parameters are still computed. The user can adjust this routine to print either plane. The 180 -degree intermediate values from the gain calculations are used with the dipole pattern to produce the E or H -plane plots, and to calculate $F / B$. If only the gain and $F / B$ values are wanted ( $\mathrm{PLOTKEY}=0.0$ ), a single line of output results. If a plot is wanted with full information on the Yagi Isee

fig. 4. E-plane plot of the NBS 4.2 wavelength Yagi with an additional 0.430 wavelength-long director spaced 0.36 wavelengths from the reflector.
the plots in any of the previous parts of this series), PLOTKEY is set to any non-zero value before calling CARTPLOT. Every second degree is plotted, and dB values are from zero to 60 dB . Values in excess of 60 dB are shown as 60 dB . To reliably print this many lines per page, hands-on control of the printer is almost a necessity. The user may want to change the code so the maximum dB value is 55 dB . Nulls of this magnitude are rarely achieved in practice, and are of informational value at best. To signify "off-page" values, the user may also want to change the code to print asterisks, periods, or some other symbol when these values are calculated. Because a line printer is a discrete device in terms of being able to print only in (many) fixed positions on the page, calculated dB values are rounded to the nearest integer value. The use of a pen plotter would circumvent this problem. It is also possible to use some sort of periodicity to emphasize small changes between predetermined dB values.

The MATH LIBRARY'S four functions are used by IMPEDANCE to calculate the mutual impedances. The resistive component is calculated by RMUT, and the reactive component by XMUT. SI and Cl are the sine integral and cosine integral routines, respectively, from IONCAP. An IF statement has been added to Cl to

fig. 5. E-plane plot of the NBS 4.2 wavelength Yagi with an additional 0.435 wavelength-long director spaced 0.36 wavelengths from the reflector.
protect against an attempt to compute the LOG of zero. This will cause a software failure, and a small value is substituted for the zero. In actual practice a zero value cannot occur, but a simple precaution is easily taken. As with any program of this complexity, an example is in order. The 4.2 wavelength ( 15 element) NBS Yagi will serve as the teaching tool. In this example the model will be used to apply a long Yagi technique to this Yagi in an attempt to increase the calculated gain.

## further optimizing the NBS 4.2 wavelength Yagi

Long Yagi techniques include placing one or more directors between the driven element and the first of the wide spaced directors. Up to this point the first of the wide spaced directors was the first director. Depending on the design approach used to implement long Yagi techniques, this same director may become the second, third, or even the fourth director. The Tilton/Greenblum Yagis, and to a greater extent the Knadle and Kmosko-Johnson Yagis that were examined earlier in this series, typify what is meant by long Yagi techniques. This new director (or directors) is generally believed to increase the Yagi's gain on what

fig. 6. E-plane plot of the NBS 4.2 wavelength Yagi with an additional 0.440 wavelength-long director spaced 0.35 wavelengths from the reflector.
is substantially the same boomlength as before. This belief was shown to be true as a result of comparing computer-iterated Yagis that employed long Yagi techniques with the equal director spaced NBS Yagis of similar boom length. ${ }^{4,5,6.7}$

To accommodate an extra director and the spacing iterations to be done only for this director, the DRIVER code has to be slightly modified. The DO statement before the calls to the five subroutines is eliminated, but the associated CONTINUE is kept. GETDATA is called as before, but the NBS parameter is replaced with the integer constant 15 . Code is now inserted to read the new director's length in wavelengths, and this is converted to a physical measurement at 400.0 MHz . A DO statement is now inserted to control the execution of the remaining subroutines. Its indices will serve to move the new director (element 16) between the driven element and element 3 , the old first director. The driven element is 0.2 wavelengths from the reflector, and the old first director is 0.508 wavelengths from the reflector. A range of 0.21 to 0.45 wavelengths from the reflector for the extra director was selected and coded as follows:

$$
\begin{aligned}
& \text { DO } 97 N=21,45 \\
& \text { ELSPACE } 16 \text { ) }=\text { FLOAT }(N) / 100.0
\end{aligned}
$$



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table 1. A comparison between the original NBS 4.2 wavelength Yagi's calculated performance parameters and the gain maximas for a series of similar Yagis with a director added as indicated.

| length of additional <br> director $(\lambda)$ | spacing of additional <br> director from reflector $(\lambda)$ | Gain <br> $(d B i)$ | F/B <br> $(\mathrm{dB})$ |
| :---: | :---: | :---: | :---: |
| - | - | 15.70 | 19.26 |
| 0.424 | 0.37 | 16.14 | 18.87 |
| 0.430 | 0.36 | 16.15 | 19.52 |
| 0.435 | 0.36 | 16.16 | 19.01 |
| 0.440 | 0.35 | 16.16 | 19.70 |
| 0.445 | 0.35 | 16.16 | 18.95 |
| 0.450 | 0.34 | 16.15 | 19.44 |
| 0.455 | 0.34 | 16.14 | 18.28 |
| 0.460 | 0.33 | 16.10 | 18.29 |


fig. 7. E-plane plot of the NBS 4.2 wavelength Yagi with an additional 0.445 wavelength-long director spaced 0.35 wavelengths from the reflector.

The remaining subroutines are called as before, but their NBS parameters are all replaced with the integer constant 16. The DO loop index should be printed during each iteration so as to identify the particulars for each line of gain and F/B calculations.

A summary of the test results of selected iterations is presented in table 1 . Up to 0.46 dB of additional calculated gain is available by applying long Yagi techniques to this NBS Yagi. This is a significant part of the claimed 0.75 dB gain from the use of the NBS trigonal reflector, and without the additional elements

fig. 8. E-plane plot of the NBS 4.2 wavelength Yagi with an additional 0.450 wavelength-long director spaced 0.34 wavelengths from the reflector.
on each side of the boom's plane and the attendant extra hardware. ${ }^{8}$ Figs. 2 through 10 contain E-plane plots for each Yagi summarized in table 1. While the increased forward gain is difficult to detect in the width of the main lobe, the main lobe's sharper definition through a deeper null and the reduction of many side lobe amplitudes, are visible. The calculated $F / B$ ratios are more or less similar to that of the original Yagi and to each other. Table 1 also indicates that as directors are moved closer to the driven element, they tend to become longer for optimal results. The new director

fig. 9. E-plane plot of the NBS 4.2 wavelength Yagi with an additional 0.455 wavelength-long director spaced 0.34 wavelengths from the reflector.
lengths used in these iterations begin with the length for the first director specified by NBS, and proceed in regular increments. Beyond 0.46 wavelength, Yagi performance deteriorates rapidly. With only one exception, the application of this long Yagi technique to the other NBS Yagis resulted in reduced gain. That exception produced an increase of 0.02 dB . The more experimentally inclined reader may want to iterate the model for the 4.2 wavelength Yagi with a second or even a third additional director.

## conclusion

This six-part series has applied and made available a computer model for Yagi antenna design and analysis. Various Yagi design approaches were explored in terms of gain, F/B, and overall pattern, with preferable designs being selected for each band from 50 MHz to 432 MHz . The antenna is the most important part of a VHF/UHF station, and the careful selection of an antenna that is also well matched to a lowloss feedline is the single greatest step a Radio Amateur can take toward effective VHF/UHF communications. The Yagi antenna remains the most effective antenna in terms of achievable gain and minimum size. While the cost of transceivers, transverters, amplifiers, and pre-amplifiers continues

fig. 10. E-plane plot of the NBS 4.2 wavelength Yagi with an additional 0.460 wavelength-long director spaced 0.34 wavelengths from the reflector.
to increase, very effective long Yagis can be constructed for comparatively little. This series has served to enable the VHF/UHF Radio Amateur to design that antenna with reasonable precision and with an accurate indication of how well that antenna will perform. VHF/UHF weak signal operators are basically experimenters, and it is with great interest that I look forward to future issues of ham radio to read the results of the experimental Yagi designs that other Amateurs produce with this model.

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## solar cycle review/preview

A review of the past six months and a preview of the next few months of the 11 -year sunspot cycle (SSN) of solar activity should be useful in forecasting propagation conditions.

The earth's geomagentic field is affected by particle influx from the sun, which in turn depends on the level of solar activity. The sun's output, expressed in flux or SSN, affects both the amount of signal absorption (and consequently the LUF, or lowest usable frequency) and the highest band we can use (the MUF or maximum usable frequency). There is a relationship between variations in signal levels (QSB) and this particle influx.

How will the signal parameters LUF, MUF, and OSB change in relation to the solar cycle by next spring? The solar flux decreased from a maximum last spring to a minimum value in August - not an unusual solar trend for most years. This year's maximum, however, was larger than most annual increases that normally occur in the winter-spring period. In addition, this spring an inflection point (increase) occurred in the recorded values of SSN two thirds of the way down from the maximum. The coincidence of the two produced an SSN level of 80 (flux 128) for the period, (February through May, 1984) about 20 SSN's above normal. This meant that MUF's were about 6 to 7 MHz higher than usual on midlatitude propagation paths over the four-month period. Now at approximately SSN 32 we should be edging
up so that next spring another slight maximum of about 8 to 10 SSNs above the average base value of 36 (flux 87) will be realized. We will check on our SSN cycle status next spring.

What does this mean in terms of working DX over the next few months? The signal strength is expected to increase because of the seasonal affect during winter as the "sun moves south,' and the Northern hemisphere turns away from the sun. Not all of the signal increase is due to seasonal changes but also from the annual solar flux increase (the sun is closer to the earth) as well. At the same time, higher MUFs should provide more and longer openings on the higher frequency bands ( 10 and 15 meters) than at the present time. Particle influx into the polar regions are expected to be small from the minor solar flares, but may be significant from coronal hole activity, though these geomagnet-ic-ionospheric disturbance effects from the latter source are not intense, they are long - as long as 3 to 5 days. DX signals will probably exhibit fading (OSB) during these disturbed times. On the positive side the clouds of ionization moving around during the disturbance often focuses a weak DX signal from a new location right to you. These enhanced signals are usually from off-great-circle propagation paths and are short-lived in time. Be ready to take advantage of them and work them rapidly before the propagation mode quits.

## last-minute update

Equinox DX conditions should prevail for October. Expect conditions to rapidly change during this month. As a result of fewer hours of daylight, airmass thunderstorms changing to frontal passage types, midday higher frequency band long-skip replacing shortskip, and some geomagnetic disturbances will all have their effects on the ionosphere. This month the higher frequency bands, 10 to 30 meters, will be best the first and last weeks of the month during high solar flux periods. The two weeks in between will favor the lower frequencies and nighttime DXing. Geomagnetic-ionospheric disturbances may further affect operation on October 3, 8, 13, 18, 22, and 31.

The Orionid meteor shower will be visible from the 15 th to 24 th of October, with a maximum rate of between ten to twenty per hour on the 20th to 21st of the month. The moon is full on the 9 th and perigee occurs on the 23 rd.

## band-by-band summary

Ten meters will be open to the southeast for a short period before noon, to the south at noon, and to the southwest in the afternoon in local time. The openings will be longer and more frequent when the solar flux is at its 27-day cycle maximum. Even better transequatorial one-long-hop propagation will occur during disturbed periods. Tune in WWV at 18 minutes after the hour and note the geomagnetic field status announcement.

Fifteen and twenty meters, almost always open to some part of the world, will be the main daytime DX bands. Twenty should stay open on long southern paths into the night, while 15 will drop out in the late afternoon. Operate 15 first and move down to 20 meters. DX is 5000 to 7000 miles ( 8000 to $11,200 \mathrm{~km}$ ) on these bands and one-long-hop transequatorial propagation is also possible, even more often than on 10 meters.

Thirty and forty meters are both day and night bands. Intermediate distances ( 1000 to 1500 miles or 1500 to 2200 km ) in any direction represents

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## the beverage antenna

As old as the spark-gap and the Alexanderson alternator is the Beverage antenna. Even today it retains its popularity as a good, lownoise receiving antenna for 160 meters. Basically, the Beverage is a long wire (one to three wavelengths) suspended 10 to 15 feet above ground.

Its maximum received signal level is from stations collinear with the wire (fig. 1). The Beverage can be made unidirectional by placing a resistive termination at the far end of the wire toward the direction of interest. Front-to-back ratios as high as 20 dB can be achieved. The value of the resistor falls between 200 and 500 ohms, depen-

fig. 1. Single-wire, terminated Beverage antenna provides good results on 160 meters. Resistor $\mathbf{R}$ is adjusted for best front-to-back ratio.

fig. 2. Simple U-plate of bent aluminum couples potentiometer to kitchen timer. Start timer and check value of front-to-back ratio of Beverage antenna over a period of an hour.
ding upon the ground conductivity and the height of the wire above ground.

How does one determine the optimum value for this resistor? Bill Pfaff, K2GNC, has solved this problem with the device shown in fig. 2. His arrangement consists of a 500 -ohm carbon potentiometer attached to a 1-hour kitchen timer by means of a bent aluminum coupling plate. The receiver is tuned to a broadcast station at the high end of the band and located off the back of the Beverage antenna. The experimenter now plots received signal strength against time, as measured on the timer. All that's necessary is to coordinate timer readings with the position of the potentiometer when the $S$-meter reading is lowest. This indicates the proper resistance (as measured on an ohmmeter) for best front-to-back ratio. The potentiometer is then replaced with a fixed resistor of the proper value.

Bill recommends that this test be run during the season of the year in which the antenna is to be used the most (probably winter), because the value of optimum resistance changes with the condition of the soil.

## the K2GNC rotary ground plane antenna

Would I fool you? That's right - Bill also has a rotary ground plane. And if you don't believe me, just look at fig. 3. (Well, it's not exactly a ground plane, but I sure got your attention!)

The antenna is a modified 2 -element Yagi beam working against a quarterwave radial system. Quarter-wave elements are used as a radiator and a reflector, an idea developed by VK2ABC. In this design, both elements are grounded to the center of the radial system and the radiator is shunt-fed by a gamma matching system. The elements are mounted in the vertical plane at an angle of about 70 degrees to each other.

Bill has made $40,20,15$, and 10 meter versions of this simple beam. He reports it has good directivity but adds, of course, that he has no means of checking signal gain but says he gets good reports with it. The groundmounted 40 -meter version uses buried radials instead of ground-plane wires.

Standard 2-element beam dimensions, cut in half, are used in all antennas tested.

## the K2GNC 160-meter toploaded vertical

Still another interesting antenna concept from K2GNC is a 160 -meter antenna that uses the top loading system popularized by the British Marconi Company (fig. 4).
The vertical antenna consists of three sections of aluminum irrigation pipe, 4, 3, and 2 inches in diameter. Its overall height is 88 feet $\mathbf{~} 26.8$ meters).

Bill uses 130 radials, with an average length of 100 feet ( 30.4 meters), and a simple matching network to feed the antenna. The antenna works, as Bill's record of WAC and 115 countries to date on the "top band" proves!
(It's always a pleasure to hear about interesting antennas; I'll be looking forward to receiving more information from readers of this column.)

## the world according to JA

We're all familiar with the Great Circle Maps centered on the United States. But have you ever seen a Great Circle map with Japan as the center point? Look at fig. 5. Most of the countries that we consider "real DX" are within a single ionospheric hop of Japan. Such prefixes as UJ8, AP, XZ

fig. 3. The K2GNC "rotary ground plane." This interesting vertically polarized array consists of a $1 / 4$-wave driven element and reflector working against four $1 / 4$-wave radial ground wires. The driven element is fed with a gamma match. All elements are connected to the tower (or mast) at center point, as are the radial wires.

fig. 4. The K2GNC top-loaded vertical antenna for 160 meters. Flat-top currents essentially cancel and majority of radiation comes from 88 -foot vertical element. Antenna is base-fed at point $A$ via coaxial line and simple L-network. Spacing between wires is about a foot.
and other goodies are right in the back yard of the JA hams. On the other hand, their "tough" DX spots (on an over-the-pole shot) are such commonplace locations as VP2, HH, KV4, FY7 and the eastern tip of Brazil. Note, too, that South America runs from about 10 degrees west of North to 150 degrees south of North. And Africa is stretched out in a similar manner to the West of Japan. In Japan, as in the United States, "DX is where you find $\mathrm{it}^{\prime \prime}$.

## SSB voice quality

I've written in the past about the poor audio quality that seems to abound in SSB communication. Must this be so? Improved response in new microphones and auxiliary speakers tend to make voices sound a bit more realistic, but some sideband signals still seem very hard to tune for good voice quality.
Maybe there's more to this than meets the eye. Intrigued by what he

heard on the bands, Willie Sayer, WA6BAN, decided to run audio measurements on some of his SSB equipment. He did this by feeding the transmitter with an audio. signal generator and sweeping the audio spectrum as he measured the power output of the transmitter into a dummy load. The results of this simple test may show why some rigs sound different than others.

Fig. 6 shows the microphone-toantenna audio characteristics of an ICOM-730 run on upper sideband. Audio response is smooth with a passband of 2128 Hz between the -6 dB points of response. The audio oscillator is swept through the range and readings logged at the points indicated on the graph.

Fig. 7 shows an old Collins KWM-1 transceiver with a Collins F-455N-20 filter in it. The curve is run on upper sideband. The response shows a characteristic filter ripple of about plus or minus 1 dB , except for a dip in the curve at about 1500 Hz . Audio passband is 1842 Hz between the -6 dB points.

Fig. 8 shows a TS-830 with a FoxTango filter installed. The curve is run on upper sideband. The response shows a characteristic filter ripple of about plus or minus 1dB. Audio passband is 1992 Hz between the -6 dB points.

The interesting fact is that all of these transmitters sound pretty good on the air, even though the passband filters have several decibels of ripple in the audio passband. Does the IC-730 sound better on the air than the TS-830? It's hard to tell, unless exacting tests are run with the same voice, microphone, etc.

But I do know that a true audiophile would frown at a passband with even a fraction of a decibel of ripple in it!

It remains to be seen when passband filters having smoother in-band responses become available whether voice transmissions on the Amateur bands will sound more lifelike and realistic.

fig. 5. The DX world as viewed from Japan - Great Circle map centered on Tokyo. (Courtesy CQ-ham radio magazine.)

fig. 6. Passband of ICOM-730. Note smooth response with little or no cusps. Audio oscillator was swept over range of $200-2500 \mathrm{~Hz}$.

It's easy to examine the audio passband of your transmitter. The test setup of fig. 9 will do the job. Reduce transmitter power by 3 dB (half
power). This lets the equipment run cooler during testing and prevents the introduction of signal distortion that would invalidate the test results.

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## keying a linear amplifier with the TS-930

Ron Nail, K5HUI, ran into some problems when he tried to key a linear with his TS-930 Kenwood transceiver. Here's his story:
"When I bought my Kenwood TS-930 transceiver a few years ago, I was disappointed to find that it would not operate the antenna changeover relay in my linear amplifier. Kenwood's solution was to send me a reed relay, which 1 installed. However, using the relay produced annoying relay clicks and also introduced a slight time lag in an otherwise excellent full break-in system incorporated in the transceiver. In addition, arcing of the antenna relay contacts was observed.
"The solution to the keying problem (shown in fig. 10) was to install a solidstate relay that switches in microseconds instead of milliseconds, as does the reed relay. In addition, this scheme is absolutely quiet.
"The diode bridge eliminates polarity problems on the keying line and, with the optical isolation, the circuit performs in a normal fashion, with the ability to switch up to 120 VAC or 125 VDC without regard to polarity or ground.
"A pre-packaged diode bridge (or individual diodes) can be soldered directly to the solid-state relay pins. With double-sided tape, the little unit can be attached to the chassis side panel of the TS-930, underneath the autotuner. Keying for the amplifier is pin no. 7 of the remote connector and ground."

## VTR-RFI

"If you go into a contest for 48 hours and run an appreciable amount of power, you're going to meet your neighbors." That's the unhappy prediction of "Bip," W6BIP, after a deTVI session with a video tape recorder (VTR).
Bip has spent countless hours working on his (and his neighbors') VTRs, trying to prevent his signal from entering the units. He's almost succeeded.
Because of the nature of the beast, and the lack of internal shielding, the

fig. 7. Passband of Collins KWM-1 transceiver with F-455N-20 filter. Note the "notch" at about 1500 Hz .

fig. 8. Passband of TS-830 with Fox-Tango filter installed.

fig. 9. Test set-up used to run audio response curves of SSB transmitter. Audio signal is inserted in microphone jack.

fig. 10. The TS-930 keyer of K5HUI. (The solid-state relay K1 is made by OPTO 22, 15461 Springdale Street, Huntington Beach, California 92649.)

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fig. 11. The W6BIP solution to VTR-RFI: wrap coaxial line to antenna and power cords to VTR and TV set around $\mathbf{1 / 2}$-inch diameter ferrite rods. A suitable rod is the Amidon R33-050-400 or R33-050-750. Rods have a permeability of $\mathbf{8 0 0}$ (No. 33 material).

VTR provides serious RFI (radio frequency interference) problems, partiçularly during playback of a tape. Interference can be expected from transmitting equipment operating on any frequency, says Bip, but the problem is worst at the low end of 80 meters, which corresponds to video processing frequencies of the unit. Transmitter power as low as 3 watts can raise havoc in the 3.5 MHz region, although it takes upward of 100 watts to cause the same picture degradation when the transmitter is operated at 3.8 MHz . ${ }^{*}$

Bip sees the challenge and rues the fact that his transmitting antenna is quite near to the TV reception antenna. But what can you do when you live on a narrow city lot?

Bip solved his RFI problem on all bands except 80 meters; on that band he has to run reduced power. But he can now run full power on all other bands up to 30 MHz using the modification of his VTR installation shown in fig. 11.

In this modification the TV antenna feed is RG-59/U and the line is wrapped around a ferrite rod just before it enters a highpass filter and the VTR. The power cable to the VTR is wrapped around a second ferrite rod.

The same procedures are used at the TV receiver end. The coaxial lead between the VTR and TV set is wrapped around a ferrite rod and a second highpass filter is installed at the TV set, as close to the tuner as possible. The power lead of the TV receiver is wrapped around a ferrite rod, too.

The combination of highpass filter and ferrite-wrapped coaxial lines isolates both the inner and outer con-
ductors of the line from the strong RF field of the local transmitter. The ferrite-wrapped line cords reduce RF pickup from the power line.

That's about all you can do without digging into the VTR or otherwise modifying it to reduce RF pickup - a formidable task.
Bip points out a possible solution to RFI problems that may be available in the near future. Many problems with stereo, TV receivers, ham gear, and computers arise because the plastic cases in which the units are enclosed are "transparent" as far as RF is concerned. The equipment is completely vulnerable to any strong, nearby RF field. And in the case of the TV receiver and the computer, these devices can radiate RF "hash" that will cause problems on nearby communications receivers. Under test now is an aerosol EMI/RFI coating that can be sprayed on the inside surface of a cabinet and, when properly applied and grounded, will provide up to 75 dB of shielding effectiveness at 100 MHz . The spray adheres to any plastic, glass, or metal surface and dries to about 2 mils thickness, providing a highly conductive coating that restricts radiation through the case. This product should be available before the end of the year. While it won't solve all RFI problems, it will help the experimenter combat direct radiation and unwanted pickup by highly sensitive electronic equipment mounted within a "dust cover" that masquerades as a cabinet. $\dagger$

## 18 and 24 MHz revisited

The Radio Society of Great Britain reports that as of January 1, 1984, 42
countries had authorized Amateur operation in the $18-\mathrm{MHz}$ Amateur band. Some countries have excluded small portions of the assignment to protect local communication circuits. The main countries holding up Amateur operation in this band by their citizens are the United States and the Soviet Union.
As for the $24-\mathrm{MHz}$ band, the RSGB reports that as of January 1, 1984, 42 countries had authorized Amateur operation in this band. Only Australia restricts a small segment of the band to protect a local communication circuit. Again, the main countries holding up Amateur operation in this band by their citizens are the United States and the Soviet Union.
Hello, Ivan! We have something in common at last!
Once again this is the case of a "clean" transmitting
signal being received by the VTR . . . Ed.
†Shielding can be enhanced by selection of appropriate
cabinet materials and use of special EMI/RFI-resistant
materials. See "Electromagnetic Interference and the
Digital Era," K3PUR, September, 1984, and "EMI/RFI
Shielding: New Techniques," by Vaughn Martin,
January and February, 1984.
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## L and C measurements

## Simple circuit determines values with ease, accuracy

The typical method of measuring small value capacitors and inductors using a grid dip meter and a known value of $L$ or $C$ is effective, but because of circuit loading and dip meter calibration errors the results are not very accurate.

Hams who own a frequency counter can take advantage of the accuracy of this instrument to determine the value of junk box unmarked components. The technique involves measuring the frequency of an LC oscillator and then adding the unknown component to the resonant circuit, again noting the output frequency. The value of the unknown component is easily calculated using these two frequencies.

## differential amplifier used as oscillator

The oscillator circuit shown in fig. 1 uses Q1 and 02 as a positive feedback differential amplifier. This minimizes the loading on LICI. Q3, a buffer stage, isolates the counter and prevents loading down the oscillator. S1 places the unknown component in parallel with the resonant circuit LIC1 for capacitance measurements and in series with $L 1$ for inductance measurements. In both modes the output frequency decreases in proportion to the value of the external component.

Once the effective values of $L 1$ and $C l$ are known, the unknown values can be calculated from:

$$
\begin{align*}
& C_{x}=\frac{C l\left(f_{l^{2}}^{2}-f_{2}^{2}\right)}{f_{2}^{2}}  \tag{1}\\
& L_{x}=\frac{L 1\left(f_{1}^{2}-f_{2}^{2}\right)}{f_{2}^{2}} \tag{2}
\end{align*}
$$

where $f_{l}$ is the original frequency in MHz
$f_{2}$ is the new frequency
$C$ is in picofarads (pF)
$L$ is in microhenries $(\mu \mathrm{H})$

I calculated a number of values and made up a series of graphs for inductance and capacitance values from 0.1 to $350 \mu \mathrm{H}$ and for 3 to 700 pF . Agreement with known values is well within normal tolerance levels. My graphs are based on the initial frequency $f_{l}$ set to 9.00 MHz . Since this frequency is slightly altered by the position of S1, the core adjustment screw of $L 1$ protrudes from the front panel so that $f_{l}$ can be trimmed to 9.00 MHz before checking an unknown.

As mentioned earlier, the effective value of $L I$ and CI must be determined as the stray capacitance and inductance in wiring needs to be accounted for. This is easily accomplished with a known value of capacitor and inductor. Set S1 to parallel with the test probes open, adjust $L 1$ to 9.00 MHz on the counter, clip on the known capacitor $C 2$, and note the new frequency . The value of Cl is:

$$
C l=\frac{f_{2}^{2} \times C 2}{f_{1}^{2}-f_{2}^{2}}
$$

To determine the effective value of $L l$, set S 1 in series with the test probes shorted and adjust $L 1$ until the oscillator is at 9.00 MHz . Attach the known inductor, $L 2$, to the test probes and note the new frequency, $L 1$ is:

$$
L I=\frac{f_{2}^{2} \times L 2}{f_{I}^{2}-f_{2}^{2}}
$$

Use these values for $C l$ and $L I$ in formulas 1 and 2 for calculating the unknowns.

Construction is not critical; I used an L-shaped piece of aluminum to form the panel and base, and a scored piece of PC board for the oscillator circuit. A 12 inch or so length of small coax with mini-alligator clips was used to connect the unknown components.

I find I'm using this unit on every construction project. It certainly is convenient for checking the minimum and maximum capacity of small trimmers and useful in making it possible to wind a coil to a specified value - a real help when building bandpass and other types of filters.

By Larry Duthie, WB6ZLN, 1305 Lubich Drive, Mountain View, California 94040

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fig. 1. Oscillator circuit uses $\mathbf{Q 1}$ and $\mathbf{Q 2}$ as a positive feedback differential amplifier.

My thanks to Jim Loring, K.A6VVE, for the oscillator circuit; it produces stable output over a very wide range of LC ratios.
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(continued from page 7)
asks that the $32-\mathrm{MHz}$ land mobile reserved segment of the 800 MHz spectrum be released immediately for their use. - Ed.)

In summary, the $220-\mathrm{MHz}$ band is not only well occupied, even in the weak-signal area, but also necessary to Amateur Radio, in order to handle the overflow of all types of operations from 2 meters, which would not be as well served by 70 cm ; Packet Radio will also occupy some of the lower frequency regions. The gaps at the bottom are there for a purpose: to eliminate the possibility of overload that frequently hampers weak-signal operation. Weak-signal operators need this valuable portion of the spectrum as a bridge between 2 meters and 70 cm , which is vastly different in radio propagation.

- Joe Reisert, W1JR
*For a thorough description of all the propagation modes effective on 220 see the July and September, 1984, VHF/UHF World columns by W1JR - Editor


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# Smith Chart impedance matching on your Commodore 64 

## Crunch the numbers, plot results with this handy 200-line program

If you have ever tried impedance matching, you've probably been introduced to the Smith Chart. Although it's fashionable to turn to computers to perform a variety of tasks, many RF types prefer to use the slower "graphic approach" because the Smith Chart provides a visual means of analysis not obvious in long columns of numbers.

But using the Smith Chart can be frustrating: let's see - do I rotate clockwise or counterclockwise? I want a shunt element; do I follow impedance or admittance curves? Do I multiply or divide by $Z_{0}$ ? Using this program fig. 1, the computer will do all the number crunching for you, and display your impedances on the screen within a few seconds. It will even handle errors; if you come up with an incorrect value, just press a key - your last trial disappears. If you like the answer, just press another key: the computer then stores that value and you can add another section.

This article assumes that you understand Smith Charts. If you don't, see the references listed at the end of this article for an explanation.) But even if you don't understand the plot, you can still use this program because all impedances are first printed in tabular form; the plot is an option you can ignore.

## program description

This program is written for a Commodore 64 using Simons' BASIC for efficient utilization of graphics commands. If you have a different computer system you can use the equations in lines $\mathbf{1 0 0 0}$ through 7504
and add your own printing/plotting commands. A summary of the major program sections is listed in table 1, and a detailed description follows.

Lines 1 through 44 are used for program initialization. In lines 10-11 you select a smooth or discrete plot. Later, when impedances are plotted on the screen, either selection will print a " + " on the Smith Chart at each frequency; if you select a smooth plot, a line will connect the plots to form a continuous



```
NCE MATCHING":FKINT" C=S DWN'SDWN:
4 CENTFEEFOF "USING":PFINT
6 FFINT" DWN SWN'SED:":CENTFE FOF "SMITH CHART"
```




```
    (S)":O$ D*"D"ANDD&-%"S"THEN1G
```



```
INFUT"DWNFOON WHAT VALUE VSWF CIFELE":
```



```
SGN: DWNOMOW
FEONTMDWN:INFUT FFECUENCY"S : INFWT"TN MHZ":FF(U)
```



```
PRINT"SWN: FREQ, FS XG"FRINT
```




```
FFINT####,##", XSE:FFINT:NEXT
INF!IT"ARE YOUSATISFIED (Y=YEG)":A4
```




```
XNFUT"FLOT LOAD, MMEEDANCE YEYES
XM=1:4:JFF%="Y" THEN GOSUE GOOO
CFINT" CLFS CHO
CRINT", = SERIES LUNED (SEFIES M-C)
OEINT" S SEFIES TUNED (SEFIIES L-C)
FRINT"
FEIINT""& SHUNT TUNED (SERIES (FAFALEC)
FFINT":G SHLNT TFANGMISSION LINE
FEINT":1 TFIANSFOFMER
FFINT": SEFIEGF
FFNT": GHUNT FODWN
CFINT"14 STOF ADDING SECTIONS
"NFUT"FED DWN'ODWNYDWNODWNSCHDICE (1-14)",M:FRINT"CO=
IF M, OF M,14 THEN 30
```

fig. 1A. Computer aided Smith Chart design program listing, lines 1-82.

By Lynn A. Gerig, WA9GFR, RR \#1, Monroeville, Indiana 46773

```
1000 FEINT CHR\$ (147)"ADD SERIES CAF'ACITOR
00\% INEUT"WHAT IS VALUE (IN FF)":C
FAR \(J=1 T J\) N
\(\times(2)=6: 3)\)
\(Y(J)=1\{J\rangle-1 /(2 * * * F(J) * C * 1 E-06)\)
FRINT CHR \({ }^{(147)}\) (ADD SERIES INDUCTOF
INFUT"WHAT IS VALUE (IN UH)":L
INFUT"WHAT IS
\(F O R\)
\(J=1\)
TO
\(\mathrm{N}: ~ X(J)=R(J)\)
\(Y(J)=I(J)+\) + \(\quad\) FF \((J)\) *L: NEXT: GOTOPOOO
CFINT CHF (:AT) יADE SERIES TUNED (SERIES (-C)
INFUT"WHAT IS VALUE OF L (IN UH)":
\(F D R \quad J=1\) TO \(N: X(J)=F(J)\)
```



```
INFUT"WHAT IS VALUE OF C (IN FF)":C
FOR \(J=1\) TO N: \(X(J)=R(J)\)
```



```
T: 60709000
000 FRINT CHR \(\$\) (147) "ADD SERIES TRANSMISSION LINE
3002 INFUT"WHAT IS LINE IMPEDANCE (DHMS)"; 1
3006 INFUTWHAT IS VELOCITY FACTOR:IV
3010 ENFUT"WHAT IS LENGTH (IN INCHES)";LL
\(3010 \mathrm{FDR} J=1\) TO \(N\)
\(3015 \quad T=1,2 \pm L L F(J) / 39.37 / V\)
\(\begin{array}{ll}3020 & D=(R(J)+Z 1) 2^{2}+I(J)^{\wedge 2} \\ 0025 & =\left(R(J) * 2-21^{2}+I(J)^{2} 2\right) / D\end{array}\)
    \(I=2 * Z 1 * I(J) / D\)
\(Z=S 0 R(R * R+1\)
\(3040 \quad T=180 /\) i \(*\) ATN \((I /(R+1 E-30))-2 * T+180 k(R * 0)\)
3045 R=2* \(\cos (T *: / 180\) )
\(3050 I=2 * S I N(T *: / 180)\)
```



```
Soed \(\times(J)=21 *\left(1-F^{2} 2-I \times 2\right) / D\)
```




```
SEOO PFINT CHFS ( 147 )"ADD SHUNT CAFACITDR
Z5O2 INFLT"WHAT IS VALUE CF C (IN FF)":C
ESOG FOR J=1 TQ N: W=2* WC*1E-OE
-
SE: X (J) = R (J) /
4000 FR
4000 FFINT EHF虫: 47)"ADD SHUNT INDUCTOR
40OC INFUT"WHAT IS VALUE OF \(L\) (IN UH)":L
\(401 \mathrm{E} F \mathrm{FIR} J=1\) TO N: \(W=2 *, * F(J) * L\)
\(40 \sum 5=F(\Omega) \quad(J+(1 \leq J)+W)\)
```



```
\(40 耳 E\)
\(404(X)=W *(F G)\)
\(45 X: G O T O Q O G\)
4500 FRINT CHFíi (47)"ADD SHLNT TINED
4500 FRIN CHFid (:47:"ADD SHLNT TUNED (SEEIES L-C
4504 INFUT"WHAT IS VALUE OF C \{IN FF)":C
\(4 \mathrm{E} 10 \mathrm{FOF} \quad J=1\) TO N
\(4515 W=2 * * F(J) * L-(1 E+06) /(2 * * F(J) * C)\)
    \(D=F_{1}(5,2+15+W)=2\)
    \(X(J)=F(J) * W=D\)
\(Y(J)=W\)
```



```
    FFINT CHF\$ ( 147 )'ADD SHUNT TLNED (FAFALLEL L-E)
EOOE INFUT"WHAT IS VALUE OF C (IN FF)":C
EOO4 INFUT"WHAT IS UALUE OF \(L\) (IN UH)":L
5010 FOF \(\quad 3=1 T 0 \mathrm{~N}\)
```



```
    \(D=F:(N)=(I(J)+W)^{2}=\)
    \(x(J)=F(J) * W=2 / D\)
    Y(J) =W* (F, (J) \(+1(0)=+W * I(J)) / D\)
    NEXT:GOTOQOOO
    FFINT CHF: 147 "ADD SHUNT TFANSMISSION LINE
    INFUT"WHAT IS LINE IMFEDANCE !OHMS!"Z1
    INFIT"NAA : 5 LNE JELOETT'FACTMK": \(V\)
    INFUT"WHAT IS LENGTH (IN INCHE SOM"LL
    INPUT \(\mathrm{S}^{*}\)
    IF S S S" "Q" AND S\$ン"S" THEN E510
    EOF \(J=1 \quad\) TO N
```



```
    IF \(\mathcal{S} \$=" \mathrm{D}\) " THEN \(W=21\) TAN \((1+90)\), 180\()\)
```



```
    \(x(J)=\left\{\begin{array}{c}(J) * W 2 / D \\ \hline\end{array}\right.\)
    Y(J) \(=W *\) (F (J) \(2+I(J)=2+W * 1(コ)) / D\)
    NEXT:GOTOGOOO
    FFINT CHRS (147) 'ADD TFANSFQFMER
    INFUT'STEF UF OF DOWN UOF D: \(:\) :
    TF TS U"AND TS "D" IHEN 6000
    INFUT"WHAT TFANSFGFMATION FATIG": W
    IF TB="D" THEN W=1:W
    2OR \(J=1 \quad\) TC \(N: x(J)=W * \&(J)\)
    \(Y(コ)=W * I(2):\) NEXT GOTO 9000
    ELINT CHF: 4 \% "ADD SEF:ES FESISTJF
    INFUT"WHAT VALUE OF F:":FG
    \(Y(N)=I(J)\) NEXT: GOTO 9000
    FRINT CHR (147)"ADD SHUNT RESISTOR
    INPUT"WHAT VALUE OF Fi": FiS
    FOF J=1 TO N
    \(Q=\{F(J)+F, 5)-+\{J\}=\)
```




```
    FRINT CHFL(147)
    INFUT "WAN TO KUN ANGTHEF JHE": A\$
    IF LEFTGi (Aま, 1)="Y" THEN 10
75 G4 FRINT AT (ROF: 14,1 )"ELUGDOD-GY:C=4.":END
3000 HIFESKOF OF, \(: X A=100 * \times M\)
BOOT CIFCLE FOF \(160,100, \times F, 100,1\)
3004 LINE FOF \(160-X R, 100,160+X R, 100\),
gơg ARCROF \(1601+x R, 9,190,270,10, \times R, 100\)
```



```
3014 CIFCLECNOF \(160+X R /=100, \times R /=\)
```

fig．1B．Program listing，lines 1000－8014．

fig．1C．Program listing，lines 8016－9230．
curve．The goal of most impedance matching is to find a result which is within a particular VSWR．In lines 12－13 you select the value of a VSWR circle to appear on the plot．This makes it easy to check your results； either your plots are within the circle，or you need to refine your circuit．In line 14 you select the charac－ teristic impedance．This does not affect any calcula－ tions or tabular results：it is the value which is at the center of your Smith Chart plot．All impedances are normalized to this before being plotted（lines 8120－8130）．

You are next asked how many frequencies you wish to work with（line 15）；you then must input each fre－ quency and the resistive and reactive series com－ ponents of the starting（load）impedance at each frequency．

After you input all frequencies and load impedances， you are given a chance to start over if you made an error．Then you can choose to print the tabulated load impedances on your printer，plot them on a Smith Chart，or begin matching．

Lines 50－82 present a menu for the type of matching element to select．The program next branches to the correct set of equations for that choice（lines 1000－7504），and you are then asked to input those component values．For a detailed explanation of each matching section，see the section on matching net－ work equations in the appendix．
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ADD SEFIES INDUCTOF
WHAT IS VALLUE (IN UH)? 36.9

| FFEQ | FS | $\times 5$ |
| :---: | :---: | :--- |
| 1.8 | 7. | 17.32 |

ADD SHUNT CAFACITOF
WHAT IS VALUE OF C (IN FF)? 4400

$$
\begin{array}{lll}
\text { FREQ } & \text { FS } & \times 5 \\
1.8 & 49.89 & -.37
\end{array}
$$

fig. 2. The addition of two components converts an 80 -meter vertical to $\mathbf{1 6 0}$ meters.
table 1. Major program sections.

| line numbers | program content |
| ---: | :--- |
| $1-10$ | Format, select discrete or smooth plot. |
| $12-13$ | Select VSWR circle to plot. <br> 14 |
| $15-44$ | Select characteristic impedance. <br> Input resistive \& reactive parts of load <br> impedance at each frequency. Print or <br> plot result if desired. |
| $50-82$ | Select type of matching section to try. <br> Calculation of impedances according to |
| $1000-7504$ | type of matching section chosen. |
| $8000-8195$ | Subroutine for graphics plotting of <br> Smith Chart. |
| $9000-9170$ | Print new impedances in tabular form, <br> then choose whether to print, plot, <br> discard, or keep trial value. <br> "Good" trial value becomes new impe- <br> dance to match with next section. |

Lines 8000-8195 contain the graphics commands for plotting a Smith Chart on the screen. Most of these lines use graphics commands peculiar to Simons' BASIC: you may choose to write your own plotting subroutine if you have another system. A new chart is drawn in lines 8000-8023. If you choose to plot on an old screen, you enter at line 8100, which recalls the last graphics screen from memory. The impedance plotting is performed in lines $\mathbf{8 1 1 5 - 8 1 6 0}$. The equations in 8120-8130 convert the impedances to a point on the chart normalized to the previously selected $Z_{0}$. The chart $y$-radius is 100 bits, and the $x$-radius depends on the value of " XM " Isee section on printer interfaces below). Line 8150 will connect the " + " plots with a line if "smooth plot" was previously selected. The plot-

## THESE WERE YOUR LOAD IMFEDANCE INFLTS

| FREQ | RS | $\times 5$ |
| :---: | :---: | ---: |
|  |  |  |
| 7. | 52. | -110. |
| 7.1 | 57. | -100. |
| 7.2 | 65. | -90. |
| 7.3 | 70. | -80. |

ADD SEFIES TRANSMISSION LINE
WHAT IS LINE IMFEDANCE (OHMS)?50
WHAT IS VELOCITY FACTOF? . 67
WHAT IS LENGTH (IN INCHES)? 130

| FREQ | RS | $\times S$ |
| ---: | ---: | ---: |
|  |  |  |
| 7. | 9.74 | -25.46 |
| 7.1 | 11.60 | -23.89 |
| 7.2 | 14.15 | -22.96 |
| 7.3 | 16.49 | -21.89 |

ADD SHUNT TFANSMISSION LINE
WHAT IS LINE IMFEDANCE (OHMS)? 50
WHAT IS LINE VELDCITY FACTOR? . 67
WHAT IS LENGTH (IN INCHES)? 100
OFEN (ロ) OF SHDFTED (S) STUET S

| FREQ | RS | $\times 5$ |
| :---: | :--- | ---: |
|  |  |  |
| 7. | 74.46 | -11.64 |
| 7.1 | 59.70 | -8.10 |
| 7.2 | 51.39 | -1.24 |
| 7.3 | 45.36 | 2.91 |


fig. 3. Compensating for tower effect on 40-meter slopers (example 2).
ted chart will stay on the screen until either function key 77 or $f 8$ is pressed. Pressing $f 8$ will copy your plot to your printer, and 77 will return you to the tabular listing of frequencies and impedances with another menu.

No matter what type of matching section is chosen, after the appropriate impedance calculations are per-


formed the program branches to line 9000 and the new impedances at each frequency are printed on the screen below the values of the network components you chose. A menu appears at the bottom of the screen. You must then press a function key to continue. Pressing f 1 or f 2 will cause the impedances listed to be plotted on a new "clean" screen (see section on printer interfaces below). Pressing f 3 will add the new plot to a previous chart. If you press f 4 , the tabulated data at the top of the screen is printed on your printer. Pressing $f 5$ causes the computer to erase the bad value you just tried, and 7 causes the trial value to become the next load impedance to be matched (lines 9200-9230): you then branch back to the master menu at line 50.

## examples

The three examples given below demonstrate some of the possibilities available in the program.

Example 1. My 80 -meter vertical antenna is electrically "short" at 160 meters and exhibits an impedance of about 7-j400 ohms. What values of $L$ and $C$ do I need to match it to 50 ohms? I know I should start with a
series inductor with a reactance of greater than 400 ohms (about $35 \mu \mathrm{H}$ ) then add a shunt capacitor. After experimenting with several values, I ended up with those in fig. 2. I only printed tabular results without graphics plot.

Example 2. When I erected my 60 -foot tower, I fed the top set of guy wires as 40 -meter slopers. Probably because of coupling to the tower, they were not resonant, as was to be expected. The impedances as measured at the shack end of the coax feedline are listed and plotted in fig. 3. Although I could have obtained a good match with a series inductor, I wanted to use leftover lengths of coaxial cable for the experience of matching with lines/stubs. The resulting impedances, shown in fig. 3, are an example of superimposing several plots on the same chart lusing function key f 3 ). I am presently using this network built from RG-58 cables, and the measured results are within 5 percent of those calculated.

Example 3. My 2-meter whip antenna looks like 70 ohms at resonance, including ground losses, with an increasing impedance off resonance. I wish to "broadband" match it and have less than 2:1 VSWR from

110 to 160 MHz for reception of aircraft and public service bands in addition to the 2 -meter ham band. The results are shown in fig. 4. In this case I printed intermediate tabular results with each new element, but I plotted only the original and final impedances (on separate plots).

## entering the program

Enter the program as shown taking the normal precautions to SAVE it before you RUN it, so that if you make a typing error that could cause a lock-up, you'll be able to go back to the saved version without having to retype the entire program. The following is an explanation of the mnemonics printed by my interface:

```
<CLR> = SHIFT-CLR
<DWN>= cursor down
<LFT> = cursor left
<BLU> = CTRL-7 (blue)
<RED> = CTRL-3 (red)
<C=4> = Commodore-4 (gray 1)
```

In addition, my interface sometimes prints<ROF $>$, directly following unique Simons' BASIC commands. Ignore this when you type the program. Using Simons' BASIC on the Commodore 64, high-resolution graphics commands permit a BASIC program of only 200 lines, using about 6K of RAM. However, the equations listed are valid for any computer or calculator.

If you don't want to type the program yourself, I'll make two verified copies for you. (Just send me a blank tape or formatted disk with a stamped, selfaddressed mailer, and a check or money order for $\$ 5.00$. Use the address shown at the beginning of this article.) Without Simons' BASIC, bank switching for the high-resolution screen and point-by-point plotting needs to be done with additional programming. I also have a version for the Commodore 64 that does not require Simons' BASIC, but it is over 500 lines long and therefore not practical for listing here. I will supply a copy of it, or a similar version specifically for the VIC-20, requiring 32 K expansion, under the terms described above.

## appendix

The convention I used for the various matching elements and impedances is shown in fig. A1. The equations used for each type

fig. A1. Matching network configurations.
of reactive matching element (used in program lines 1000 -7504) follow in fig. A2. These equations can be used on any computer or calculator.

## impedance value to Smith Chart plot

Although the Smith Chart looks complicated, it's nothing more than a plot of the reflection coefficient, $\varrho$, defined as

$$
\varrho=\frac{Z-Z_{0}}{Z+Z_{0}}
$$

where $Z_{0}=$ the characteristic impedance you are working with and $Z=X+j Y$ (your complex impedance). When plotting an impedance, the following two equations apply:

$$
\begin{aligned}
& x \text {-axis value }= X^{2}-Z_{0}^{2}+Y^{2} \\
&\left(X+Z_{0}\right)^{2}+Y^{2} \\
& y \text {-axis value }=\left(X+Z_{0}\right. \\
&\left(X+Z_{0}\right)^{2}+Y^{2}
\end{aligned}
$$

The value obtained will range from 0 (center of chart for $V S W R=$ I) to 1 (outside edge of chart for $V S W R=\infty$ ). They can be scaled by any value you desire. I multiplied by 100 for a circle with a radius of 100 dots. Equations are found in lines 8120-8130.
series L-C components

series capacitor
$x=R$
$y=1-1$

series L-C in series
$X=R$
$Y=2 \pi f L-\frac{1}{2 \pi f C}+1$

series L-C in parallel
$X=R \quad 2 \pi f L$
$X=R$
$Y=1+\frac{2 \pi f L}{1-(2 \pi f) 2 L C}$

fig. A2. Equations and type of matching section used in program lines 1000-7504.

## shunt inductor

$W=2 \pi f L$
$X=\frac{R W^{2}}{R^{2}+(I+W)^{2}}$
$Y=\frac{W\left(R^{2}+12+W I\right)}{R^{2}+(I+W)^{2}}$

shunt capacitor
$W=\frac{-1}{2 \pi f C}$
$X=R^{2}+\frac{R W^{2}}{(1+W)^{2}}$
$Y=\frac{W\left(R^{2}+12+W I\right)}{R^{2}+(1+W)^{2}}$

shunt $L-C$ in series
$W=2 \pi f L-\frac{1}{2 \pi f C}$
$X=\frac{R W^{2}}{R^{2}+(1+W)^{2}}$
$Y=\frac{W\left(R^{2}+I^{2}+W I\right)}{R^{2}+(I+W)^{2}}$
shunt L-C in parallel
$W=\frac{2 n f L}{1-(2 n f)^{2} L C}$
$X=\frac{R W^{2}}{R^{2}+(1+W)^{2}}$
$Y=\frac{W\left(R^{2}+12+W I\right)}{R^{2}+(I+W)^{2}}$

series transmission line

$$
\begin{aligned}
& W=\frac{1.2 L f}{39.37 V} \\
& D=\frac{2 Z_{1} I}{\left(R+Z_{1}\right)^{2}+12} \\
& E=\frac{R^{2}-Z_{1} 2+12}{\left(R+Z_{1}\right)^{2}+12} \\
& Z=\left(D^{2}+E^{2}\right)^{1 / 2} \\
& T=\tan -1(D / E)-2 W
\end{aligned}
$$



LENGTH $=$ L(INCHES )
CHARACTERISTIC
IMPEDANCE $=Z_{1}$
VELOCITY FACTOR $=V$
Note: If calculator gives only first and fourth quadrant for tan-1 answers $\left(-90^{\circ}<W<90^{\circ}\right)$, add $180^{\circ}$ to $T$ if $D$ was negative.
$x=\frac{Z_{1}\left\{1-(Z \cos T)^{2}-(Z \sin T)^{2}\right\}}{(1-Z \cos T)^{2}+(Z \sin T)^{2}}$
$Y=\frac{2 Z_{1} Z \sin T}{(1-Z \cos T)^{2}+(Z \sin T)^{2}}$
shunt transmission line (open or shorted stubs)

$$
W=\begin{gathered}
1.2 \mathrm{Lf} \\
39.37 \mathrm{~V}
\end{gathered}
$$

if open stub: $T=Z_{0} \tan \left(W+90^{\circ}\right)$
if shorted stub: $T=Z_{0} \tan (W)$
length $=L$ (inches)
characteristic impedance $=Z_{1}$
velocity factor $=$ V
length $=L$ (inches)
characteristic impedance $=Z_{1}$
velocity factor $=V$
$x=R 2 T^{2}$
$X=R^{2}+(I+T)^{2}$
$Y=\frac{W\left(R^{2}+I 2+T I\right)}{R^{2}+(I+T)^{2}}$

$Y=\frac{W(R+I}{R^{2}+(I+T)^{2}}$

## transformer



## printer interface

This program was designed to calculate impedances and display them in tabular or graphic form on the screen, so you can use the program even if you don't have a printer. Just don't respond with a "yes" to questions such as "Do you want to print?"

If you do have a printer, you may want to note the two printer commands used; HRDCPY (lines 40, 9140) gives a normal screen dump (tabular data), and COPY line 8195 copies a highresolution ( 320 by 200 bits) graphics screen to the printer. Although the commands are optimized specifically for a Commodore printer, the program should run successfully with any printer/ interface combination that emulates the Commodore. I use a Star Gemini-10X printer (an Epson responds the same way) with a Tymac Connection for an interface, and reproduction of the full high-resolution plot takes less than a minute. $A$ friend with a Prowriter and Cardco interface gets similar results. Using a Cardco/ $+G$ with a Gemini or Epson printer produces the same plot, but a high-res dump takes about 45 minutes, so be patient. If you have another brand, you may need to experiment, but I am not aware of any combination that won't work.

Note: the aspect ratio (relative distance between dots on a line versus distance between lines) is different for the screen than the printer. To draw a circle on the screen, use an $X / Y$ ratio of 1.4 (value of XM in lines 44, 9110). This will copy as an oval on the printer. If you want a printed chart (lines 9055,9120 ), use the ratio 0.833 ; this produces an oval on the screen, but a circle on the printer. If another brand of printer produces ovals, experiment with the value of XM in line 9120.

- WA9GFR


## references

1. The ARRL Antenna Book, 14th edition, American Radio Relay League, Newington, Connecticut, 1982.
2. James R. Fisk, W1HR, "How To Use The Smith Chart," ham radio, March, 1978, page 92.
3. Phillip H. Smith, Electronic Applications of the Smith Chart, McGraw-Hill, New York. 1969.
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## AEA's "Doctor DX" Morse-code contest trainer

When I visited the AEA booth at Dayton several years ago, I sat down with Mike Lamb, AEA's president, to look at a new "mini-transceiver" they had on display. I was quite impressed with its credentials: it had all the bands I would want to work, and the sensitivity and selectivity numbers were good.

At Mike's urging I put the headphones on and tuned around the bands to see what was going on. Twenty and 15 were hopping with DX and it seemed as if a contest were going on. Mike nudged me in the ribs. "Go ahead," he said, "give one a call." I tuned in a G3 station who was calling CQ. I dumped my call and got an immediate response: "N1ACH de G3XXX UR 59914 BK," I went back, "G3XXX de N1ACH TNX UR 5990573 BK. " $A$ bell should have gone off in the back of my mind that something was amiss; there are no contests scheduled for the Dayton weekend. Oblivious to Mike's snickers, I blithely went on. After a few minutes, Mike let me in on his little secret: I was talking to a microcomputer. Needless to say I felt a little foolish. But I knęw I was in good company. They'd been able to fool almost everyone who'd stopped by their booth so far. In fact, in their dozens of demonstrations, only two people figured it out.

Mike then explained what they were up to and gave me additional background on the unit. After that, I really didn't hear much about the simulator until the other day when Mike called to tell me about his newest product.

## Doctor DX

Doctor DX is a cleverly designed module made up of two custom programmed EPROMs and several AEA designed integrated circuits. It fits into the cartridge port of the Commodore C-64 computer and lets you simulate chasing DX without actually being on the air. You can program Doctor DX to put your QTH anywhere around the world from Albania to Zambia. Other variable parameters are time of day, power output, and frequency of operation.

## use

After installing the board into the computer and hooking up a keyer, you have to set a couple of variables before you can begin. The first is to locate your station by longitude and latitude. The second is setting the internal clock for the time of day at which you'd like to be operating. You then set your power output to one of three levels: 2, 20, or 200 watts. Finally, you select the band on which you want to operate.

Propagation is programmed to simulate what you'd hear on a given band at that time of day. For instance during the daylight hours, 10 and 15 meters will be open to DX; 160 and 80 will be dead. At night the opposite will be true: 160 , 80 , and 40 will be open, with the two higher bands closed. Twenty meters will be open to various parts of the world most all the time.


Another interesting aspect is that AEA has programmed the EPROMs to simulate the propagation conditions that existed during September 1979. At that time the three higher bands $(20,15$, and 10$)$ were much better than they are now. (Gee, if you get depressed listening to 10 meters nowadays, listening to the computer will restore your faith in the band!) This also means that propagation of the three lower bands 160,80 , and 40 is not as good as we are now experiencing but . . . you can't have everything, can you?

Callsigns are all randomly generated by the computer, with prefixes weighted by Amateur population density in that country. AEA guarantees that at least one station will be on from each of the 304 DXCC countries programmed into the computer. In an effort to replicate conditions as much as possible, stations on the lower end of each band are found working at highspeed CW (30-40 WPM). The higher you go on each band, the slower the stations are. Contacts consist of a signal report followed by CQ WW zones. If you miss an exchange, you can ask the station for a repeat. You can also request that the station speed up (QRQ) or slow down (QRS).

There are four frequency tuning rates with Doctor DX. The function keys on the right of the Commodore keyboard are used to "tune" the receiver up and down frequency. F-1 is FAST UP, to 20 kHz per second, F3 up 2 kHz per sec-
ond, F5 is FAST DOWN -20 kHz per second and F7 is down -2 kHz per second.

So that you can follow your progress with the test, the computer is programmed to constantly display your score and QSO rate. Contest lengths can be varied from a one-hour sprint to a test of several hours' duration.

## operation

Now that everything is all hooked up and location, time of day, power, and frequency (160 meters, of course) are all programmed in, it's time to get this mock contest started. The first station worked was a K2, and I even got a 599! Hey, I'm off and running!

The first thing to decide is whether I'm going to find a clear frequency and call CQ or do a "hunt and pounce" contest. Since I want to try both, I start by calling CQ. After two calls, a VE3 comes back with a 589 in zone 5. I quickly work another 10 stations before a VE2 starts calling CQ up a few kHz from mine. However, I hear a weak call, and ask QRZ? By golly, it's my first DX, an HI7. He gives me a 589 and zone 8. I shoot back his report only to have him ask twice for a repeat. Repeat? I am talking to a computer aren't I? After a couple of minutes, I'm not so sure. (Mike's done it again. I actually can believe I'm in the midst of a CQ WWII

Now it's time to do some looking to see what I can find. I change bands and start at the bottom, looking up frequency. The first station I tune by is running at least 40 WPM. I call him twice only to have him go back to two other computer calls. Finally he calls me and I put another into the log.

After about an hour's worth of operation it's time to see how l've done. I have 28 contacts on three bands, with the majority (22) on 160 meters, 4 on 40 meters, and one Ti3 on 80 meters. I'm sure I would have done better during my one-hour sprint if there'd been no phone calls or other interruptions.

My QSO rate varied from 35 to 45 QSOs per hour while I was able to dedicate full time and attention to the test. I feel quite strongly that with a little practice my rate during actual contests would improve dramatically.

There's the real beauty of Doctor DX. No matter where your interest in Amateur Radio lies, using Doctor DX will help improve your CW operating skills. After a couple of hours of use, you'll find that code copy comes much more easily. One of our own Novices stopped by and watched while I was running the test and commented that the real-life simulation offered by Doctor DX would be a tremendous help in improving CW skills and operating confidence in a way that wouldn't be embarrassing to the beginner. Experienced contesters will find operating a contest from EP2 to be quite a change from their normal QTH. I think that many will find the added insight of having worked portable EP2 to give them a tactical edge during actual contests. Doctor DX can be many things to different people. I think that those who use it will find it to be very rewarding and plenty of fun.


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The price of Doctor DX will be $\$ 149.95$ from AEA dealers and the unit should be available by the time you read this review. It is a perfect Holiday gift for that hard to buy for ham friend. Clubs will also find it quite useful for training in sprint contests or in any number of other applications.

For information, contact AEA, P.O. Box C2160, Lynnwood, Washington 98036.

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The "tough tones" from your handheld's keypad are transmitted to another receiver which provides the audio link into the "Remote-APad." The tone selected then activates the keypad. If you hit a \#1 on the portable then a \#1 on the radio to be controlled is activated. When controlling radios like the ICOM-701 and using the RM-2 controller the power of the microprocessor already built into the rig is unleashed. Many other radios can also be used with the "Re-mote-A-Pad," in fact any radio or rotator (Pro Search for example) having a $3 \times 4$ or $4 \times 4$ keypad may be controlled since the rows and columns are found on all keypads which are used to control computerized devices.

Find yourself a radio which is now controlled with a keypad and install a "Remote-A-Pad." Add a phone patch for audio link, and the "Remote-A-Pad" will also turn on and off your link with two on board 4 digit DTMF (touch tone) programmable decoders. You set the code to any series of the 16 DTMF tones. LEDs on the board will tell you the status of the controlled device (on or off). A momentary pulse is also provided and may be used directly into logic to control on-off devices. Relays may be added by using a transistor driver.

The "Remote-A-Pad" is shipped with a 22-(gold) pin card edge connector as well as a 16-pin dip socket ribbon cable for easy installation. Detailed installation instructions and schematics are provided for $\$ 149.00$.

For further information, contact Engineering Consulting, 583 Candlewood Street, Brea, California 92621.

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## satellite converter

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Provisions are made to allow duplex operation so your transmitted signal can be received simultaneously for system and frequency checks. A front panel SPOT pushbutton switch places the transmitter in operation with carrier inserted.

Priced at $\$ 489$, the unit simplifies station assembly, reduces the number of separate items and interconnections, eliminates the need to buy separate converters, and converts your HF station into a transceiver type OSCAR station.

For additional information, contact Ten-Tec, Inc., Sevierville, Tennessee 37862.

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For additional information, contact Bird Electronic Corporation, 30303 Aurora Road, Cleveland (Solon), Ohio 44139-2794.

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## HF antenna accessories catalog

Microwave Filter's Catalog PC/84 describes baluns, multiband traps, and remote antenna switching relays for the 2 to 1000 MHz communications bands.

The catalog illustrates the construction of single and multiband dipoles in the 1.8 to 30 MHz Amateur and HF communication bands and offers other construction accessories such as end insulators, weatherized center-feed insulators, wire, cable, and connectors.

The system of remote, voltage-controlled antenna switching relays allows selection of up to nine separate antennas through a single coaxial cable as well as direction changing of antenna arrays and automatic pairing of antenna/transmitter sets.

For a copy, contact Microwave Filter Company, Inc., 6743 Kinne Street, East Syracuse, New York 13057.

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## simplex autopatch system

Hamtronics, Inc., has offered a Repeater Autopatch in kit form, including the DTMF Tone Decoder/Controller module for several years. They now have a new module that can be used with the Autopatch to allow operation on simplex transceivers. When an autopatch is used on a repeater, the duplex operation of the repeater allows the mobile operator to break into the telephone conversation anytime; when operating simplex - that is, transmitting and receiving on the same frequency - it is necessary to have a method to allow the mobile operator to access the base station receiver even though the base transmitter is on the same frequency.

The new AP-2 Simplex Autopatch Timing Module kit provides the required timing and logic circuits to allow the mobile operator to bring up the autopatch through touch-tone control, and it keys the base station transmitter with an automatic window generator circuit, which breaks periodically to allow the receiver to listen for the mobile station. If the mobile station is on the air, the window generator stops the base transmitter for the duration of the mobile transmission so the mobile operator maintains complete con-
trol of the transmit-receive switching of the base transceiver. Window length is automatically adjusted to compensate for the characteristics of the transceiver for minimal disruption of mobile reception by the window in the base transmissions. The new AP- 2 module along with the basic Autopatch and DTMF Tone Decoder modules are priced at $\$ 200$. The system is also available wired and tested.

For more information, contact Hamtronics, Inc., 65 Moul Road, Hilton, New York 144689535.

Circle 1305 on Reader Service Card.

## terminal interface

Terminal Interface sends messages around the world using any personal or home computer. Compatible with any home computer, such as Heath's H-8 or H-89, Commodore, Atari, Radio Shack, Apple, or IBM, it sends or receives ASCII/Baudot RTTY and Morse Code messages at up to 300 Baud using any standard transceiver, TTY terminal or monitor, and a computer with the appropriate software.

Optional six-pole filters for the HD-3030 include a preselect filter that delivers strong, readable tones in the standard 170 Hz shift and print clearly even in a crowded band, as well as filters for 425 and 850 Hz audio shifts. Features include a crystal-controlled AFSK generator, capability for full FSK with equipped transmitters, true mark/space detection, oscilloscope tuning outputs, front panel LED bargraph tuning, and data and status indicators. TTL and RS-232C 1/O compatibility and a built-in loop supply are also included. A row of flag-type pushbuttons permits full up-front control of send and receive (including reverse shift) configurations. A convenient autostart relay energizes the rear panel AC receptacle for unattended start of the computer and/or printer, while an internal thershold adjustment sets the desired recognition level.

The Terminal Interface kit includes a mate for the DB-25 socket and a step-by-step assembly manual that supplies a pin-out and criss-cross interconnection chart.

Heath also offers Super CW and Super RTTY Terminal Interface software for use with their H-8 and H-89 computers.
For further details, contact Heath Company, Benton Harbor, Michigan 49022.

Circle /306 on Reader Service Card.

## self-contained, transportable HF antenna system

A self-contained, transportable log-periodic HF antenna system has been announced by Telex/Hy-Gain. The system, Model 5025, consists of the antenna, rotator, 60 foot ( 18.3 meter) telescoping tower, generator, and installation tools and hardware, all stowed on one tandemaxle trailer. The compact design permits all

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For additional information, contact Telex Communications, Inc., Hy-Gain CIM Department, 8601 N.E. Highway Six, Lincoln, Nebraska 68505.

## microprocessor controlled repeater

The new SCR2000X microprocessor-controlled repeater from Spectrum Communications includes full autopatch and touch-tone repeater remote control capability and patch AGC for constant levels, as well as phone line and "over-theair" command modes.

Able to store up to 13 "auto dial" phone numbers, the unit includes a touch-tone to dial pulse converter and offers full 16 -digit decoding with crystal controlled decoder IC, allows the use of "A, B, C, and D" characters in control codes. This expands the number of possible codes and increases security.

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The following transmitter options are available: 2 meters: 30 or 75 watts; $220 \mathrm{MHz}: 30$ or 65 watts; $440 \mathrm{MHz}: 40$ watts. High power rack mount repeater power amps and power supplies are available to 150 watts.

A high-performance receiver is included, with high sensitivity, selectivity and wide-dynamic range. An 8 -pole front end filter is standard as well as a 12 -pole IF filter. "Super Sharp" filter options are also available.

For further details, contact Spectrum Communications Corp., 1055 W. Germantown Parkway, Norristown, Pennsylvania 19401-9616.

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HAM TRADER WEST classifieds, 25 cents a word for subscribers, $\$ 9$ a year bimonthly, Canadians $\$ 11.50$, posted same day as U.S. from Canada. Others 50 cents a word, commercial 75 cents a word. Name, address, and phone free. Ham Trader West. Box 202, Lynden, Wash 98264.
TRAVEL-PAK QSL KIT - Converts post cards, photos to QSLs. Stamp brings circular. Samco, Box 203-c, Wynantskill, New York 12198.
ULTIMATE CW FILTER: Four pole Gaussian response with variable selectivity and center frequency. Includes audio amplifer. See October 1983 OST, page 14. Complete PC assembly kil only $\$ 21$ postpaid. Orders or information: Analog Technology, Box 8964, Fort Collins, CO 80525.
RADIO ITEMS before 1930 wanted Buying battery operated radios, horn and cone speakers, radio tubes and parts, radio literature - books, catalogs, magazines, radio advertising signs, posters. Gary Schneider, 6848 Commonwealth Blvd., Parma Heights, Ohio 44130.
CUSTOM MADE embroidered patches. Any size, shape, colors. Five patch minimum. Free sample, prices and ordering information. Hein Specialties, Inc., Dept. 301, 4202 N. Drake, Chicago, IL 60618.
DIGITAL AUTOMATIC DISPLAYS for FT-101's TS-520's, and most others. Six $1 / 2^{\prime \prime}$ digits. Write for information. Grand Systems, P.O. Box 2171, Blaine, Washington 98230. (604) 530-4551.
SQUIRES SANDERS, SSIR (701 series); SS1V-SSi-S, SS1-MS mint condition. Factory manuals and other parts. Heath HX-10 transmitter with accessories, HO-10 scope. Icom IC-280 FoMoXceiver, Kenwood TR-2400. All in excellent condition with manuals. (616) 382-5401. K8WPQ, 9549 No. 17, Kalamazoo, MI 49007.
RUBBER STAMPS: 3 lines $\$ 4.50$ PPD. Send check or MO to G.L. Pierce, 5521 Birkdale Way, San Diego, CA 92117. SASE brings information.
FOR SALE: Kenwood TS-520 still in box. Operated once to check out. Great buy $\$ 400.00$. MFJ antenna tuner $\$ 15.00$. HyGain 18 AVT vertical antenna $\$ 20.00$. Ham Radio magazines back to $1980 \$ 1.00$ each. Call Warren (617) 335-7756 nights 7 PM to 10 PM . No calls on Sundays please.
FOR SALE: Swan 350 transceiver w/ps $\$ 250$. SA2040 antenna tuner $\$ 125$. QF-1A audio filter $\$ 50$. Kantronics CW/RTTY interface for Vic-20 with programs board + cables $\$ 135$. Shipping included. Send money order. Package price $\$ 500$. Write ping included. Send money order. Package price \$500. Wrie 637-0313 evenings.
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PORTABLE 2-meter Quads and J-Verticals. Write Radio Engineers, 3941 Mt. Brundage Avenue, San Diego, CA 92111.

RECONDITIONED TEST EQUIPMENT $\$ 1.00$ for catalog Walter, 2697 Nickel, San Pablo, CA 94806.
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# Coming Events ACTIVITIES 

"Places to go..."
PENNSYLVANIA: The Irwin Area ARA will sponsor a Swap \& Shop. Saturday, October 20, Circleville V.F.D., off Rt. 30, 3.5 miles west of Pennsylvania Turnpike, exit 7 . Talk in on 325/925 and 52. For information: Don Myslewski, K3CHD. 359 McMahon Road, North Huntingdon, PA 15642. (412) 863-0570.
LOUISIANA: The Twin City Hams are sponsoring a Hamfest, Saturday, November 10, Convention Center, West Monroe. Swap tables, new dealers, exams, ladies' events. All indoors. Talk in on 146.25/85. Contact: Benson Scott, AE5V, 107 Contempo, West Monroe, LA 71291.
TENNESSEE: Hamfest Chattanooga and the Tennessee State ARRL Convention, October 27 and 28, Memorial Auditorium, Oak Street at Lindsay Avenue, Chattanooga. Forums, contests and non-ham activities. Amateur exams Saturday morning. October 27, at 8 AM, Tech through Extra. Eight foot flea ing. October 27, at 8 AM, Tech through Extra. Eight foot lea
market tables indoors available $\$ 6.00$ per day or $\$ 10.00$ both market tables indoors available $\$ 6.00$ per day or $\$ 10.00$ both
days. For information: Hamfest Chattanooga, PO Box 3377 , Chattanooga, TN 37404 or call Nita Morgan, N4DON. (404) 820-2065.
KANSAS: Sandhills ARC's Swaplest, Sunday, October 7, 4-H Building, Scott County Fairgrounds, Scott City. Doors open 9 AM. Talk in on 146.10/.70. Covered dish lunch.
geORgia: Rome Hamtest (the South's oldest) will be held Sunday, October 1, Civic Center, Rome. Starts 8 AM. Talk in on $147.90 / 30$ Contact: T.J. Freeman, (404) 232-2830.
OHIO: The Marion Amateur Radio Club's 10th annual "Heart of Ohio" Ham Fiesta, Sunday, October 28, 0800 to 1600 , Marion County Fairgrounds Coliseum. Tickets $\$ 3.00$ advance. $\$ 4.00$ door. Tables $\$ 5.00$. Plenty of parking, food. Check in on 146.52 or $147.90 / 30$. For information, tickets or tables: Paul Kilzer, W8GAX, 393 Pole Lane Road, Marion, Ohio 43302.
NEW MEXICO: The UNM ARC and Westside ARC are cosponsoring a tailgate swaptest, November 3, 10 AM to 2 PM MST. UNM North Campus parking lot, corner of University Blvd. and Tucker Avenue, Albuquerque. No charge. Bring own tables. Talk in on 147.75/147.15 and 449.3/444.3 repeaters. For further information SASE to K8BI, WB5YYX or WA5WHN or via $3.939 \mathrm{MHz}, 0100$ UTC daily.
MICHIGAN: The Blossomland Amateur Radio Association's 1984 Blossomland Blast, Sunday, October 7, Lake Michigan College Community Center, 1-94 exit 30, west of Benton Harbor. 8 AM to 3 PM EDT. Admission $\$ 3$ per person. Special teatures: Air Force MARS display. Skywarn training program, RC airplane display. Talk in $22 / 82$ and 52. For table space: BARA, POB 175, St. Joseph, M1 49085 or Paul, WD8MWT (616) 983-1710.

ILLINOIS: Third annual CCRL Hamtest, Sunday, October 21, 7 AM to 2 PM, American Legion Post \#21, 6040 N. Clark St., Chicago. Admission $\$ 1.00$ advance, $\$ 1.50$ at door. $\$ 2.00$ per table. Talk in on 145.030 simplex. For information: Norman Geuder, KA9EZA, John Ibes, KA9FUI or Frank Bonnell, WB9OHN.

MASSACHUSETTS: The Framingham Amateur Radio Assocition's annual Fall flea market, Sunday, October 28, Framingham Civic League Bidg., 214 Concord Street, Framingham. Doors open 10 AM. Sellers setup 8:30. Admission $\$ 2.00$. Tables $\$ 10.00$ pre-registration only. Bargains galore. Talk in on 75/15 and 52. Contact: Jon Weiner, K1VVC, 52 Overlook Drive, Framingham, MA 01701. (617) 877-7166.
NEW ENGLAND: Hosstraders' Fall Tailgate Swaptest, Saturday, October 6, sunrise to sunset at Deerfield, NH Fairgrounds. Admission $\$ 2$ including tailgaters. Friday night camping at nominal fee after 4 PM. No reservations. Profits benefit Boston Burns Unit of Shriners Hospital. Last Spring's donation $\$ 5,813.00$. For map to northeast's biggest ham flea market SASE to Norm, WA1IVB, RFD Box 57, West Baldwin, ME 04091.

## OPERATING EVENTS

## "Things to do..."

OCTOBER 6-14: Special event stations K5MHZ and KN5D will operate during the 13th annual International Hot Air Balloon Fiesta in Albuquerque, New Mexico. Most operations SSB with some RTTY, CW and SSTV. Variable hours. Frequencies: $3900,7230,14250,21350$ and 28550 and 147.510 simplex FM. For a special OSL send QSL to PO Box 997, Corrales, NM 87048 . Include SASE with sufficient postage.
OCTOBER 6: Southeastern Michigan ARA will sponsor Michigan All Saints Day, 1500Z to 2100 Z with stations in all 9 cities named after Saints. Phone only, General portions of 20, 40 and 80 meters plus 147.480 and/or nearest repeater. Look for St. Joseph, KC8JX, St. Helen NBBAR, St. Johns NIBL, St. Clair W8GV, St. Charles WB8TTA, St. Ignace KD8CW, St. Louis WABAEG, St. James KD8CG and Sault Sainte Marie WA8DLO. QSL once with 110 SASE and log to N8COY, 161 Lothrop, Grosse Pointe, MI 48236 for certificate with endorsements.

OCTOBER 16, 17, 18: Colquitt County Ham Radio Society will operate club station WD4KOW from the site of the 7th annual Sunbelt Agricultural Exposition. 0900 to 1700 EDST each day. Operations: General portion of HF bands. Members will listen for visiting hams on 146.19/.79. For a special QSL card send SASE to: CC Ham Radio Society, PO Box 813, Moultrie. GA 31776.

OCTOBER 27 AND 28: Members of the Rutherford Appleton Laboratory ARC (G3RRS) will be active from VP2MF during this years contest. Operators: G3SJK, G3UKS, GM3YOR, G4BGH, G4JVG, G4XRI, G4XRJ. An award for DX stations working VP2MF on $10-160 \mathrm{~m}$ during the contest will be issued QSL via bureau or to G3RRS, c/o Jean Mills, R20, Rutherford Appleton Laboratory ARC, Chilton, Didcot, Oxon, UK.

OCTOBER 20 AND 21: The Armadillo Gang will operate WD5HOR to commemorate the Arkansas Pass "Shrimporee" Operation will be on $10,15,20,40,80$ meters 15 kc from lower General band edges. QSL card available via SASE to the Armadillo Gang, WB5YPE, David Stephens, 5709 Bobalo, Corpus Christi, TX 78412.

NOVEMBER 25 AND 26: The BOMB Squad (Best of Mt. Baidy) will operate W6HCP (Hollywood Christmas Parade) from 1600Z, November 25 to 0400Z, November 26. Frequencies: $7.284,14.284$, and 21.284 MHz SSB. SASE to W6GVR for special commemorative QSL.
OCTOBER 14: LARC will operate special event station WA3QGA from $1300 Z$ to $2400 Z$ to commemorate the Bollman Truss RR Bridge - the only one of its kind in the world. Frequencies: 7237, 14285, 21385, 144.250 USB and 147.540 simplex. Certificate available for " 10 SASE to LARC, PO Box 3039, Laurel, MD 20708.

OCTOBER 21, 22: JOTA - Scouts 27th annual Jamboree on the Air. Look for K2BSA, the BSA headquarters station in Dallas, Texas and HB9S, the World Scout Headquarters in Switzerland and other special call signs from many countries Calling frequencies: $\mathrm{CW}-3590,7030,14070,21140,28190$. Voice - 3940, 7290, 14290, 21360, 28990. RTTY, SSTV, ATV on usual trequencies. Check Novice trequencies. Do a good turn for Scouting and Ham Radio.
NOVEMBER 3: K4MJN will operate a special events station in Blythewood, SC, to commemorate the birthplace of J Gordon Coogler, acclaimed by literary critics as the "worst practicing poet in U.S. literary history!". All stations working K4MUN during this second annual festival will receive a handsome certificate with a photo of "The Bard of Blythewood" and some of his poetry. Please send QSL and contact number with large SASE to K4MJN, Rt. 3, Box 154, Blythewood, SC 29016. 14.290 MHz from 1400Z to 1800 Z and 21.390 MHz from 1800Z to 2200Z.

OCTOBER 20: The 24th Infantry Division Association will sponsor a special event station K4TF, to commemorate the 40th anniversary of the landing in the Philippines. A special commemorative certificate to any Amateur station making

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2-way contact with K4TF during the 24-hour GMT period. Operations will be 10 kHz inside the General portion of each band. For certificate send QSL card and $9 \times 12$ SASE to K4TF, 1630 Venus Street, Merritt Island, Florida 32953.

AMSAT Technical Symposium and General Membership Meeting, Sunday, November 10, Amfac Hotel, 8601 Lincoln Blvd., Los Angeles, CA 90045. Tech presentations on present/future Amateur satellite projects. General membership meeting following a banquet dinner. For conference registration information SASE to Dennis Dinga, N6DD, PO Box 4111 , Diamond Bar, CA 91765.

OCTOBER 13 AND 14: Oregon QSO party sponsored by the Hermiston ARC, 1700Z Oct. 13 to 0800Z and from 1500Z Oct 14 to 0000 Z Oct. 15. Exchange: OR stations, signal report and county. Others signal report and state/province/country. Mixed mode or CW only. You may obtain log sheets from HARC (please SASE). Log sheets must be received by November 12. Mail entries and request log sheets from: Hermiston ARC, PO Box 962. Hermiston, OR 97838.

OCTOBER 13 AND 14: QRP Amateur Radio Club International Fall QSO Contest. 1200 UTC Oct. 13 to 2400 UTC Oct. 14. 24 hours max. operation. Only one mode of operation, CW or SSB may be used. Exchanges: Members give RS(T). state/province/country and QRP ARCI membership number. Non-members give RS(T), state/province/country and power output. Logs must be received by November 12. Send all material to: QRP ARCI Contest Chairman, Gene Smith, KA5NLY, 8201 Chatham Drive, Little Rock, AR 72207.

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808 N. Main Street - Evansville, IN 47711 - NEW IC-02A/T

ICOM's new IC-02A/T represents the latest in state-of-the-art handheld radios. The IC-02A/T uses a microprocesser to control this radio. The IC-02A/T will scan, has 10 memories, stores offset frequency in memory. has keyboard selectable PL tones and an internal lithium battery memory back up.
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Call Ham Shack today for more information and your price on this and the rest of the

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For superior performance at lower cost, use toprated 8 -pole Fox Tango crystal filters to fill the optional spots in your rig. For example, our 1800 Hz FT2808 equivalent of the YK88SN has $60 / 6 \mathrm{~dB}$ shape factor of 1.7 compared with 2.0 , a price of $\$ 55 \mathrm{vs} \$ 63$, and squarer shoulders at the top with steeper skirts all the way down to more than -80 dB !
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Fox Tango filters are better because of their discrete crystal (not monolithic) construction. This makes them slightly larger than YK filters so they are patched into the circuit with short lengths of coax Installation is easy-no drilling or circuit changes. Order with confidence.

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Have the power you need when you need it with Yaesu's new 5-watt. 2 -meter handheld Power to get out in situations where ordinary HTs just won't make it.

We designed our HT with a unique userprogrammable Power Saver that puts the rig to "sleep" while youre monitoring and "wakes it up" when the squelch breaks. So you can listen for hours and still have plenty of power to hit those hard-to-reach repeaters when you need to.

With the FT-209RH there's no need to fiddle with knobs when you change from one memory channel to another. That's because you can independently store everything you need in each of the ten memories: receive frequency, standard or non-standard offset, even tone encode decode with an optional module And then recall any channel at the touch of a button.

It's easy to hear what's happening on your favorite repeaters or simplex frequencies. Just touch a button and scan all memory channels. or selected ones. Or all frequencies between any two adjacent memories. Use the prionty feature to return automatically to your special frequency when it becomes active

Bring up controlled-access machines with the optional plug-in subaudible tone encoder/ decoder independently programmed from the keyboard for each channel Listen for toneencoded signals on selected channels - without having to hear a bunch of chatter - by enabling the decode function.

The FT-209RH which covers 10 MHz for CAP and MARS use, comes complete with a 500-mAh battery charger and soft case.

For those who want a basic radio without the bells and whistles. consider the compact. lightweight FT-203R. This economical HT features 2.5 watts of power and an optional DTMF keypad. Most all the accessories for the 209 work with the 203. including an optional VOX headset that gives you hands-free operation that's perfect for public service events.

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## Digital Code Squelch...

## TR-2600A

Kenwood's TR-2600A introduces DCS (Digital Code Squelch) circuitry, a signaling concept developed by Kenwood. DCS allows each station to have its own
"private call" code or to respond to a "group call" or "common call" code. There are 100,000 different 5 -digit ASCII code combinations possible. You can program in call signs up to 6 digits in the ASCII code. When operating in the DCS mode, this information can then be automatically transmitted each time the transmit key is depressed. This revolutionary feature is only the beginning! The TR-2600A also sports a high impact plastic case, that is extra rugged and scuff-resistant. The molded-in color adds to the attractive appearance. The large L.C.D. display is easy to read in direct sunlight or in the dark with a convenient lamp switch. It displays transmit/receive frequencies, memory channels, and five arrow indicators for "F LOCK" frequency lock, "REV" repeater reverse, "PROG.S" programmed scan, "MS" memory scan,
"ALERT.S" alert scan. A star indicates "MemORY LOCK-OUT" is activated, and repeater offset indicated by ",,$+- S$ and $M$." The TR-2600A has 10 memories, nine for simplex or transmit with frequency offset $\pm 600 \mathrm{kHz}$ and one (memory 0 ) for non-standard split frequencies. Memory scan and programmable band scan have the added convenience of "Time operated Resume" that stops on busy channel and holds for approximately 5 seconds, then resumes scanning, or "Carrier Operated Resume" that stops on busy channel and resumes when signal ceases. Memory scan, scans only those memories in which data is stored, and memory lock-out allows you to skip selected memory channels

without loss of data previously stored! Manual Scanning UP/ DOWN in $5-\mathrm{kHz}$ steps and programmable automatic band scan are also useful features. The TR2600A has a built-in "S" meter on the top panel which also indicates battery level when in fransmit mode. Extended frequency coverage, $142.000-148.995 \mathrm{MHz}$ allows transmit capability in $5-\mathrm{kHz}$ steps for simplex or repeater operation on most MARS and CAP frequencies. Receive frequency coverage includes $140.000-159.995 \mathrm{MHz}$.

These features only tell part of the story. The TR-2600A also has keyboard frequency selection, built-in 16-key autopatch encoder, "TX STOP" switch. HI (2.5)/LOW ( 300 mw ) power switch, REV switch. "SLIDE-LOC" battery pack, high efficiency speaker, BNC antenna terminal, and all of this in an extremely compact and lightweight package!

Kenwood's TR-2600A, with D.C.S., leads the way in high technology handheld transceivers!

## Optional accessories:

- TU-35B built-in programmable
sub-tone encoder
- ST-2 Base Stand
- MS-1 Mobile Stand
- PB-26 Ni-Cd Battery
- DC-26 DC-DC Converter
- HMC-1 Headset with VOX
- SMC-30 Speaker Microphone
- LH-3 Deluxe Leather Case
- SC-9 Soft Case
- BT-3 AA Manganese/Alkaline Battery Case
- EB-3 External C Manganese/ Alkaline Battery Case
- RA-3, 5. Telescoping Antenna
- CD-10 Call Sign Display

More information on the
TR-2600A is available from
authorized dealers of
Trio-Kenwood Communications, 1111 West Walnut Street.
Compton, CA 90220.


[^0]:    - A comprehensive report on all aspects of this situation, including those parts of the actual petitions pertaining to land mobile interest in the 220 band is available in the latest issue of 220 Notes. (308 Eastgate Court, New Lenox, Illinais 60451 - Single copy, $\$ 1.25$; yearly subscription, \$5.)

[^1]:    table 1. Proposed 220 to 225 MHz band plan. (Submitted by Joe Reisert, W1JR, Chairman VUAC.)
    trequency ( $\mathrm{MHz}_{2}$ )
    220.0-220.05 EME (Earth-Moon-Earth)
    220.05-220.06 propagation beacons
    220.06-220.1 weak signal CW
    220.1
    220.1-220.5 general weak-signal, rag chewing and experimental
    220.5-221.9 experimental and control links
    221.9-222.0 weak-signal guard band (Note 2)
    222.0-222.05 EME (Note 2)
    222.05-222.06 propagation beacons (Note 2)
    222.06-222.1 weak-signal on CW (Note 2)
    222.1
    222.1-222.3 general operation CW or SSB etc. (Note 2)
    222.3-222.38 FM repeater inputs (Note 3)
    222.42-223.9 FM simplex (Note 4)
    223.94-225.0 FM repeater outputs (Note 3)

    Notes:

    1. After establishing contact QSY at least 10 kHz up or down for general rag chewing or weak-signal operation.
    2. This area is primarily needed where TV channel 13 spillover and long-distance search radars are in operation (e.g., California area).
    3 This is the existing ARRL Repeater Plan. 1.6 MHz splits.
    3. 223.5 is the national calling frequency for FM simplex. Alternative frequencies in 20 kHz increments in this region.
[^2]:    *Note that " $D$ ", rather than ham radio 's customary "CR", is used to designate diodes in this article and accompanying artwork.

[^3]:    *Courtesy Beckman Instruments, Inc., 2500 Harbor Blvd., Fullerton, California 92634.

[^4]:    1. Joseph M. Boyer, W6UYH, "The Multi-Band Trap Antenna," CQ, February, March, April, May, 1977, pages 26, 51, 46, 22 respectively. 2. Robert H. Johns, W3JIP, "Coaxial Cable Antenna Traps," QST. May, 1981, page 15.
    2. R.P. Haviland, "Trap Antenna," HP Library Program 97-04766-2, Corvallis, Oregon.
[^5]:    estimated average retail price

    - Gain and F/B ratio cannot be published in QST. They are included in Cushcraft specification sheets and other publications.

[^6]:    QUALITY STEEL PRODUCTS BY
    ROHN
    manan U.S.A.

[^7]:    *International Crystals, P.O. Box 26330, Oklahoma City, Oklahoma 73126.

[^8]:    *See "The VHF/UHF Primer: An Introduction to Propagation," by Joe Reisert, W1JR, ham radio, July, 1984, page 14, for a comprehensive survey of the VHF/UHF modes.
    tHFers experience that same frustration. - Editor.

[^9]:    *Available from the author at nominal cost.

[^10]:    
    6743 Kinne St., East Syracuse, NY 13057 Toll Free 1-800-448-1666 TWX 710-541-0493 NYIHI/AK/Canada (Collect) 315-437-3953

[^11]:    *We regret that neither the author nor the staff of ham radio can provide software assistance or consultation.

[^12]:    $\square 21874$ Hardbound

[^13]:    FOX TANGO CORPORATION
    Box 15944 H, W. Palm Beach, FL 33416 (305) 683.9587

